OPTIMISATION AND IMPLEMENTATION OF FUZZY CONTROLLERS FOR POWER SYSTEM STABILISATION

by

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Optimisation and implementation of fuzzy controllers for power system
To my family
# Contents

<table>
<thead>
<tr>
<th>Section</th>
<th>Page</th>
</tr>
</thead>
<tbody>
<tr>
<td>Contents</td>
<td>i</td>
</tr>
<tr>
<td>List of Figures</td>
<td>ix</td>
</tr>
<tr>
<td>List of Tables</td>
<td>xxiii</td>
</tr>
<tr>
<td>List of Principal Symbols and Abbreviations</td>
<td>xxvi</td>
</tr>
<tr>
<td>Abstract</td>
<td>xxxiv</td>
</tr>
<tr>
<td>Statement of Originality</td>
<td>xxxvii</td>
</tr>
<tr>
<td>Preface</td>
<td>xxxviii</td>
</tr>
<tr>
<td>Acknowledgements</td>
<td>xl</td>
</tr>
<tr>
<td>1 Introduction</td>
<td>1</td>
</tr>
<tr>
<td>1.1 Excitation Control and Its Role on Power System Stability</td>
<td>1</td>
</tr>
<tr>
<td>1.2 The Definition of Power System Stability</td>
<td>4</td>
</tr>
<tr>
<td>1.3 The Application of Power System Stabilisers (PSSs)</td>
<td>5</td>
</tr>
<tr>
<td>1.4 Conventional Power System Stabilisers (CPSSs)</td>
<td>7</td>
</tr>
</tbody>
</table>
## Contents

1.5 Adaptive Power System Stabilisers ........................................ 8
1.6 Fuzzy Logic and Fuzzy Control ........................................... 10
1.7 The Application of Fuzzy Controllers as PSSs ......................... 13
1.8 Motivation for the Thesis .................................................. 14
1.9 Contributions of the Thesis ............................................... 16
1.10 Organisation of the Thesis ............................................... 17

2 Experimental Systems Used in the Power Laboratory .................. 20
   2.1 Introduction ..................................................................... 20
   2.2 Single-machine Infinite Bus Power System ......................... 20
   2.3 Two-machine Infinite Bus Power System ............................. 23

3 Excitation Control System Design ........................................ 26
   3.1 Introduction ..................................................................... 26
   3.2 Mathematical Modelling of the Experimental System ............. 27
   3.3 Discrete-time Analytical Design Method ............................. 31
   3.4 Digital Automatic Voltage Regulator (AVR) Design .............. 34
   3.5 Experimental Test Results ............................................. 37
   3.6 Concluding Remarks ..................................................... 39

4 Proposed Design of Two Fuzzy Control Schemes ....................... 45
   4.1 Introduction ..................................................................... 45
   4.2 Introduction to Fuzzy Logic Controller (FLC) ...................... 45
4.2.1 Structure of the FLC ........................................ 45
4.2.2 Data Base .................................................. 48
4.2.3 Rule Base .................................................. 51
4.2.4 Defuzzification Strategies .............................. 53
4.2.5 Design Parameters of the FLC ......................... 55
4.3 Design of a FLC as a PSS ................................. 55
4.4 Design of the Proposed Fuzzy Logic Based PSS (FLBPSS) ........ 64
4.5 Concluding Remarks ................................. 69

5 Optimisation of the Fuzzy Control Strategy 70

5.1 Introduction .............................................. 70
5.2 Optimisation of the FLC by Observation of Model Behaviour ........ 71
  5.2.1 Optimisation of the FLC using Whole Overlap Ratio (WOR) . 71
  5.2.2 Sensitivity to Nominal Parameter Variations and Robustness to Operating Condition Variations ............. 75
5.3 Optimal Setting of the FLBPSS Parameters and Sensitivity Analysis 80
  5.3.1 Optimal Setting of the FLBPSS Parameters .................. 80
  5.3.2 Robustness to Operating Condition Variations and Sensitivity to Nominal Parameter Variations ............. 93
5.4 Comparison of the Proposed FLBPSS and Hassan’s Self-tuned FLBPSS 96
  5.4.1 Review of Hassan’s Self-tuned FLBPSS (STFLBPSS) ........ 96
  5.4.2 Optimal Setting of the STFLBPSS Parameters .............. 98
5.4.3 Comparison of the Performance Index .... 98
5.4.4 Comparison of the Dynamic Response .... 99
5.5 Comparison Study of the Two Fuzzy Control Schemes .... 101
  5.5.1 Comparison of the Performance Index .... 101
  5.5.2 Comparison of the Dynamic Response .... 102
5.6 Concluding Remarks .... 102

6 Implementation Study .... 112

6.1 Introduction .... 112
6.2 Hardware Development .... 113
  6.2.1 Sensor .... 113
  6.2.2 A/D and D/A Adapter .... 114
  6.2.3 Field Drive Unit .... 114
  6.2.4 Rotor Position Measurement by Using an Optical Shaft Encoder .... 114
6.3 Software Development .... 115
  6.3.1 The Main Program .... 115
  6.3.2 The Driver Routines .... 116
  6.3.3 The Interrupt Set up and Handling Routines .... 116
  6.3.4 The FLBPSS Routine .... 116
  6.3.5 The AVR Routine .... 117
  6.3.6 Screen Graphics .... 117
  6.3.7 Other Features .... 117
6.3.8 The Block Diagram of the Software .................................. 117

6.4 Implementation Tests ......................................................... 117

6.4.1 Step Change in the Reference Voltage ................................ 119

6.4.2 Sudden Load Change ....................................................... 119

6.4.3 Three-phase to Ground Fault ........................................... 121

6.5 Concluding Remarks ........................................................... 127

7 Application of the FLBPSS to Multi-machine Systems ............... 131

7.1 Introduction ........................................................................ 131

7.2 AVR Design ....................................................................... 133

7.2.1 Design of the AVR for Generator 1 .................................. 133

7.2.2 Design of the AVR for Generator 2 .................................. 133

7.2.3 Practical Evaluation of the Designed AVRs ......................... 135

7.3 The Design and Optimisation of the FLBPSS ......................... 136

7.4 Simulation Results for the FLBPSS ....................................... 136

7.5 Implementation and Test Results for the FLBPSS .................. 137

7.5.1 Step Change in the Reference Voltage at Generator 1 Side .... 137

7.5.2 Rated Load Change ......................................................... 137

7.5.3 Test Results Under Different Operating Conditions ............ 148

7.5.4 Three-phase to Ground Fault ........................................... 148

7.5.5 Transmission Line Loss Between Generators 1 and 2 .......... 157

7.6 Concluding Remarks ............................................................. 159
8 Rules Reduction for the FLC Using Neural Networks

8.1 Introduction .......................... 161
8.2 Rules Reduction for the FLC Using Neural Networks .......... 163
8.3 Comparison Study .............................. 166
8.4 Concluding Remarks .............................. 170

9 Conclusions

9.1 A Retrospective Overview of the Thesis ..................... 171
9.2 Avenues to be Explored in Further Work .......................... 178

A Mathematical Model of the Synchronous Machine

A.1 Mathematical Model of the Synchronous Machine ............. 181
A.1.1 Flux Linkage Equations .......................... 182
A.1.2 Voltage Equations .............................. 184
A.1.3 Torque and Power Equations ......................... 185
A.1.4 Swing Equation ............................... 186
A.1.5 Load Equation ................................. 186
A.1.6 Formulation of State-Space Equations .................. 187
A.1.7 Current Model ................................. 188
A.2 Linearisation of the Non-linear Power System Model ........ 191
A.2.1 Linearisation of the Generator State-Space Current Model . 191
A.2.2 Linearisation of the Load Equation for the Single-machine Infinite Bus Power System ............... 192
A.3 Simplified Linear Model .......................... 194

B Introduction to Fuzzy Set Theory .................. 201

B.1 Fuzzy Sets and Terminology ......................... 201
B.2 Fuzzy Set Theoretical Operations .................. 203
B.3 Linguistic Variables and Linguistic Hedges ........... 206
B.4 Fuzzy Inference and Composition .................. 208
B.5 Fuzzy Logic and Approximate Reasoning ............ 212

C The Whole Overlap Ratio (WOR) ..................... 214

C.1 The WOR for Linear Membership Functions .......... 214
C.2 The WOR for Quadratic Membership Functions ......... 216
C.3 The WOR for Gaussian Membership Functions .......... 219

D Mathematical Model for Multi-machine Power System ...... 222

D.1 Statement of the Problem .......................... 222
D.2 Conversion to a Common Reference Frame ............ 224
D.3 Conversion of Machine Coordinates to System Reference .... 226
D.4 Linearised Model for the Network .................. 228
D.5 Generator Equations ................................ 231

E The Input FPL File and the Generated Rule Base ....... 232

E.1 The Input FPL File .................................. 232
E.2 The Generated Rule Base ............................ 233
F Bibliography 241

List of Figures

2.1 The overall view of the single-machine infinite bus experimental power system ........................................... 22

2.2 Experimental circuit configuration of single-machine infinite bus power system ........................................... 23

2.3 The overall view of the two-machine infinite bus experimental power system ........................................... 24

2.4 Two-machine infinite bus power system .................................................. 25

3.1 Block diagram of the simplified linear model .................................................. 29

3.2 The voltage regulator loop ................................................................. 30

3.3 Unit step response of the voltage regulator loop ........................................... 37

3.4 Terminal voltage corresponding to 1/2 sudden inductive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR ........................................... 38

3.5 Terminal voltage corresponding to 3/4 sudden inductive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR ........................................... 40

3.6 Terminal voltage corresponding to 1/2 sudden capacitive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR ........................................... 40
List of Figures

3.7 Terminal voltage corresponding to 3/4 sudden capacitive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR .................................................. 41

3.8 Terminal voltage corresponding to 1/2 sudden resistive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR .................................................. 41

3.9 Terminal voltage corresponding to 3/4 sudden resistive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR .................................................. 42

3.10 Control signals corresponding to 1/2 and 3/4 sudden inductive load changes with the AVR, (a)-1/2 rated inductive load change, (b)-3/4 rated inductive load change ........................................ 42

3.11 Control signals corresponding to 1/2 and 3/4 sudden capacitive load changes with the AVR, (a)-1/2 rated capacitive load change, (b)-3/4 rated capacitive load change ........................................ 43

3.12 Control signals corresponding to 1/2 and 3/4 sudden resistive load changes with the AVR, (a)-1/2 rated resistive load change, (b)-3/4 rated resistive load change ........................................ 43

3.13 Terminal voltage and control signal corresponding to a 10% step increase in the reference voltage sustained for 7.5 seconds, (a)-terminal voltage, (b)-control signal ........................................ 44

3.14 Terminal voltage and control signal corresponding to a three-phase to ground fault at A (Figure 2.2) sustained for 125 milliseconds, (a)-terminal voltage, (b)-control signal ........................................ 44

4.1 Schematic diagram of a FLC ........................................ 46

4.2 Inappropriate universe of discourse ........................................ 57

4.3 Inappropriate output universe of discourse ................................. 58
4.4 Disproportionately large output membership function 59
4.5 Membership functions for both condition parts and consequent parts 60
4.6 Two sectors in the phase plane 65
4.7 The proposed non-linear membership functions 67
4.8 Gain factor related to distance $D(k)$ 68

5.1 Membership functions after tuning 72
5.2 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition for a 20% step change in mechanical torque ($\beta = -35$) 81
5.3 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition for a 20% step change in mechanical torque ($\beta = -38$) 81
5.4 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition for a 20% step change in mechanical torque ($\beta = -40$) 82
5.5 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition for a 20% step change in mechanical torque ($\beta = -42$) 82
5.6 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition in response to a three-phase to ground fault ($\beta = -35$) 83
5.7 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition in response to a three-phase to ground fault ($\beta = -38$) 83
5.8 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition in response to a three-phase to ground fault ($\beta = -40$) . . . . . . . . . . . . . . . . . . . . 84

5.9 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition in response to a three-phase to ground fault ($\beta = -42$) . . . . . . . . . . . . . . . . . . . . 84

5.10 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm20\%$ variation in inertia constant $H$ for a 20% step change in mechanical torque ($H = 1.2s, \beta = -35$) . . . . . . . . . . . . . 85

5.11 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm20\%$ variation in inertia constant $H$ for a 20% step change in mechanical torque ($H = 1.2s, \beta = -38$) . . . . . . . . . . . . . 86

5.12 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm20\%$ variation in inertia constant $H$ for a 20% step change in mechanical torque ($H = 1.2s, \beta = -40$) . . . . . . . . . . . . . 86

5.13 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm20\%$ variation in inertia constant $H$ for a 20% step change in mechanical torque ($H = 1.2s, \beta = -42$) . . . . . . . . . . . . . 87

5.14 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm20\%$ variation in inertia constant $H$ for a 20% step change in mechanical torque ($H = 0.8s, \beta = -35$) . . . . . . . . . . . . . 87

5.15 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm20\%$ variation in inertia constant $H$ for a 20% step change in mechanical torque ($H = 0.8s, \beta = -38$) . . . . . . . . . . . . . 88

5.16 Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm20\%$ variation in inertia constant $H$ for a 20% step change in mechanical torque ($H = 0.8s, \beta = -40$) . . . . . . . . . . . . . 88
5.17 Performance index corresponding to \( \alpha \) changes \( J = f(\alpha) \) with different \( D_r \) values and -20\% variation in inertia constant \( H \) for a 20\% step change in mechanical torque \( (H = 0.8s, \beta = -42) \) 89

5.18 Minimum performance index corresponding to changes in \( \beta \) values
\[ J_{\text{min}} = f(\beta) \] (20 \% step increase in mechanical torque) 89

5.19 Minimum performance index corresponding to changes in \( \beta \) values
\[ J_{\text{min}} = f(\beta) \] (three-phase to ground fault) 90

5.20 System response corresponding to a 20\% step change in \( T_m \) under two optimal settings 91

5.21 System response corresponding to a 20\% step change in \( T_m \) and a three-phase to ground fault, (a)-20\% step increase in mechanical torque, (b)-three-phase to ground fault 92

5.22 Performance index corresponding to changes in \( \alpha \) \( J = f(\alpha) \) with different \( D_r \) values in response to a 20\% step increase in \( T_m \) under operating condition P1 \( (\beta = -40) \) 93

5.23 Performance index corresponding to changes in \( \alpha \) \( J = f(\alpha) \) with different \( D_r \) values in response to a three-phase fault under operating condition P1 \( (\beta = -40) \) 94

5.24 Performance index corresponding to changes in \( \alpha \) \( J = f(\alpha) \) with different \( D_r \) values in response to a 20\% step increase in \( T_m \) under operating condition P4 \( (\beta = -40) \) 94

5.25 Performance index corresponding to changes in \( \alpha \) \( J = f(\alpha) \) with different \( D_r \) values in response to a three-phase fault under operating condition P4 \( (\beta = -40) \) 95

5.26 System responses at operating condition P4 with the corresponding optimal settings (COS) and the nominal optimal settings (NOS), (a)-20\% step increase in mechanical torque, (b)-three-phase to ground fault 105
5.27 System responses at P0 with inertia constant parameter variation $H = 1.2s$ with the corresponding optimal settings (COS) and the nominal optimal settings (NOS), (a)-20% step increase in mechanical torque, (b)-three-phase to ground fault...

5.28 System response corresponding to three-phase to ground fault under different operating conditions with the nominal optimal settings (NOS), (a)-operating conditions P0, P1, P2 and P4, (b)-operating condition P3...

5.29 System response corresponding to a 20% step increase in mechanical torque with the nominal optimal settings (NOS) for different system parameter changes, (a)-±20% variation in $H$, (b)-±20% variation in $\tau'_{d0}$...

5.30 Membership functions used for the STFLBPSS...

5.31 System response corresponding to a 20% step change in mechanical torque and a three-phase fault under the nominal operating condition, (a)-20% step increase in mechanical torque, (b)-three-phase fault...

5.32 System response corresponding to a 20% step change in mechanical torque under different operating conditions, (a)-(d) provide the speed deviation responses under operating conditions P1-P4 respectively...

5.33 System response corresponding to a three-phase to ground fault under different operating conditions, (a)-(d) provide the speed deviation responses under operating conditions P1-P4 respectively...

5.34 System response corresponding to a 20% step change in mechanical torque with ±20% variation in inertia constant $H$, (a)-$H = 1.2s$, (b)-$H = 1s$, (c)-$H = 0.8s$...

5.35 System response corresponding to a 20% step change in mechanical torque with ±20% variation in $\tau'_{d0}$, (a)-$\tau'_{d0} = 0.414s$, (b)-$\tau'_{d0} = 0.345s$, (c)-$\tau'_{d0} = 0.276s$...
<table>
<thead>
<tr>
<th>Figure</th>
<th>Description</th>
<th>Page</th>
</tr>
</thead>
<tbody>
<tr>
<td>5.36</td>
<td>System response corresponding to a 20% step change in mechanical torque with ( \pm 20% ) variation in ( X_e ), ( \text{(a)}-X_e = 0.48pu, \ (b)-X_e = 0.4pu, \ (c)-X_e = 0.32pu )</td>
<td>110</td>
</tr>
<tr>
<td>5.37</td>
<td>System response corresponding to a 20% step change in mechanical torque and reference voltage change (without PSS)</td>
<td>110</td>
</tr>
<tr>
<td>5.38</td>
<td>System response corresponding to a 20% step change in mechanical torque and reference voltage change (with the FLC)</td>
<td>111</td>
</tr>
<tr>
<td>5.39</td>
<td>System response corresponding to a 20% step change in mechanical torque and reference voltage change (with the FLBPSS)</td>
<td>111</td>
</tr>
<tr>
<td>6.1</td>
<td>Sensor circuit of rectifier, potential divider and filter circuit</td>
<td>113</td>
</tr>
<tr>
<td>6.2</td>
<td>Software diagram (Part I)</td>
<td>118</td>
</tr>
<tr>
<td>6.3</td>
<td>Software diagram (Part II)</td>
<td>118</td>
</tr>
<tr>
<td>6.4</td>
<td>Rotor angle and speed deviation corresponding to a 10% step increase in the reference voltage sustained for 7.5 seconds (without the FLBPSS), ( \text{(a)})-rotor angle, ( \text{(b)})-speed deviation</td>
<td>120</td>
</tr>
<tr>
<td>6.5</td>
<td>Rotor angle and speed deviation corresponding to a 10% step increase in the reference voltage sustained for 7.5 seconds (with the FLBPSS), ( \text{(a)})-rotor angle, ( \text{(b)})-speed deviation</td>
<td>121</td>
</tr>
<tr>
<td>6.6</td>
<td>Control signal corresponding to a 10% step increase in the reference voltage sustained for 7.5 seconds, ( \text{(a)})-without the FLBPSS and ( \text{(b)})-with the FLBPSS</td>
<td>122</td>
</tr>
<tr>
<td>6.7</td>
<td>Rotor angle and speed deviation corresponding to sudden resistive load change without the FLBPSS (operating condition OC1), ( \text{(a)})-rotor angle, ( \text{(b)})-speed deviation</td>
<td>123</td>
</tr>
</tbody>
</table>
6.8 Rotor angle and speed deviation corresponding to sudden resistive load change with the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation ............................... 123

6.9 Rotor angle and speed deviation corresponding to sudden inductive load change without the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation ............................... 124

6.10 Rotor angle and speed deviation corresponding to sudden inductive load change with the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation ............................... 124

6.11 Rotor angle and speed deviation corresponding to sudden capacitive load change without the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation ............................... 125

6.12 Rotor angle and speed deviation corresponding to sudden capacitive load change with the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation ............................... 125

6.13 Rotor angle and speed deviation corresponding to sudden resistive load change without the FLBPSS (operating condition OC2), (a)-rotor angle, (b)-speed deviation ............................... 126

6.14 Rotor angle and speed deviation corresponding to sudden resistive load change with the FLBPSS (operating condition OC2), (a)-rotor angle, (b)-speed deviation ............................... 126

6.15 Rotor angle and speed deviation corresponding to sudden resistive load change without the FLBPSS (operating condition OC3), (a)-rotor angle, (b)-speed deviation ............................... 128

6.16 Rotor angle and speed deviation corresponding to sudden resistive load change with the FLBPSS (operating condition OC3), (a)-rotor angle, (b)-speed deviation ............................... 128
6.17 Rotor angle and speed deviation corresponding to sudden resistive load change without the FLBPSS (operating condition OC4), (a)-rotor angle, (b)-speed deviation ................................. 129

6.18 Rotor angle and speed deviation corresponding to sudden resistive load change with the FLBPSS (operating condition OC4), (a)-rotor angle, (b)-speed deviation ................................. 129

6.19 Rotor angle and speed deviation corresponding to a three-phase fault at A (Figure 2.2) sustained for 125 milliseconds (without the FLBPSS), (a)-rotor angle, (b)-speed deviation ................................. 130

6.20 Rotor angle and speed deviation corresponding to a three-phase fault at A (Figure 2.2) sustained for 125 milliseconds (with the FLBPSS), (a)-rotor angle, (b)-speed deviation ................................. 130

7.1 Terminal voltage corresponding to a 10% step change in reference voltage at generator 1 side, (a)-terminal voltage for generator 1, (b)-terminal voltage for generator 2 ................................. 139

7.2 Terminal voltage corresponding to 3/4 rated inductive load change, (a)-terminal voltage for generator 1, (b)-terminal voltage for generator 2 ................................. 139

7.3 Terminal voltage corresponding to 3/4 rated capacitive load change, (a)-terminal voltage for generator 1, (b)-terminal voltage for generator 2 ................................. 140

7.4 Terminal voltage corresponding to 3/4 rated resistive load change, (a)-terminal voltage for generator 1, (b)-terminal voltage for generator 2 ................................. 140

7.5 Terminal voltage corresponding to a three-phase to ground fault, (a)-terminal voltage for generator 1, (b)-terminal voltage for generator 2 ................................. 141
List of Figures

7.6 Excitation control signal corresponding to a three-phase to ground fault, (a)-control signal for generator 1, (b)-control signal for generator 2 .................................................. 141

7.7 System response corresponding to a 10% step change in reference voltage and mechanical torque without PSS, (a)-speed deviation for generator 1, (b)-speed deviation for generator 2 .......................... 142

7.8 System response corresponding to a 10% step change in reference voltage and mechanical torque with the FLBPSS, (a)-speed deviation for generator 1, (b)-speed deviation for generator 2 .......................... 142

7.9 System response corresponding to a 20% step change in reference voltage and mechanical torque without the FLBPSS, (a)-speed deviation for generator 1, (b)-speed deviation for generator 2 .......................... 143

7.10 System response corresponding to a 20% step change in reference voltage and mechanical torque with the FLBPSS, (a)-speed deviation for generator 1, (b)-speed deviation for generator 2 .......................... 143

7.11 Rotor angle and speed deviation for generator 1 corresponding to a 10% step increase in the reference voltage at generator 1 sustained for 7.5 seconds (without the FLBPSS), (a)-rotor angle, (b)-speed deviation 144

7.12 Rotor angle and speed deviation for generator 1 corresponding to a 10% step increase in the reference voltage at generator 1 sustained for 7.5 seconds (with the FLBPSS), (a)-rotor angle, (b)-speed deviation 144

7.13 Rotor angle and speed deviation for generator 2 corresponding to a 10% step increase in the reference voltage at generator 1 sustained for 7.5 seconds (without the FLBPSS), (a)-rotor angle, (b)-speed deviation 145

7.14 Rotor angle and speed deviation for generator 2 corresponding to a 10% step increase in the reference voltage at generator 1 sustained for 7.5 seconds (with the FLBPSS), (a)-rotor angle, (b)-speed deviation 145
7.15 Rotor angle and speed deviation for generator 1 corresponding to sudden resistive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation .................................................. 146

7.16 Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden resistive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation .................................................. 146

7.17 Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden resistive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation .................................................. 147

7.18 Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden resistive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation .................................................. 147

7.19 Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden inductive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation .................................................. 149

7.20 Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden inductive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation .................................................. 149

7.21 Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden inductive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation .................................................. 150

7.22 Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden inductive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation .................................................. 150

7.23 Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden capacitive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation .................................................. 151
7.24 Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden capacitive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation ........................................ 151

7.25 Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden capacitive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation ........................................ 152

7.26 Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden capacitive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation ........................................ 152

7.27 Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden resistive load change without the FLBPSS (Operating condition OC1), (a)-rotor angle, (b)-speed deviation ................................. 153

7.28 Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden resistive load change without the FLBPSS (Operating condition OC1), (a)-rotor angle, (b)-speed deviation ................................. 153

7.29 Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden resistive load change with the FLBPSS (Operating condition OC1), (a)-rotor angle, (b)-speed deviation ................................. 154

7.30 Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden resistive load change with the FLBPSS (Operating condition OC1), (a)-rotor angle, (b)-speed deviation ................................. 154

7.31 Rotor angle and speed deviation for generator 1 corresponding to a three-phase fault at B (Figure 2.4) sustained for 125 milliseconds (without the FLBPSS), (a)-rotor angle, (b)-speed deviation ................................. 155

7.32 Rotor angle and speed deviation for generator 1 corresponding to a three-phase fault at B (Figure 2.4) sustained for 125 milliseconds (with the FLBPSS), (a)-rotor angle, (b)-speed deviation ................................. 155
List of Figures

xxi

7.33 Rotor angle and speed deviation for generator 2 corresponding to
a three-phase fault at B (Figure 2.4) sustained for 125 milliseconds
(without the FLBPSS), (a)-rotor angle, (b)-speed deviation

156

7.34 Rotor angle and speed deviation for generator 2 corresponding to
a three-phase fault at B (Figure 2.4) sustained for 125 milliseconds
(with the FLBPSS), (a)-rotor angle, (b)-speed deviation

156

7.35 Rotor angle and speed deviation for generator 1 corresponding to the
loss of the transmission line (without the FLBPSS), (a)-rotor angle,
(b)-speed deviation

157

7.36 Rotor angle and speed deviation for generator 2 corresponding to the
loss of the transmission line (without the FLBPSS), (a)-rotor angle,
(b)-speed deviation

158

7.37 Rotor angle and speed deviation for generator 1 corresponding to
the loss of the transmission line (with the FLBPSS), (a)-rotor angle,
(b)-speed deviation

158

7.38 Rotor angle and speed deviation for generator 2 corresponding to
the loss of the transmission line (with the FLBPSS), (a)-rotor angle,
(b)-speed deviation

8.1

159

Speed deviation and rotor angle corresponding to a 10% step increase
in mechanical torque followed by a 10% step increase in the reference
voltage sustained for 7.5 seconds with the original 49-rule FLC

8.2

. . .168

Speed deviation and rotor angle corresponding to a 10% step increase
in mechanical torque followed by a 10% step increase in the reference
voltage sustained for 7.5 seconds with the 24-rule FLC

8.3

168

Speed deviation and rotor angle corresponding to a 20% step increase
in mechanical torque followed by a 20% step increase in the reference
voltage sustained for 7.5 seconds with the original 49-rule FLC

. . .169


8.4 Speed deviation and rotor angle corresponding to a 20% step increase in mechanical torque followed by a 20% step increase in the reference voltage sustained for 7.5 seconds with the 24-rule FLC . . . . . . . . 169

C.1 Two adjacent linear membership functions . . . . . . . . . . . . . 215

C.2 Two adjacent quadratic membership functions . . . . . . . . . . . . . 217

C.3 Two adjacent exponential membership functions . . . . . . . . . . . . . 219

D.1 Two frames of reference for phasor quantities for a voltage $V_i$ . . . . 224
## List of Tables

<table>
<thead>
<tr>
<th></th>
<th>Description</th>
<th>Page</th>
</tr>
</thead>
<tbody>
<tr>
<td>2.1</td>
<td>Ratings of the single-machine infinite bus power system</td>
<td>21</td>
</tr>
<tr>
<td>2.2</td>
<td>Generator parameters</td>
<td>21</td>
</tr>
<tr>
<td>2.3</td>
<td>Ratings of the two-machine infinite bus power system</td>
<td>23</td>
</tr>
<tr>
<td>2.4</td>
<td>Generator parameters</td>
<td>23</td>
</tr>
<tr>
<td>4.1</td>
<td>The decision table</td>
<td>62</td>
</tr>
<tr>
<td>4.2</td>
<td>Comparison of the defuzzification methods</td>
<td>64</td>
</tr>
<tr>
<td>5.1</td>
<td>Some usual membership functions and WOR evaluation formulas</td>
<td>73</td>
</tr>
<tr>
<td>5.2</td>
<td>The performance index corresponding to changes in WOR (10% step change in $T_m$ and $V_{ref}$)</td>
<td>73</td>
</tr>
<tr>
<td>5.3</td>
<td>The performance index corresponding to changes in WOR (20% step change in $T_m$ and $V_{ref}$)</td>
<td>74</td>
</tr>
<tr>
<td>5.4</td>
<td>The performance index corresponding to changes in WOR with different defuzzification methods (20% step change in $T_m$)</td>
<td>75</td>
</tr>
<tr>
<td>5.5</td>
<td>The performance index corresponding to changes in WOR with different defuzzification methods (three-phase to ground fault)</td>
<td>75</td>
</tr>
<tr>
<td>5.6</td>
<td>The performance index corresponding to changes in WOR (Mamdani, Centroid, 20% step increase in mechanical torque)</td>
<td>76</td>
</tr>
<tr>
<td>Table</td>
<td>Description</td>
<td>Page</td>
</tr>
<tr>
<td>-------</td>
<td>-------------</td>
<td>------</td>
</tr>
<tr>
<td>5.7</td>
<td>The performance index corresponding to changes in WOR (Mamdani, Means of maximum, 20% step increase in mechanical torque)</td>
<td>76</td>
</tr>
<tr>
<td>5.8</td>
<td>The performance index corresponding to changes in WOR (Larsen, Centroid, 20% step increase in mechanical torque)</td>
<td>77</td>
</tr>
<tr>
<td>5.9</td>
<td>The performance index corresponding to changes in WOR (Larsen, Means of maximum, 20% step increase in mechanical torque)</td>
<td>77</td>
</tr>
<tr>
<td>5.10</td>
<td>The performance index corresponding to changes in WOR with different implication and defuzzification methods, three-phase to ground fault</td>
<td>78</td>
</tr>
<tr>
<td>5.11</td>
<td>Operating conditions</td>
<td>78</td>
</tr>
<tr>
<td>5.12</td>
<td>Performance index corresponding to changes in WOR under different operating conditions (Mamdani, Means of maximum or centroid, 20% step increase in mechanical torque)</td>
<td>78</td>
</tr>
<tr>
<td>5.13</td>
<td>Performance index corresponding to changes in WOR under different operating conditions (Larsen, Means of maximum or centroid, 20% step increase in mechanical torque)</td>
<td>79</td>
</tr>
<tr>
<td>5.14</td>
<td>Performance index corresponding to changes in WOR under different operating conditions (Mamdani, Centroid, three-phase to ground fault)</td>
<td>79</td>
</tr>
<tr>
<td>5.15</td>
<td>Performance index corresponding to changes in WOR under different operating conditions (Mamdani, Means of maximum, three-phase to ground fault)</td>
<td>79</td>
</tr>
<tr>
<td>5.16</td>
<td>Optimal settings of the FLBPSS for different operating conditions</td>
<td>95</td>
</tr>
<tr>
<td>5.17</td>
<td>Comparison of the performance index (small perturbation of a 20% step change in mechanical torque (T_m))</td>
<td>99</td>
</tr>
<tr>
<td>5.18</td>
<td>Comparison of the performance index (large perturbation of a three-phase fault at A of Figure (2.2) sustained for 125 milliseconds)</td>
<td>99</td>
</tr>
</tbody>
</table>
5.19 Comparison of the performance index for parameter changes (small perturbation of a 20% step change in mechanical torque $T_m$) .... 99

5.20 Comparison of the performance index for parameter changes (large perturbation of a three-phase fault at A of Figure (2.2) sustained for 125 milliseconds) .................................................. 100

5.21 Comparison of the performance index (small perturbation of a 20% step change in mechanical torque $T_m$) .................. 100

5.22 Comparison of the performance index (large perturbation of a three-phase fault at A of Figure (2.2) sustained for 125 milliseconds) ...... 100

5.23 Comparison of the performance index of the FLC and the FLBPSS (small perturbation of a 20% step increase in mechanical torque) . . . 101

5.24 Comparison of the performance index of the FLC and the FLBPSS (large perturbation of a three-phase to ground fault) ............... 102

6.1 Operating conditions for single-machine infinite bus power system .. 119

7.1 Operating conditions for two-machine infinite bus power system . . . 148

8.1 The decision table after learning ........................................ 166

8.2 The performance index corresponding to changes in WOR (20% step increase in mechanical torque followed by a 10% step increase in the reference voltage sustained for 7.5 seconds) ................. 167

8.3 The performance index corresponding to different mechanical torque changes .......................................................... 167
List of Principal Symbols and Abbreviations

Unless otherwise stated, the following definitions of the notation are applied throughout this thesis.

<table>
<thead>
<tr>
<th>Symbol or Abbreviation</th>
<th>Description</th>
<th>Defined in</th>
</tr>
</thead>
<tbody>
<tr>
<td>A</td>
<td>field drive unit gain</td>
<td>Section 3.2</td>
</tr>
<tr>
<td>a, b, c</td>
<td>phase identification</td>
<td>App.A</td>
</tr>
<tr>
<td>A, B, C</td>
<td>phase identification</td>
<td>6.2</td>
</tr>
<tr>
<td>A, B</td>
<td>linear continuous time system state matrix</td>
<td>App.A</td>
</tr>
<tr>
<td>AC</td>
<td>Alternative Current</td>
<td>2.2, 6.1</td>
</tr>
<tr>
<td>A/D</td>
<td>Analog to Digital</td>
<td>2.2, 6.1</td>
</tr>
<tr>
<td>abs</td>
<td>absolute value</td>
<td>5.2</td>
</tr>
<tr>
<td>arg</td>
<td>argument</td>
<td>4.2</td>
</tr>
<tr>
<td>AVQ</td>
<td>Adaptive Vector Quantisation</td>
<td>8.1</td>
</tr>
<tr>
<td>AVR</td>
<td>Automatic Voltage Regulator</td>
<td>1.1, 6.1</td>
</tr>
<tr>
<td>B</td>
<td>voltage sensor gain</td>
<td>3.2</td>
</tr>
<tr>
<td>CON</td>
<td>Concentration</td>
<td>App.B</td>
</tr>
<tr>
<td>COS</td>
<td>Corresponding Optimal Setting</td>
<td>5.3</td>
</tr>
<tr>
<td>CPSS</td>
<td>Conventional Power System Stabiliser</td>
<td>1.4</td>
</tr>
<tr>
<td>D</td>
<td>Damping constant</td>
<td>App.A, 3.3</td>
</tr>
<tr>
<td>D-D'</td>
<td>generator damper winding</td>
<td>App.A</td>
</tr>
<tr>
<td>D/A</td>
<td>Digital to Analog</td>
<td>2.2, 6.1</td>
</tr>
<tr>
<td>d-axis</td>
<td>direct axis</td>
<td>App.A, App.D</td>
</tr>
<tr>
<td>D(k), D_r</td>
<td>distance parameter</td>
<td>4.4</td>
</tr>
<tr>
<td>DC</td>
<td>Direct Current</td>
<td>2.2, 6.1</td>
</tr>
<tr>
<td>DIL</td>
<td>Dilation</td>
<td>App.B</td>
</tr>
<tr>
<td>EMF</td>
<td>Electromotive Force</td>
<td>App.A</td>
</tr>
<tr>
<td>E_{F_D}(t)</td>
<td>generator stator EMF</td>
<td>App.A</td>
</tr>
<tr>
<td>E_{F_D\Delta}(t)</td>
<td>linearised generator stator EMF</td>
<td>App.A</td>
</tr>
<tr>
<td>Symbol</td>
<td>Description</td>
<td>Page/Section</td>
</tr>
<tr>
<td>-----------------</td>
<td>------------------------------------------------------------------------------</td>
<td>--------------</td>
</tr>
<tr>
<td>$e(t), e(kT)$</td>
<td>error signal</td>
<td>3.3</td>
</tr>
<tr>
<td>$E_q(t)$</td>
<td>generator q-axis component of stator EMF</td>
<td>App.A</td>
</tr>
<tr>
<td>$E_d(t)$</td>
<td>generator d-axis component of stator EMF</td>
<td>App.A</td>
</tr>
<tr>
<td>$E'_q(t), e'_q(t)$</td>
<td>generator q-axis transient stator EMF</td>
<td>App.A</td>
</tr>
<tr>
<td>$E'_d(t)$</td>
<td>generator d-axis transient stator EMF</td>
<td>App.A</td>
</tr>
<tr>
<td>$E'_{q0}$</td>
<td>steady-state value of $E_q(t)$</td>
<td>App.A</td>
</tr>
<tr>
<td>$E'_{q\Delta}$</td>
<td>linearised generator q-axis transient stator EMF</td>
<td>3.2</td>
</tr>
<tr>
<td>$f$</td>
<td>a set of non-linear function</td>
<td>App.A</td>
</tr>
<tr>
<td>$F$</td>
<td>Fuzzy set</td>
<td>App.B</td>
</tr>
<tr>
<td>$F-F'$</td>
<td>generator field winding</td>
<td>App.A</td>
</tr>
<tr>
<td>FLC</td>
<td>Fuzzy Logic Controller</td>
<td>1.7, 4.2</td>
</tr>
<tr>
<td>FLBPSS</td>
<td>Fuzzy Logic Based Power System Stabiliser</td>
<td>1.7, 4.4</td>
</tr>
<tr>
<td>FNN</td>
<td>Fuzzy Neural Networks</td>
<td>9.2</td>
</tr>
<tr>
<td>FPL</td>
<td>Fuzzy Programming Language</td>
<td>8.2, App.E</td>
</tr>
<tr>
<td>$F(t)$</td>
<td>restore force of an inverted pendulum</td>
<td>8.1</td>
</tr>
<tr>
<td>$F(z)$</td>
<td>desired close loop pulse transfer function</td>
<td>3.3</td>
</tr>
<tr>
<td>$F_\alpha$</td>
<td>$\alpha$-cut of fuzzy set $F$</td>
<td>App.B</td>
</tr>
<tr>
<td>$F_\delta$</td>
<td>strong $\alpha$-cut of fuzzy set $F$</td>
<td>App.B</td>
</tr>
<tr>
<td>$G(k)$</td>
<td>gain factor</td>
<td>4.4</td>
</tr>
<tr>
<td>$G_a(s)$</td>
<td>continuous time power system stabiliser</td>
<td></td>
</tr>
<tr>
<td>$G(z)$</td>
<td>z transform of the plant $G_p(s)$</td>
<td>3.3</td>
</tr>
<tr>
<td>$G_{AVR}(z)$</td>
<td>discrete time transfer function of the AVR</td>
<td>3.3</td>
</tr>
<tr>
<td>$H$</td>
<td>generator inertia constant</td>
<td>2.2</td>
</tr>
<tr>
<td>$h$</td>
<td>maximum height of the intersection between two adjacent MFs</td>
<td>App.C</td>
</tr>
<tr>
<td>$height(F)$</td>
<td>height of a fuzzy set F</td>
<td>App.B</td>
</tr>
<tr>
<td>I/O</td>
<td>Input Output port</td>
<td>6.1</td>
</tr>
<tr>
<td>INT</td>
<td>Intensification</td>
<td>App.B</td>
</tr>
<tr>
<td>$i(t)$</td>
<td>generator current</td>
<td>App.A</td>
</tr>
<tr>
<td>$i_a(t), i_b(t), i_c(t)$</td>
<td>generator three-phase stator current</td>
<td>App.A</td>
</tr>
<tr>
<td>$i_F(t)$</td>
<td>generator field current</td>
<td>App.A</td>
</tr>
<tr>
<td>Symbol</td>
<td>Description</td>
<td></td>
</tr>
<tr>
<td>--------</td>
<td>-------------</td>
<td></td>
</tr>
<tr>
<td>$i_F(t)$</td>
<td>linearised generator field current</td>
<td></td>
</tr>
<tr>
<td>$i_D(t), i_Q(t)$</td>
<td>generator damper winding current</td>
<td></td>
</tr>
<tr>
<td>$i_{DA}(t)$</td>
<td>linearised generator damper winding current</td>
<td></td>
</tr>
<tr>
<td>$i_d(t)$</td>
<td>generator d-axis stator current</td>
<td></td>
</tr>
<tr>
<td>$i_{dA}(t)$</td>
<td>linearised generator d-axis stator current</td>
<td></td>
</tr>
<tr>
<td>$I_d(t)$</td>
<td>generator d-axis stator current</td>
<td></td>
</tr>
<tr>
<td>$i_q(t)$</td>
<td>generator q-axis stator current</td>
<td></td>
</tr>
<tr>
<td>$i_{QA}(t)$</td>
<td>linearised generator q-axis stator current</td>
<td></td>
</tr>
<tr>
<td>$I_q(t)$</td>
<td>generator q-axis stator current</td>
<td></td>
</tr>
<tr>
<td>$i_{QA}(t)$</td>
<td>linearised generator damper winding current</td>
<td></td>
</tr>
<tr>
<td>$I_i(t)$</td>
<td>generator terminal current</td>
<td></td>
</tr>
<tr>
<td>$\bar{I}$</td>
<td>complex current vector for multi-machine system</td>
<td></td>
</tr>
<tr>
<td>$\hat{I}$</td>
<td>complex current vector use common reference frame</td>
<td></td>
</tr>
<tr>
<td>$J$</td>
<td>performance index</td>
<td></td>
</tr>
<tr>
<td>$J_{min}$</td>
<td>minimum performance index</td>
<td></td>
</tr>
<tr>
<td>$K$</td>
<td>generator DC gain</td>
<td></td>
</tr>
<tr>
<td>$K_A$</td>
<td>voltage regulator gain</td>
<td></td>
</tr>
<tr>
<td>KB</td>
<td>Knowledge Base</td>
<td></td>
</tr>
<tr>
<td>$K_0$</td>
<td>conventional power system stabiliser DC gain</td>
<td></td>
</tr>
<tr>
<td>$K$</td>
<td>number of required sample period</td>
<td></td>
</tr>
<tr>
<td>$K_1 \sim K_6$</td>
<td>coefficient of single-machine infinite bus power system</td>
<td></td>
</tr>
<tr>
<td>$L$</td>
<td>transportation lag</td>
<td></td>
</tr>
<tr>
<td>L</td>
<td>switching line in the phase plane</td>
<td></td>
</tr>
<tr>
<td>$L_e$</td>
<td>transmission line inductance</td>
<td></td>
</tr>
<tr>
<td>$L_{jk}$</td>
<td>generator self or mutual inductance</td>
<td></td>
</tr>
<tr>
<td>$m, m_1, m_2$</td>
<td>parameters of two adjacent MFs</td>
<td></td>
</tr>
<tr>
<td>$MAX, max$</td>
<td>maximum</td>
<td></td>
</tr>
<tr>
<td>$MIN, min$</td>
<td>minimum</td>
<td></td>
</tr>
<tr>
<td>MF</td>
<td>Membership Function</td>
<td></td>
</tr>
<tr>
<td>MIMO</td>
<td>Multi-Input Multi-Output</td>
<td></td>
</tr>
<tr>
<td>MISO</td>
<td>Multi-Input Single-Output</td>
<td></td>
</tr>
<tr>
<td>Symbol</td>
<td>Description</td>
<td>Page</td>
</tr>
<tr>
<td>--------</td>
<td>-------------</td>
<td>------</td>
</tr>
<tr>
<td>$\bar{M}$</td>
<td>matrix for linearised multi-machine system</td>
<td>App.D</td>
</tr>
<tr>
<td>$\bar{m}_{ij}$</td>
<td>general term of the matrix $\bar{M}$</td>
<td>App.D</td>
</tr>
<tr>
<td>$N{\theta_{i}(k)}$</td>
<td>membership function for the FLBPSS</td>
<td>4.4</td>
</tr>
<tr>
<td>NB</td>
<td>Negative Big</td>
<td>4.3</td>
</tr>
<tr>
<td>NM</td>
<td>Negative Medium</td>
<td>4.3</td>
</tr>
<tr>
<td>NN</td>
<td>Neural Networks</td>
<td>8.1</td>
</tr>
<tr>
<td>NOS</td>
<td>Nominal Optimal Setting</td>
<td>5.3</td>
</tr>
<tr>
<td>NS</td>
<td>Negative Small</td>
<td>4.3</td>
</tr>
<tr>
<td>OC1 ~ OC4</td>
<td>Operating Conditions</td>
<td>6.4, 7.5</td>
</tr>
<tr>
<td>$P$</td>
<td>real power</td>
<td>5.2, 7.5.3</td>
</tr>
<tr>
<td>PB</td>
<td>Positive Big</td>
<td>4.3</td>
</tr>
<tr>
<td>$p_i(k)$</td>
<td>a point in the phase plane</td>
<td>4.4</td>
</tr>
<tr>
<td>$P_0 \sim P_4$</td>
<td>operating conditions</td>
<td>5.2</td>
</tr>
<tr>
<td>$P_e(t)$</td>
<td>electrical power</td>
<td>App.A</td>
</tr>
<tr>
<td>$PF$</td>
<td>Power Factor</td>
<td>7.5</td>
</tr>
<tr>
<td>PM</td>
<td>Positive Medium</td>
<td>4.3</td>
</tr>
<tr>
<td>$P_m(t)$</td>
<td>mechanical power</td>
<td>App.A</td>
</tr>
<tr>
<td>PS</td>
<td>Positive Small</td>
<td>4.3</td>
</tr>
<tr>
<td>PSS</td>
<td>Power System Stabiliser</td>
<td>1.3</td>
</tr>
<tr>
<td>$pu$</td>
<td>per unit</td>
<td>2.2, 2.3</td>
</tr>
<tr>
<td>$P{\theta_{i}(k)}$</td>
<td>membership function for the FLBPSS</td>
<td>4.4</td>
</tr>
<tr>
<td>q-axis</td>
<td>quadrature axis</td>
<td>App.A, App.D</td>
</tr>
<tr>
<td>$R, S$</td>
<td>fuzzy relation</td>
<td>App.B</td>
</tr>
<tr>
<td>$r$</td>
<td>generator winding resistance</td>
<td>App.A</td>
</tr>
<tr>
<td>$r$</td>
<td>number of elements</td>
<td>4.2</td>
</tr>
<tr>
<td>$R_e$</td>
<td>transmission line resistance</td>
<td>2.2</td>
</tr>
<tr>
<td>$R_{10}, R_{12}, R_{20}$</td>
<td>transmission line resistance</td>
<td>2.3</td>
</tr>
<tr>
<td>$R_B$</td>
<td>Boolean fuzzy implication</td>
<td>App.B</td>
</tr>
<tr>
<td>$R_G$</td>
<td>Goguen's fuzzy implication</td>
<td>App.B</td>
</tr>
<tr>
<td>$R_l$</td>
<td>Larsen's product operation of fuzzy implication</td>
<td>App.B</td>
</tr>
<tr>
<td>$R_m$</td>
<td>Mamdani's mini operation of fuzzy implication</td>
<td>App.B</td>
</tr>
<tr>
<td>$R_s$</td>
<td>standard fuzzy implication</td>
<td>App.B</td>
</tr>
<tr>
<td>Symbol</td>
<td>Description</td>
<td>Page No.</td>
</tr>
<tr>
<td>---------</td>
<td>-----------------------------------------------------------------------------</td>
<td>----------</td>
</tr>
<tr>
<td>$R_{Z_{a}}$</td>
<td>sequence fuzzy implication</td>
<td>App.B</td>
</tr>
<tr>
<td>$R_{Z_{m}}$</td>
<td>Zadeh's max-min rule of implication</td>
<td>App.B</td>
</tr>
<tr>
<td>$s_{1}, \ldots, s_{n}$</td>
<td>linguistic variables</td>
<td>4.3</td>
</tr>
<tr>
<td>$S_{i}^{j}$</td>
<td>linguistic values of the linguistic variables</td>
<td>4.3</td>
</tr>
<tr>
<td>$sup$</td>
<td>supremum</td>
<td>App.B</td>
</tr>
<tr>
<td>SECV</td>
<td>State Electricity Commission Victoria</td>
<td>3.2, 9.2</td>
</tr>
<tr>
<td>SISO</td>
<td>Single-Input Single-Output</td>
<td>1.6</td>
</tr>
<tr>
<td>SMIB</td>
<td>Single-Machine Infinite Bus</td>
<td>App.G</td>
</tr>
<tr>
<td>STFLBPSS</td>
<td>Self-tuned Fuzzy Logic Based PSS</td>
<td>1.7, 5.4</td>
</tr>
<tr>
<td>$T_{d}(.)$</td>
<td>damping torque</td>
<td>1.1, App.A</td>
</tr>
<tr>
<td>$T_{e}(t)$</td>
<td>electrical torque</td>
<td>App.A</td>
</tr>
<tr>
<td>$T_{m}(t)$</td>
<td>mechanical torque</td>
<td>App.A</td>
</tr>
<tr>
<td>$T_{m}$</td>
<td>mechanical torque</td>
<td>5.2</td>
</tr>
<tr>
<td>$T_{m\Delta}(t)$</td>
<td>linearised mechanical torque</td>
<td>3.2, App.A</td>
</tr>
<tr>
<td>$T_{a}(t)$</td>
<td>accelerating torque</td>
<td>App.A</td>
</tr>
<tr>
<td>$t_{r}$</td>
<td>rising time</td>
<td>3.4</td>
</tr>
<tr>
<td>$\Delta T_{s}$</td>
<td>synchronising component of the electrical torque</td>
<td>1.1</td>
</tr>
<tr>
<td>$u(kT)$</td>
<td>control signal</td>
<td>3.2, 3.3</td>
</tr>
<tr>
<td>$u$</td>
<td>driving function</td>
<td>App.A</td>
</tr>
<tr>
<td>$u$</td>
<td>a generic element in a universe of discourse</td>
<td>App.B</td>
</tr>
<tr>
<td>$U$</td>
<td>control signal</td>
<td>3.4, 4.2</td>
</tr>
<tr>
<td>$U, V, W$</td>
<td>universe of discourse</td>
<td>App.B</td>
</tr>
<tr>
<td>$U_{max}$</td>
<td>maximum stabilising signal</td>
<td>4.4</td>
</tr>
<tr>
<td>$U_{s}$</td>
<td>stabilising signal</td>
<td>5.6</td>
</tr>
<tr>
<td>$v(t)$</td>
<td>generator voltage</td>
<td>App.A</td>
</tr>
<tr>
<td>$v_{d}(t)$</td>
<td>generator d-axis stator voltage</td>
<td>App.A</td>
</tr>
<tr>
<td>$v_{d\Delta}(t)$</td>
<td>linearised generator d-axis stator voltage</td>
<td>App.A</td>
</tr>
<tr>
<td>$V_{d}(t)$</td>
<td>generator d-axis stator voltage</td>
<td>App.A</td>
</tr>
<tr>
<td>$v_{F}(t)$</td>
<td>generator field voltage</td>
<td>App.A</td>
</tr>
<tr>
<td>$v_{F\Delta}(t)$</td>
<td>linearised generator field voltage</td>
<td>App.A</td>
</tr>
<tr>
<td>$v_{q}(t)$</td>
<td>generator q-axis stator voltage</td>
<td>App.A</td>
</tr>
<tr>
<td>$v_{q\Delta}(t)$</td>
<td>linearised generator q-axis stator voltage</td>
<td>App.A</td>
</tr>
<tr>
<td>Symbol</td>
<td>Description</td>
<td>Page(s)</td>
</tr>
<tr>
<td>--------</td>
<td>-------------</td>
<td>---------</td>
</tr>
<tr>
<td>$V_q(t)$</td>
<td>generator q-axis stator voltage</td>
<td>App.A</td>
</tr>
<tr>
<td>$V_{ref}, V_{ref}(t)$</td>
<td>reference voltage</td>
<td>1.4, 3.2</td>
</tr>
<tr>
<td>$V_i(t)$</td>
<td>generator terminal voltage</td>
<td>3.2, App.A</td>
</tr>
<tr>
<td>$V_{iA}(t)$</td>
<td>linearised generator terminal voltage</td>
<td>3.2</td>
</tr>
<tr>
<td>VS</td>
<td>Very Small</td>
<td>4.3</td>
</tr>
<tr>
<td>$V_\infty$</td>
<td>infinite bus voltage</td>
<td>App.A</td>
</tr>
<tr>
<td>$\hat{V}$</td>
<td>complex voltage vector for multi-machine system</td>
<td>App.D</td>
</tr>
<tr>
<td>$\hat{V}$</td>
<td>complex voltage vector use common reference frame</td>
<td>App.D</td>
</tr>
<tr>
<td>WOR</td>
<td>Whole Overlap Ratio</td>
<td>1.10, 5.2</td>
</tr>
<tr>
<td>x</td>
<td>state variable</td>
<td>App.A</td>
</tr>
<tr>
<td>$x_d$</td>
<td>generator d-axis component of synchronous reactance</td>
<td>2.2, 2.3</td>
</tr>
<tr>
<td>$x_q$</td>
<td>generator q-axis component of synchronous reactance</td>
<td>2.2, 2.3</td>
</tr>
<tr>
<td>$x'_d$</td>
<td>generator d-axis transient reactance</td>
<td>2.2, 2.3</td>
</tr>
<tr>
<td>$x'_q$</td>
<td>generator q-axis transient reactance</td>
<td>2.2, 2.3</td>
</tr>
<tr>
<td>$X_e$</td>
<td>transmission line reactance</td>
<td>2.3</td>
</tr>
<tr>
<td>$X_{10}, X_{12}, X_{20}$</td>
<td>transmission line reactance</td>
<td>2.3</td>
</tr>
<tr>
<td>$x(t), \theta(t)$</td>
<td>linear and angular position of an inverted pendulum</td>
<td>8.1</td>
</tr>
<tr>
<td>$\hat{Y}$</td>
<td>short circuit state admittance matrix</td>
<td>App.D</td>
</tr>
<tr>
<td>$\hat{Z}$</td>
<td>open circuit state impedance matrix</td>
<td>App.D</td>
</tr>
<tr>
<td>ZR</td>
<td>Zero</td>
<td>4.3</td>
</tr>
<tr>
<td>$\alpha$</td>
<td>infinite bus voltage angle</td>
<td>App.A</td>
</tr>
<tr>
<td>$\alpha$</td>
<td>threshold level which forms a parameter varying as $[0,1]$</td>
<td>4.2</td>
</tr>
<tr>
<td>$\alpha, \beta$</td>
<td>parameters in the phase plane for FLBPSS</td>
<td>4.4</td>
</tr>
<tr>
<td>$\tau$</td>
<td>voltage sensor time constant</td>
<td>3.2</td>
</tr>
<tr>
<td>$\tau_0 \sim \tau_4$</td>
<td>time constant of conventional PSS</td>
<td>1.4</td>
</tr>
<tr>
<td>$\tau'_d$</td>
<td>d-axis open circuit transient time constant</td>
<td>2.2, 3.2</td>
</tr>
<tr>
<td>$\tau_A$</td>
<td>conventional analog AVR time constant</td>
<td>1.1</td>
</tr>
<tr>
<td>$\omega$</td>
<td>angular velocity</td>
<td>1.1</td>
</tr>
<tr>
<td>$\omega_R$</td>
<td>rated synchronous generator speed</td>
<td>3.2</td>
</tr>
<tr>
<td>$\omega_{syn}$</td>
<td>synchronous speed</td>
<td>2.2</td>
</tr>
<tr>
<td>$\omega(t)$</td>
<td>generator speed</td>
<td>App.A</td>
</tr>
<tr>
<td>Symbol</td>
<td>Description</td>
<td>App.</td>
</tr>
<tr>
<td>--------</td>
<td>-------------</td>
<td>------</td>
</tr>
<tr>
<td>$\omega_\Delta(t)$</td>
<td>linearised generator speed</td>
<td>A</td>
</tr>
<tr>
<td>$\delta$</td>
<td>distance parameter between two adjacent MFs</td>
<td>C</td>
</tr>
<tr>
<td>$\delta(t)$</td>
<td>generator rotor angle</td>
<td>A</td>
</tr>
<tr>
<td>$\delta_\Delta(t)$</td>
<td>linearised generator rotor angle</td>
<td>A</td>
</tr>
<tr>
<td>$\Delta T$</td>
<td>sampling interval</td>
<td>4.3</td>
</tr>
<tr>
<td>$\Delta \omega$</td>
<td>speed deviation</td>
<td>4.3</td>
</tr>
<tr>
<td>$\Delta \dot{\omega}$</td>
<td>acceleration</td>
<td>4.3</td>
</tr>
<tr>
<td>$\delta_{ij}$</td>
<td>rotor angle between machine i and j</td>
<td>D</td>
</tr>
<tr>
<td>$\delta_{ij\Delta}$</td>
<td>linearised value of $\delta_{ij}$</td>
<td>D</td>
</tr>
<tr>
<td>$\lambda(t)$</td>
<td>flux linkage of the synchronous generator</td>
<td>A</td>
</tr>
<tr>
<td>$\lambda_d(t)$</td>
<td>generator d-axis stator flux linkage</td>
<td>A</td>
</tr>
<tr>
<td>$\lambda_D(t)$</td>
<td>generator d-axis damper winding flux linkage</td>
<td>A</td>
</tr>
<tr>
<td>$\lambda_F(t)$</td>
<td>generator field winding flux linkage</td>
<td>A</td>
</tr>
<tr>
<td>$\lambda_q(t)$</td>
<td>generator q-axis stator flux linkage</td>
<td>A</td>
</tr>
<tr>
<td>$\lambda_Q(t)$</td>
<td>generator q-axis damper winding flux linkage</td>
<td>A</td>
</tr>
<tr>
<td>$\theta$</td>
<td>rotor position</td>
<td>A</td>
</tr>
<tr>
<td>$\theta_i(k)$</td>
<td>phase angle in the phase plane</td>
<td>4.4</td>
</tr>
<tr>
<td>$\theta_0$</td>
<td>initial angle</td>
<td>4.4</td>
</tr>
<tr>
<td>$\mu$</td>
<td>fuzzy membership function</td>
<td>B</td>
</tr>
<tr>
<td>$\mu_F(u)$</td>
<td>membership function of a fuzzy set $F$</td>
<td>B</td>
</tr>
<tr>
<td>$\mu_A, \mu_B$</td>
<td>membership function for two fuzzy sets $A$ and $B$</td>
<td>B</td>
</tr>
<tr>
<td>$\cup$</td>
<td>union</td>
<td>B</td>
</tr>
<tr>
<td>$\cap$</td>
<td>intersection</td>
<td>B</td>
</tr>
<tr>
<td>$\bullet$</td>
<td>algebraic product</td>
<td>B</td>
</tr>
<tr>
<td>$\odot$</td>
<td>bounded product</td>
<td>B</td>
</tr>
<tr>
<td>$\hat{\otimes}$</td>
<td>drastic product</td>
<td>B</td>
</tr>
<tr>
<td>$\ast$</td>
<td>triangular norm</td>
<td>B</td>
</tr>
<tr>
<td>$\hat{\oplus}$</td>
<td>triangular co-norm</td>
<td>B</td>
</tr>
<tr>
<td>$\hat{\otimes}$</td>
<td>algebraic sum</td>
<td>B</td>
</tr>
<tr>
<td>$\oplus$</td>
<td>bounded sum</td>
<td>B</td>
</tr>
<tr>
<td>$\triangledown$</td>
<td>drastic sum</td>
<td>B</td>
</tr>
<tr>
<td>$\Delta$</td>
<td>disjoint sum</td>
<td>B</td>
</tr>
<tr>
<td>Symbol</td>
<td>Description</td>
<td>Section</td>
</tr>
<tr>
<td>--------</td>
<td>--------------</td>
<td>-----------</td>
</tr>
<tr>
<td>∨</td>
<td>max</td>
<td>App.B</td>
</tr>
<tr>
<td>∧</td>
<td>min</td>
<td>App.B</td>
</tr>
<tr>
<td>∑</td>
<td>summation</td>
<td>5.1, App.D</td>
</tr>
</tbody>
</table>

**List of Principal Symbols and Abbreviations**

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XXXIII
This thesis investigated the application of fuzzy controllers as real-time power system stabilisers for single-machine and two-machine infinite bus power systems.

The advantages of using the-state-of-the-art power system stabilisers to damp low-frequency oscillation in power systems is well known. The most widely used conventional power system stabiliser is the lead-lag compensator where the gain settings are fixed at certain values and determined for a particular operating condition. The design of the conventional power system stabiliser is based on a linear approximation of the non-linear power plant. This means that the conventional power system stabiliser can provide the optimal performance only for that particular operating point. Since the operating point of a power system drifts as a result of continuous load changes or unpredictable major disturbances such as a three-phase fault, the fixed gain conventional power system stabiliser can not adapt the stabiliser parameters in real time based on on-line measurements. Although general parameters can be decided for a conventional power system stabiliser according to a particular range of operating conditions, the design procedure is very complex. For multi-machine systems, individual machine may have different requirements of damping torque and synchronising torque, and multi-machine multi-mode power system stabilisation techniques must be sought, especially when many conventional power system stabilisers are used in the system and their coordination has to be taken into consideration. These constraints made the design of the conventional power system stabiliser even more complex.

Self-tuning and adaptive power system stabilisers have been employed to adapt the stabiliser parameters to maintain good dynamic performance over a wide range of operating conditions. However, self-tuning and adaptive power system stabilisers suffer from a major drawback of requiring model identification in real-time which is very time consuming and computational intensive. Therefore, self-tuning and adaptive power system stabilisers are difficult to realise because they require parameter identification, state observation and feedback gain computation.

This thesis is mainly concerned with new simpler alternative fuzzy control
schemes for power system stabilisation. Two fuzzy control schemes are proposed and explored in the thesis. One of the fuzzy control schemes involves a **fuzzy logic controller (FLC)** being applied to a power system as a power system stabiliser. The core of the FLC is a set of linguistic control rules related by the dual concepts of fuzzy implication and the compositional rule of inference. In essence, the FLC provides an algorithm which can convert the linguistic control strategy based on expert knowledge into an automatic control strategy. The second fuzzy control scheme involves the development of a **Fuzzy Logic Based Power System Stabiliser (FLBPSS)** based on fuzzy set theory. The stabilising signal is computed according to the proposed new non-linear fuzzy membership functions depending on the speed and acceleration states of the synchronous generator. These fuzzy control schemes are very suitable for on-line control due to their lower computational burden, simplicity and robustness. The design frame work of these control schemes does not necessitate the use of a mathematical model to describe the dynamics of the control system. Comprehensive sensitivity analysis has been carried out to assess the robustness of the FLC and FLBPSS for changes in system parameters and under different operating conditions for both small and large perturbations. The input and output membership functions of the FLC were adjusted according to an evaluation index in order to achieve the optimal performance. The initial FLC design with a complete filled rule table (49 rules) have been reduced using neural network techniques to improve the dynamic performance. Optimisation of the two fuzzy control schemes is carried out through digital simulation using a performance index.

In order to carry out an investigation into the design, optimisation and implementation of the two fuzzy control schemes, it is essential to design a digital **automatic voltage regulator (AVR)**. A discrete-time analytical design method is employed. The effectiveness of the designed automatic voltage regulator is demonstrated through simulation and implementation.

The optimised fuzzy controller has also been implemented in real-time for on-line control of both single-machine and two-machine infinite bus power systems. The effectiveness of the fuzzy controller was experimentally confirmed by observing the effects of a step change in reference voltage, a step change in load and a three-phase
to ground fault. Numbers of tests have also been conducted at various operating conditions. A very oscillatory generator rotor angle and speed deviation were observed without any stabilisation control when the system is subjected to the above disturbances. The oscillation of rotor angle and speed deviation were substantially damped out with the fuzzy controller in operation. The simulation and experimental results reveal that the optimised fuzzy controller has enhanced the damping of both the dynamic and transient stability of the single-machine and two-machine infinite bus power systems.
Statement of Originality

I hereby certify that the work embodied in this thesis is the result of original research and has not been submitted for a higher degree to any other University or Institution.

This thesis may be made available for consultation within the University Library and may be photocopied or lent to other libraries for the purposes of consultation if accepted for the award of the degree.

(Signed) Juan Shi
Preface

This thesis examines the optimisation and implementation of fuzzy controllers for power system stabilisation. An optimal fuzzy controller has been used on-line in real time for both single-machine and two-machine infinite bus power systems. A digital automatic voltage regulator has also been designed. A listing of all the relevant publications [Shi, Herron and Kalam, 1992; Shi, Herron and Kalam, 1993 and Shi, Herron and Kalam, 1994] is provided here:


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Finally, I wish to dedicate this thesis to my parents. They have brought me
up with all the love, understanding and wisdom for which I am greatly indebted. I would also like to express my gratitude to my husband Les Nakonieczny for his encouragement and support to accomplish my education. My gratitude also extends to my brother and sister, my friend Yiqiu Li and Jian Wang for their encouragement and support during all these years.
Chapter 1

Introduction

1.1 Excitation Control and Its Role on Power System Stability

In the last few decades, considerable attention has been given to the excitation system and its role in improving power system stability. Because of the small effective time constants in the excitation control loop, it was assumed that a large control effort could be expanded through excitation control with a relatively small input of control energy. By the use of a voltage regulator in the excitation control system, the output of the exciter can be adjusted so that the generated voltage and reactive power change in a desired way. In early systems, the voltage regulator was entirely manual. In modern control systems the voltage regulator is an automatic controller that senses the generator output voltage as a feedback signal then adjusts the generator excitation level in the desired direction. This kind of voltage regulator has been known as an Automatic Voltage Regulator or AVR.

Early investigators realised that the so-called "steady-state" power limits of power networks could be increased by using the high-gain AVRs [Concordia, 1944]. A high-gain AVR was also recommended for reducing the steady state error of the system output. Although modern voltage regulators and excitation systems with fast speed of response and with a high ceiling voltage can be used to improve the
transient stability (defined in Section 1.2) by increasing the synchronising torque of the machine, their effects on the damping torque are rather small. It was also recognised that the voltage regulator gain requirement was different at no-load conditions from that needed for good performance under load. For different stability (transient or dynamic) control problems, the requirements on the excitation control system may be significantly different. In transient stability studies, a very fast and high-ceiling voltage control action from the excitation control system is needed to reduce the amplitude of the first oscillatory swing and to help the generator to maintain its synchronism. Due to this reason, a fast excitation system with a high-gain AVR is beneficial to the control of the system transient stability. However, in the case where the system may operate with negative damping characteristics the high-gain excitation control system aggravates the situation by increasing the negative damping and hence instability may result in the system [DeMello, 1969], [Heffron, 1952], [Anderson, 1977]. This can be analysed in dynamic stability studies by using the small signal linearised system model given in Section A.3 of Appendix A, with constant reference signals [Heffron, 1952], [DeMello, 1969]. For a system without the AVR regulation, the damping torque component of the electrical torque at frequency $\omega$ is given by

$$\Delta T_d(\omega) = \frac{K_2K_3^2K_4\tau_{do}^2\omega}{1 + K_3^2\tau_{do}^2\omega^2}\Delta\delta(\omega)$$  \hspace{1cm} (1.1)$$

Since the parameters $K_2$, $K_3$, and $K_4$ are all positive, the damping torque given by equation (1.1) is positive. However, for a system with the AVR in operation, the damping torque component of the electrical torque can be expressed approximately as follows:

$$\Delta T_{d2}(\omega) \approx \frac{K_2K_5K_A(\tau_{d0} + \tau_A/K_3)\omega}{[(1/K_3 + K_6K_A) - \tau_{d0}/\tau_A\omega^2]^2 + (\tau_{d0} + \tau_A/K_3)^2\omega^2}\Delta\delta(\omega)$$  \hspace{1cm} (1.2)$$

where $\Delta T_d(\omega)$ has the same sign as $K_5$. At low frequencies, the synchronising component of the electrical torque is described approximately by

$$\Delta T_s(\omega) \approx [K_1 - \frac{K_2K_5}{K_6}]\Delta\delta(\omega)$$  \hspace{1cm} (1.3)$$
Chapter 1. Introduction

At some operating conditions such as for moderate to high system transfer impedances, and heavy loadings, the parameter $K_5$ can be negative [DeMello, 1969], [El-Sherbiny, 1973]. In these cases the damping torque in equation (1.2) becomes negative. Thus it can be assumed that the voltage regulator in the excitation system introduces negative damping when $K_5$ is negative.

In the 1950s engineers became aware of the instabilities introduced by the (then) modern voltage regulators, and stabilising feedback circuits came into common use [Crarg, 1950].

In the 1960s large interconnected systems experienced growing oscillations that disrupted parallel operation of large systems [Ellis, 1966], [Schleif, 1966], [Byerly, 1967], [Schleif, 1967], [Hanson, 1968], [Dandeno, 1968], [Shier, 1968], [DeMello, 1969], [Schleif, 1969]. The first example of inter-system low-frequency oscillations was observed during a WSCC (Western Systems Coordinating Council) in the USA [Schleif, 1966]. The interconnected system operated satisfactorily for a while, but low-frequency oscillations at about 6 cycles per minute developed. The interconnection was then tripped off, leaving the Northwest Power Pool oscillating about 3 cycles per minute and the Southwest Power Pool oscillating at about 11 cycles per minute.

A number of minor oscillations of system frequency were also observed in the South East Australian interconnected system [Bolden, 1982]. This system is characterised by having two main generator centres of La Trobe Valley in Victoria and the Snowy Mountains Hydro-electric Scheme, each connected to Melbourne (load centre) by links of length 120 and 360 km respectively.

With more and more experience accumulated from interconnected electrical power system operation, power system engineers are now convinced that the low-frequency oscillations are due to the inherently weak natural damping of large and weakly coupled systems. The situations of negative damping were further aggravated by the regulator gain [Klopfenstein, 1971]. Engineers learned that the system damping could be enhanced by artificial signals introduced through the excitation system. This scheme has been very successful in combating growing oscillation
problems experienced in the power systems. As a result, the use of power system stabiliser (PSS) to dampen the oscillations in the power system was introduced.

1.2 The Definition of Power System Stability

The definition of power system stability is as follows [Anderson, 1977]:

- **Power System Stability.** If the oscillatory response of a power system during the transient period following a disturbance is damped, and the system settles in a finite time to a new steady operating condition at constant frequency, the system is said to be stable. If the system is not stable according to this definition, then it is considered unstable.

Power system stability is further classified into two categories: *dynamic stability* due to small disturbances, and *transient stability* due to large disturbances. It should be noted that this classification is not universally used. For example, in some different classifications, the dynamic stability is called *steady-state stability*.

- **Dynamic Stability.** Dynamic stability refers to the stability of a power system subject to small and sudden perturbations.

Typical perturbations under this category may be small, randomly occurring changes in load or small alterations in reference voltage settings. If the system is *dynamically stable*, it is expected that after a temporary small disturbance the system will return to its initial state, while for a permanent small disturbance the system will acquire a new operating point after a transient period [Anderson, 1977]. In both cases the synchronism of the system should not be lost. The size of small disturbances may be measured by the criterion that the perturbed system can be stabilised in an approximately linear region [Anderson, 1977].

- **Transient Stability.** Transient stability refers to the stability of power system subject to severe disturbances which are maintained for a short time and
causes a significant reduction in the machine terminal voltage and the ability to transfer power.

The severe disturbances which cause transient stability problems may typically be large changes in load, three-phase faults or transmission line switching. It is usually assumed that the system under study is stable before a large disturbance happens. If the system is *transiently stable*, the system oscillations resulting from large disturbances are damped. However, transient stability of the system depends very much on the initial operating condition of the system and the nature (i.e., the type, magnitude, duration, and location, etc.) of the large disturbances that are applied to the system [Anderson, 1977], as well as on the post-fault system configuration.

For successful operation and control of power systems, the *dynamic stability* and *transient stability* of the system must be carefully considered.

### 1.3 The Application of Power System Stabilisers (PSSs)

The application of a power system stabiliser (PSS) is to generate a supplementary stabilising signal, which is applied to the excitation control loop of a generating unit, to introduce a positive damping torque. By using the supplementary stabilising signal, the negative damping effect of the AVR regulation can be cancelled, at the same time, the positive damping effect of the system can also be increased so that the system can operate even beyond the steady-state stability limit.

Stabilising signals are introduced in excitation systems at the summing junction where the reference voltage and the signal produced from the terminal voltage are added to obtain the error signal fed to the regulator-excitation system. The stabilising signal $V_s$ is usually obtained from speed or a related signal such as the rotor speed, bus frequency and electrical power [DeMello, 1969], [Keay, 1971], [IEEE, 1980], [Larsen, 1981], is proceeded through a suitable network to obtain the desired
phase relationship. Other input signals, such as the accelerating power [Bayne, 1977], [DeMello, 1978], [Lee, 1981] have also been used. During the last decade, the deviation on equivalent rotor speed ($\Delta \omega_{eq}$) derived from the shaft speed and integral of change in terminal electrical power has been used [Lee, 1981], [Kundur, 1989].

In the analysis and control of power system stability, two distinct types of system oscillations are usually recognised [Kundur, 1989]. One type is associated with units at a generating station swinging with respect to the rest of the power system. Such oscillations are referred to as local plant mode oscillations. The frequencies of these oscillations are typically in the range of 0.8 to 2.0 Hz. The second type of oscillation is associated with the swinging of many machines in one part of the system against machines in other parts. These are referred to as inter-area mode oscillations. The frequencies of the second type oscillations are in the range of 0.1 to 0.7 Hz. The basic function of the PSS is to add damping to both types of system oscillations.

The overall excitation control system with PSS in operation is designed so as to:

- maximise the damping of local mode as well as inter-area mode oscillations without compromising the stability of other mode;
- enhance both the steady state stability or dynamic stability, and transient stability of the power system;
- not adversely affect system performance during major system upsets which cause large frequency excursions;
- minimise the consequences of excitation system malfunction due to component failures.
1.4 Conventional Power System Stabilisers (CPSSs)

Power System Stabilisers designed using classical control theory can be called conventional power system stabilisers (CPSSs). The CPSS which is a feedback element from the shaft speed and is often given in the form [DeMello, 1969]:

\[
G_s(s) = \frac{K_0\tau_0 s}{1 + \tau_0 s} \left[ \frac{1 + \tau_1 s}{1 + \tau_3 s} \right]
\]

(1.4)

The first term in equation (1.4) is a reset term that is used to “wash out” the compensation effect after a time lag \( \tau_0 \), with typical values of 4 seconds [DeMello, 1969] to 20 seconds or 30 seconds [Schleif, 1969]. The use of reset control will assure no permanent offset in the terminal voltage due to a prolonged error in frequency, such as might occur in an overload or islanding condition. The second term in \( G_s(s) \) is a lead compensation pair that can be used to improve the phase lag through the system from \( V_{ref} \) to \( \Delta \omega \) at the power system frequency of oscillation.

The settings of the time constants of the phase compensating lead-lag functions of the stabiliser can be determined by several techniques ([Schleif, 1968], [DeMello, 1969], [Schleif, 1969], [Warchol, 1971], [Gerheart, 1971], [Hayes, 1973], [Bollinger, 1975]) once the frequency response of the excitation control system has been known [Yu, 1971], [Vaahedi, 1986], [Arnautovic, 1987], [Chow, 1989], [Bollinger, 1975].

The design of the most widely used CPSS is based on linearised fixed-parameter models of the non-linear power system which are derived from the linearisation of the system at a given operating point. The parameters of the CPSSs are fixed at certain values which are determined under this particular operating point. Since the operating point of a power system drifts as a result of continuous load changes or unpredictable major disturbances such as a three-phase fault, the fixed parameter CPSSs can not adapt the stabiliser parameters in real time based on on-line measurements, i.e., they can not track the variations in the system operating conditions over a wide range of operating conditions. Therefore, they can not provide the best response in real time.
Although general parameters can be decided for a CPSS according to a particular range of operating condition, the design and analysis of the CPSS are very complex. For multi-machine system, it is difficult to consider the interaction of the individual generating machines [Laughton, 1966], [El-sherbiny, 1971]. Moreover, individual machines in multi-machine systems may have different requirements of damping torque and synchronising torque, and multi-machine multi-mode power system stabilisation techniques must be sought, especially when many CPSSs are used in the system and their coordination has to be taken into consideration. This made the selection of the CPSS parameters and the CPSS design for multi-machine power system even more complex [Fleming, 1981], [Crusca, 1991].

Another problem with the CPSS is that because there are uncertainties in the electric power system, there always exist unmodelled dynamics in the power system. As a result, the CPSS does not always perform effectively in the real electrical power system.

It is well understood that the optimal settings of the above mentioned CPSSs at one optimal condition are no longer the optimal one under the other. Therefore, in order to get optimal response using CPSS, resetting and tuning of the CPSS parameters are necessary for different operating conditions.

In the past decade, much effort has been directed towards the development of microcomputer-based digital controllers, such as adaptive or self-tuning PSSs, to generate desired supplementary stabilising signals in order to improve the overall power system stability over a wide range of operating conditions.

### 1.5 Adaptive Power System Stabilisers

The self-tuning regulator in control system is obtained by combining control design and recursive parameter estimation method. One of the ways automating modelling and design is the following:

1. Determine a model structure;
Chapter 1. Introduction

2. Estimate the parameters of the model recursively using the methods such as least squares, maximum likelihood, extended and generalised least squares, instrumental variables, extended Kalman filtering and stochastic approximation;

3. Use the estimates to calculate the control law by a suitable design method, e.g. phase and amplitude margins, pole-placement, minimum variance control and Linear Quadratic Gaussian (LQG) control.

The regulator obtained in such a way is called a self-tuning regulator because it has facilities for tuning its own parameters.

The self-tuning regulator is motivated by the desire to obtain automatic tuning of a control loop. An adaptive regulator can be achieved by modifying a self-tuning regulator to control a plant with varying parameters. The parameter estimation algorithm has to be changed so that it can track varying plant parameters. There are many schemes for adaptive control that are closely related to the self-tuning control. Three of these schemes are Gain Scheduling, Model-Reference Adaptive Systems (MRAS), and an adaptive regulator obtained from Stochastic-Control Theory.

The adaptive and self-tuning PSS have offered better dynamic performance than the fixed gain CPSS because it has the ability to automatically track the variations in power system parameters and operating conditions. However, for the realisation of such adaptive and self-tuning PSS, on-line identification of system parameters, observation of system states and computation of feedback gains in a short sampling period are needed which are so time consuming and computational intensive that it becomes infeasible to implement it in a real time control environment. As an alternative to a self-tuning PSS, variable structure PSSs have been proposed in the literature [Hsu, 1983], [Chan, 1983], [Hsu, 1986].

Lately, simpler alternative control schemes for stabilisation of power systems were proposed, they are the rule-based PSS [Hiyama, 1989] and fuzzy logic controllers [Hsu, 1990], [Hiyama, 1991]. These schemes are very suitable for on-line control due to their lower computational burden and simplicity. A comparison study between a fuzzy controller and a rule-based PSS [Hassan, 1991] shows that fuzzy controller is more suitable due to its robustness.

1.6 Fuzzy Logic and Fuzzy Control

Over the past years, the design of control systems has been based on classical or modern control theory (such as Nyquist, Bode, state-space, optimal control, root locus, $H_{\infty}$, $\mu$-analysis, etc.). Both approaches require a mathematical model based upon assumptions of linearity and stationarity to describe the plant to be controlled. Few of these design methods represent uncertainty and incompleteness in process knowledge or complexity in the resultant design. Classical control theory still provides good solution to linear single-input, single-output (SISO) systems. Modern control theory is also useful in solving multiple-inputs, multiple-outputs (MIMO) problems using state-space methods. However, the mathematical model represents a formulation of prior information into an analytic structure. In the real world, systems have some unknown parameters or highly complex and non-linear characteristics. Attempts to overcome this difficulty have resulted in research in adaptive control but the structure of such systems is very complex and non-linear, and its sta-
bility requirements often limit its successful application. Recent work on $H_\infty$ and $\mu$-analysis in robust control design deals with multi-variable linear systems with additive disturbances and parametric uncertainty, but still requires a notional low order model of the process, measures of the process and disturbance variations, and frequently leads to controller designs of very high order. Whilst many of these new techniques are mathematically advanced, their adoption by industry has been slow, this apparent reluctance is due to the amount and quality of information that has to be gathered to ensure adequate controller performance, and the constraints associated with the applicability of the method.

However there are many processes that are too complex, highly non-linear, uncertain (in parameters and disturbances), incomplete (aspects of the process or systems are unknown) or non-stationary, and have subtle and interactive exchanges with the operating environment. Yet such processes are successfully controlled by skilled human operators, using only experiential knowledge [Efstathiou, 1988]. The human operator also has the attribute of providing highly non-linear controls, with time varying parameters; additionally elements of learning and self-organisation are natural aspects of human control. Classical expert systems based upon a domain-independent inference engine which manipulates the heuristic based domain-dependent knowledge base; have been investigated widely in control systems design [Astrom, 1986], [Harris, 1985], [Trankle, 1985], [Mamdani, 1986]. Expert systems are usually rule based systems which have the attribute of being very fast to execute, with simple pattern matching of the antecedent being sufficient to activate a response under forward chaining inference. However under classical rule based systems a (situation/action) pair is required for every possible combination. The deliberate overlapping or interference of fuzzy sets avoids this problem by allowing rule generation within the quantisation range of the variable under control, which provides a tool that efficiently copes with adequately precise linguistic representations of the system, and produces a control protocol that satisfies some performance criterion that may be mathematical or linguistically prescribed.

Fuzzy sets are a generalisation of conventional set theory that were introduced by Zadeh in 1965 as a mathematical way to represent vagueness in every day life
[Zadeh, 1965]. Nowadays, fuzzy sets are equipped with their own mathematical foundations, rooting from set-theoretical basis and many-valued logic. Their achievements have already enriched the classic two-valued calculus with a deep and novel perspective. In more than two decades since its inception by Zadeh, the theory of fuzzy sets has matured into a wide-ranging collection of concepts, models, and techniques for dealing with complex phenomena which do not lend themselves to analysis by classical methods based on probability theory and bivalent logic.

Applications of fuzzy set theory have been already found in many different areas. One could probably classify those applications as follows [Zimmermann, 1990]:

- Applications to mathematics, that is, generalisations of traditional mathematical such as topology, graphy theory, algebra, logic, etc.;
- Applications to algorithms such as clustering methods, control algorithms, mathematical programming, etc.;
- Application to standard models such as “the transportation model,” “inventory control models,” “maintenance models”, etc.;
- And finally applications to real-world problems of different kinds.

Fuzzy set theory is a generalisation of classical set theory that allows more realistic mathematical representation of linguistic values that contain a degree of fuzziness. Detailed overviews of fuzzy set theory are presented in Zadeh [Zadeh, 1973], Lee [Lee, 1990a and 1990b] and Gupta et al [Gupta, 1977].

The first application of fuzzy set theory to the control of systems was by Mamdani and Assilian [Mamdani, 1975], who reported on the control of a laboratory model steam engine. This was followed by Kickert and Van Nauta Lemke [Kickert, 1976], who derived a PI type FLC for a warm water plant; the FLC had a fast response, with same accuracy as the PI controller. For the same laboratory plant Mamdani developed a self-organising FLC that synthetised the control rule base by observing the process response; later this approach was extended by Procyk and Mamdani [Procyk, 1979] and by Harris et al for autonomous guided vehicles.
Since the mid 1980s fuzzy control has become more popular among control engineers working in industry, and more and more systems are implemented. Application of fuzzy control includes automatic train operation, water quality control, elevator control, automobile transmission control, fuzzy logic controller hardware systems, fuzzy memory devices, and fuzzy computers. These applications have demonstrated the use of fuzzy control in the context of ill defined processes that can be controlled by a skilled human operator without the knowledge of the underlying dynamic operation. The advantage of using fuzzy set theory to construct controller lies in its ability to merge the experience, heuristic and intuition of expert operators in the control design. Fuzzy logic, the logic in which fuzzy control is based, provides an effective means of capturing the approximate, inexact nature of the real world. The core of a fuzzy logic controller (FLC) is a set of linguistic control rules related by the dual concepts of fuzzy implication and the compositional rule of inference. In essence, a FLC provides an algorithm which can convert the linguistic control strategy based on expert knowledge into an automatic control strategy. Fast fuzzy controllers have been designed and fabricated using different technologies. Fuzzy control literature has reported superior performance to those obtained by conventional control algorithms.

### 1.7 The Application of Fuzzy Controllers as PSSs

The first application of a traditional fuzzy logic controller (FLC) as a PSS was reported in 1990 [Hsu, 1990]. The FLC has been applied to a multi-machine power system. The performance of the FLC has been compared with the CPSS through digital simulation and found to be better. However, comprehensive analysis and fine tuning of the FLC has not been investigated and the FLC has not been implemented in real time. The system exhibited minor oscillation under steady state since the rule base and the membership function shapes have not been fine tuned.
Hiyama et al proposed a PSS based on fuzzy set theory in 1991 [Hiyama, 1991] and it has been named a fuzzy logic based power system stabiliser (FLBPSS). For the FLBPSS, operating conditions of the synchronous machine are expressed by the quantities of speed deviation and acceleration in the phase plane. The generator speed is measured at every sampling instant. Only one set of previous data is required to evaluate the generator acceleration. Therefore, the heavy calculation burden is avoided. The design framework of a fuzzy controller does not necessitate the use of a mathematical model to describe the dynamics of the control system and experience has shown that it yields results which are better than those obtained by conventional schemes. The fuzzy control schemes can be constructed using a simple microcomputer or a PC associated with A/D and D/A converters. Comparison studies between a self-tuning stabiliser and a fuzzy logic stabiliser has been done by Lim and Hiyama [Lim, 1993]. In the studies, different tests were simulated, with the non-linear power systems operating over a wide power range. Simulation results show that both stabilisers are suitable for, and effective in, enhancing the damping of the mechanical mode oscillations in a single-machine infinite bus power system and two-machine power systems without an infinite bus, of which one exhibits multi-mode oscillations. Recently, Hassan et al have proposed a self-tuned FLBPSS to improve the system dynamic performance [Hassan, 1992], [Hassan, 1993a], [Hassan, 1993b].

1.8 Motivation for the Thesis

This thesis involves the optimisation and implementation of fuzzy controllers for power system stabilisation. The objective is to incorporate the advantage of fuzzy controllers with the digital AVR to enhance the damping for both dynamic and transient responses and to improve the stability of power systems.

In the literature, no research has been carried out to optimise the above mentioned fuzzy logic controller (FLC) and fuzzy logic based power system stabiliser (FLBPSS). No real time implementation had been done at the time of initiating this project. Moreover, performance of the fuzzy controllers must be improved,
comparison study of the two fuzzy control schemes must be carried out and most importantly, the optimal fuzzy controller must be tested in real time.

In order to improve the performance of the FLC, a different design method has been utilised. Continuous membership functions have been used and adjusted to obtain the best performance. An index named *Whole Overlap Ratio (WOR)* has been defined to assist in the fine tuning of the fuzzy membership function shape in order to improve the performance of the FLC. The initial FLC was designed with a complete filled rule table (49 rules). Neural network techniques were used for learning the corresponding control surface and for extracting a reduced set of rules describing the system.

Also to improve the performance of the FLBPSS, new non-linear membership functions that differ from the ones used in the past ([Hiyama, 1991], [Hassan, 1992]) have been proposed. Comprehensive analysis has been examined to optimise the settings of the FLBPSS. Sensitivity analysis has been carried out to assess the robustness of the proposed FLBPSS for changes in system parameters and under different operating conditions for both small and large perturbations.

Hassan et al [Hassan, 1992] suggested a self-tuned FLBPSS (STFLBPSS) whose performance has been shown to be better than that of the FLBPSS proposed by Hiyama et al [Hiyama, 1991]. However, they have not considered any comprehensive analysis to test the robustness of the FLBPSS. In this work, it is intended to compare the performance of the proposed FLBPSS with that of the STFLBPSS of Hassan et al.

Comparison studies of the two kinds of fuzzy control schemes (FLC and FLBPSS) have also been explored. The most effective one has been chosen for real time implementation. The implementation has been carried out on a single-machine infinite bus and a two-machine infinite bus power system respectively.

The availability of inexpensive microprocessors and digital controllers has prompted a great deal of attention towards digital excitation control [Runtz, 1973], [Kanniah, 1984a], [Kanniah, 1984b], [Kanniah, 1984c], [Ghandakly, 1987a], [Ghandakly, 1987b]. These microprocessor control systems have a great deal of flexibility and
have the ability to implement sophisticated control algorithms efficiently and economically. In order to get the knowledge of how to apply a fuzzy controller to power system stabiliser, it is necessary to complete the following tasks:

- Design of digital voltage regulator. To avoid complexities as the design of self-tuned regulators, an effective and straightforward digital AVR design has been carried out which can be easily implemented;

- Develop a fuzzy logic controller (FLC) and a fuzzy logic based power system stabiliser (FLBPSS);

- Optimise the above fuzzy logic control schemes;

- Comparison study of the proposed fuzzy controllers with self-tuned FLBPSS (STFLBPSS);

- Implementation of an optimal fuzzy controller in a single-machine infinite bus power system;

- Implementation of an optimal fuzzy controller in a multi-machine power system.

So far, the fuzzy PSS is still the only one put into real operation in an experimental power system in Australia. During this research time, similar work has been carried out in Canada [Hassan, 1993a], [Hassan, 1993b] and Japan [Matsuki, 1991].

1.9 Contributions of the Thesis

The original contributions of this thesis are summarised as follows:

1. Two types of fuzzy controllers have been proposed and analysed;

2. Discrete-time analytical design of an Automatic Voltage Regulator has been employed;
3. Insight into the influence of different membership function shapes to the performance of the fuzzy controller has been examined;

4. Comprehensive sensitivity analysis of the two fuzzy control schemes have been investigated to assess the robustness of the proposed FLC and FLBPSS;

5. Neural Network techniques have been used to simplify the original fuzzy controller by learning the FLC control surface;

6. The effectiveness of the FLBPSS was experimentally corroborated by observing the effects of a step change in the load on the system, a three-phase fault and a step change in reference voltage. The implementation has been carried out on both a single-machine infinite bus and a multi-machine power system.

1.10 Organisation of the Thesis

This thesis consists of nine chapters. The rest of the eight chapters are organised as follows:

In Chapter 2, the single-machine and multi-machine power systems used for this research are described.

In Chapter 3, the design of the automatic voltage regulator (AVR) has been carried out in the z-domain. The voltage regulator is the intelligence of the power system and controls the output of the exciter so that the generated voltage and reactive power change in a desired way. Mathematical modelling of the single-machine infinite bus experimental system is detailed in Chapter 3 for the analysis and design of the AVR. Chapter 3 also provides the theoretical design and simulation result of the digital AVR. The z-domain analytical design method has been employed.

Fuzzy Logic Controller (FLC) structure has been described in the beginning of the Chapter 4. Two fuzzy control schemes for power system stabilisation have been proposed in this chapter. One uses traditional FLC as a power system stabiliser
and the other is a fuzzy logic based power system stabiliser (FLBPSS). For the FLC 49 rules have been used and 7 rules have been utilised for the FLBPSS. Two new non-linear membership functions have been proposed for the FLBPSS in order to improve its performance.

After the fuzzy controller had been designed in Chapter 4, the remainder of the work was to adjust the fuzzy controller parameters to obtain the optimal performance. In Chapter 5, an index—Whole Overlap Ratio (WOR)—has been defined to assist in the fine tuning of the FLC membership function shape so that the optimal performance of the FLC can be achieved. The optimal setting of the proposed FLBPSS has also been studied in detail in this chapter. Comprehensive sensitivity analysis has been carried out to assess the robustness of the proposed FLC and FLBPSS for changes in system parameters and operating conditions under both small and large perturbations. The performance of the proposed FLBPSS has also been compared with that of the self-tuned FLBPSS of Hassan et al. The comparison study has been evaluated by using both a discrete-type quadratic performance index and the dynamic response. The performance indices and the dynamic responses of the optimised FLC and FLBPSS has also been compared. The most effective one has been chosen for real time implementation.

The implementation study of the proposed fuzzy PSS applied to a single-machine infinite bus system is demonstrated in Chapter 6. The development of the hardware and software is described in detail in this chapter. The performance of the optimised fuzzy PSS is evaluated when the power system is subjected to both small and large perturbations under wide range of operating conditions for the single-machine infinite bus power system.

To evaluate the effectiveness of the proposed fuzzy controller for multi-machine systems, simulation and implementation studies are carried out on a two-machine infinite bus system. Chapter 7 presents both the simulation and implementation results. Due to the equipment limitation, the multi-machine system study have only been carried out on a two-machine infinite bus power system.

In Chapter 8, Neural Networks (NN) have been used for learning the corre-
sponding control surface and for extracting a reduced set of rules describing the system. The performance of the fuzzy controller with 24 rules is compared with the original 49 rules fuzzy controller in this chapter.

Finally, Chapter 9 presents the general conclusions and suggestions for further work. The advantages of using the proposed fuzzy control scheme are given in this final chapter.

Appendix A derives the mathematical model of the single-machine infinite bus power system. Appendix B introduces basic concepts of fuzzy set theory. Appendix C presents the derivation of the proposed membership function evaluation parameter Whole Overlap Ratio (WOR) for different membership functions. Appendix D includes the modelling of the multi-machine power systems. Appendix E demonstrates the input FPL (Fuzzy Programming Language) file and the generated rule base by using neural network techniques followed by the bibliography.
Chapter 2

Experimental Systems Used in the Power Laboratory

2.1 Introduction

Research into using fuzzy controllers for power system stabilisation in the Department of Electrical and Electronic Engineering at Victoria University of Technology started in 1991. The proposed fuzzy controllers have been optimised and implemented on a single-machine infinite bus and a two-machine infinite bus power system respectively. These two power systems are demonstrated in the following sections.

2.2 Single-machine Infinite Bus Power System

The circuit configuration of the single-machine infinite bus system built is as shown in Figure (2.1). The synchronous generator is a salient pole type with a damping winding on the rotor shaft and driven by a DC motor.
Chapter 2. Experimental Systems Used in the Power Laboratory

The AC generator is driven by a DC motor controlled to simulate a steam turbine. A local load has been connected to the generator terminal bus. The mechanical power output from the DC motor to drive the AC generator is set constant during the operation. Thus it is assumed that the generator has a constant mechanical power input during testing. The generator delivers the electrical output via the transmission lines to the infinite bus and the load bank depending on the operating condition. If these two powers are equal (neglecting the relatively insignificant machine losses), the generator will run at its constant synchronous speed, \( \omega_{\text{syn}} \).

If, on the contrary, a difference exists between these two powers, this difference will be used to change the kinetic energy, resulting in the swing of the rotor speed. This happens when the generator is subject to a disturbance.

The digital controller, implemented by an IBM-PC compatible system and associated with A/D and D/A interfaces, acts as the AVR and PSS on the laboratory generator system. Figure (2.2) shows an experimental single-machine infinite bus system.

The ratings of the single-machine infinite bus power system is shown in Table (2.1). The generator parameter values have been experimentally determined according to the IEEE test procedure on a 5kVA, 240V synchronous machine and shown in Table (2.2).

<table>
<thead>
<tr>
<th>DC machine (Scott)</th>
<th>5kW, 240V, 21A,1500rpm</th>
</tr>
</thead>
<tbody>
<tr>
<td>Generator (Scott)</td>
<td>5kVA, 400/415V,4 Pole,50Hz</td>
</tr>
</tbody>
</table>

Table 2.1: Ratings of the single-machine infinite bus power system

The equivalent transmission line resistance and inductance are:

\[ R_e = 0.02pu, \quad X_e = 0.4pu \]

<table>
<thead>
<tr>
<th>Generator</th>
<th>kVA</th>
<th>( x_d(\text{pu}) )</th>
<th>( x'_d(\text{pu}) )</th>
<th>( x_q(\text{pu}) )</th>
<th>( \tau_{\text{do}}(s) )</th>
<th>( H(s) )</th>
</tr>
</thead>
<tbody>
<tr>
<td>Generator (Scott)</td>
<td>5</td>
<td>1.027</td>
<td>0.479</td>
<td>0.489</td>
<td>0.345</td>
<td>1</td>
</tr>
</tbody>
</table>

Table 2.2: Generator parameters
2.3 Two-machine Infinite Bus Power System

The configuration of the two-machine infinite bus experimental power system is shown in Figure (2.3). The block diagram of the system is shown in Figure (2.4). The system consists of two units and an infinite bus with the transmission lines and associated loads.

Ratings related to the two-machine infinite bus power systems are given in Table (2.3). The generator parameters are shown in Table (2.4).

<table>
<thead>
<tr>
<th>DC Machine (Macfarlane)</th>
<th>5kW, 200V, 22.8A, 1500rpm</th>
</tr>
</thead>
<tbody>
<tr>
<td>Generator (Macfarlane)</td>
<td>5kVA, 400/415V, 4 Pole, 50Hz</td>
</tr>
<tr>
<td>DC machine (Scott)</td>
<td>5kW, 240V, 21A, 1500rpm</td>
</tr>
<tr>
<td>Generator (Scott)</td>
<td>5kVA, 400/415V, 4 Pole, 50Hz</td>
</tr>
</tbody>
</table>

Table 2.3: Ratings of the two-machine infinite bus power system

<table>
<thead>
<tr>
<th>Generator No.</th>
<th>kVA</th>
<th>$x_d (pu)$</th>
<th>$x'_d (pu)$</th>
<th>$x_q (pu)$</th>
<th>$\tau_d (s)$</th>
<th>H(s)</th>
</tr>
</thead>
<tbody>
<tr>
<td>Generator 1 (Scott)</td>
<td>5</td>
<td>1.027</td>
<td>0.479</td>
<td>0.489</td>
<td>0.345</td>
<td>1</td>
</tr>
<tr>
<td>Generator 2 (Macfarlane)</td>
<td>5</td>
<td>0.777</td>
<td>0.1003</td>
<td>0.546</td>
<td>0.643</td>
<td>0.524</td>
</tr>
</tbody>
</table>

Table 2.4: Generator parameters
Figure 2.3: The overall view of the two-machine infinite bus experimental power system
Figure 2.4: Two-machine infinite bus power system

The equivalent transmission line resistance and inductance are:

\[ R_{10} = 0.02pu \]
\[ X_{10} = 0.5pu \]
\[ R_{12} = 0.02pu \]
\[ X_{12} = 0.6pu \]
\[ R_{20} = 0.02pu \]
\[ X_{20} = 0.4pu \]
Chapter 3

Excitation Control System Design

3.1 Introduction

The role and effect of excitation control systems in improving power system stability has been given considerable attention in the last few decades. A synchronous generator or alternator is equipped with an automatic voltage regulator (AVR), which is responsible for keeping the generator output voltage constant under normal operating conditions at various load levels. With the advancement in the design of fast acting AVRs as well as the increasing complexity of large interconnected power systems, oscillations may continue for an extended period of time and even instability may occur following system disturbances. The control algorithms to overcome these problems are generally implemented using analog components.

Currently, the availability of powerful PC’s has led to their increasing use in all aspects of power control engineering. In future years, they are expected to play an even greater role in power system control schemes because of their ability in combining various tasks, on-line updating of data and providing a logical or quick decision. Thus, the application of PC-based control in power system is being increasingly used for monitoring, data acquisition and on-line control. In addition to performing the primary control functions traditionally offered by analog controls, PC-based controls have a far greater deal of flexibility and ability to implement
sophisticated control algorithms.

Most of the recent investigations of digital AVRs have been focusing on sophisticated control algorithms such as those of self-tuning and adaptive regulators. Some improvements of system performance have been reported using self-tuning regulators over that of traditional AVRs. However, in view of their large computational requirements and complexity of their software, the degree of improvement obtained needs to be examined carefully for optimum solutions.

To avoid these complexities, this project presents an effective and straightforward AVR design which can be easily implemented by computer facilities with high accuracy. The design has been carried out in the z-domain using analytical design method.

The organisation of this chapter is as follows:

The mathematical modelling of the experimental system is described in Section 3.2. In Section 3.3, discrete-time analytical design method is introduced. The design of the digital AVR using discrete time analytical design method is presented in Section 3.4. In section 3.5, the designed AVR is tested on the experimental single-machine infinite bus power system. Finally, the concluding remarks are summarised.

3.2 Mathematical Modelling of the Experimental System

Mathematical model of a synchronous machine connected to a very large power system through transmission lines is given in Appendix A for use in the design of the AVR.

The synchronous machine equations, for small perturbations about a quiescent operating condition, are summarised by the following equations (in the s domain)
[Anderson, 1977]:

\[
E_{q\Delta}' = \frac{K_3}{1 + K_3 \tau_{do} s} (E_{FD\Delta} - K_4 \delta_{\Delta}) \tag{3.1}
\]

\[
T_{e\Delta} = K_1 \delta_{\Delta} + K_2 E_{q\Delta}' \tag{3.2}
\]

\[
V_{i\Delta} = K_5 \delta_{\Delta} + K_6 E_{q\Delta}' \tag{3.3}
\]

\[
2H \dot{\omega} = T_{m\Delta} - T_{e\Delta} - T_{d\Delta} \tag{3.4}
\]

\[
T_{d\Delta} = D \omega_{\Delta} \tag{3.5}
\]

\[
\delta_{\Delta} = \omega_{\Delta} \tag{3.6}
\]

The definitions of \(K_1 - K_6\) can be found in Section A.3 of Appendix A. The resulting block diagram is shown in Figure (3.1) (with script \(\Delta\) omitted for convenience).

By designating the state variables as \(E_{q}\), \(\omega\), and \(\delta\) and the input signals as \(E_{FD}\) and \(T_{m}\), the system equations is in the desired state-space form

\[
\begin{bmatrix}
\dot{E}_{q\Delta}' \\
\dot{\omega}_{\Delta} \\
\dot{\delta}_{\Delta}
\end{bmatrix} = \begin{bmatrix}
\frac{-1}{K_3 \tau_{do}} & 0 & -\frac{K_4}{\tau_{do}} \\
-\frac{K_2}{2H} & \frac{-D}{2H} & -\frac{K_1}{2H} \\
0 & 1 & 0
\end{bmatrix} \begin{bmatrix}
E_{q\Delta}' \\
\omega_{\Delta} \\
\delta_{\Delta}
\end{bmatrix} + \begin{bmatrix}
\frac{1}{\tau_{do}} & 0 \\
0 & \frac{1}{2H} \\
0 & 0
\end{bmatrix} \begin{bmatrix}
E_{FD\Delta} \\
T_{m\Delta}
\end{bmatrix} \tag{3.7}
\]

The configuration of the single-machine infinite bus experimental power system was shown previously in Figure (2.1). The synchronous generator is a salient pole type with a damper winding on the rotor shaft and driven by a DC motor.

The generator is equipped with an AVR and an IBM PC-486 associated with
A/D and D/A converters acts as the real time controller. The synchronous generator is connected to an infinite bus (SECV grid) through a modelled short transmission line. There is a resistive load bank connected to the generator bus terminal as a local load. A system transient can be generated by a step change in the resistive, inductive or capacitive load bank, a three-phase to ground fault.

The dynamic behaviour of the generator is described by a simplified linear model.

In a practical system, the system parameters have been measured and calculated according to the IEEE test procedure for a 5kVA, 240V synchronous machine at the Power System Laboratory of Victoria University of Technology. These parameters under a nominal operating condition (real power $P = 1pu$, power factor $PF = 0.85$ lag) are shown as follows:

- $K_1 = 0.9785$
- $K_2 = 0.8461$
- $K_3 = 0.6162$
- $K_4 = 0.3616$
• $K_5 = -0.1439$

• $K_e = 0.42567$

• $M = 2H = 2 \times 1$

• $\tau_{do} = 0.345$

• $D = 4$

Here, with the exception of $K_3$, all other parameters change with load change. At some operating conditions such as for moderate to high system transfer impedances and heavy loadings, $K_5$ becomes negative. $K_1$ is decreased by increasing system and machine reactance ($X_e$).

Consideration of the single voltage-regulator loop results in the block diagram of Figure (3.2):

\[ G_v(s) = \frac{K}{1 + \tau_{do}s} \quad (3.8) \]
Where \( K \) is the DC gain and \( \tau'_{d0} \) is the open circuit d-axis time constant of the generator respectively. The transfer function between the terminal voltage and the field voltage can be represented as:

\[
G_v(s) = \frac{0.2622}{1 + 0.2126s}
\]  

(3.9)

The exciter is modelled using a field drive unit and the time constant of the unit is found to be very small compared to the significant time constant of the system under study and is therefore neglected. The transfer function of the field drive unit is:

\[
G_{FDU} = A
\]  

(3.10)

where \( A \) is the gain of the field drive unit and is found to be 25 in this case.

The three-phase line voltages are transformed to a proportional DC signal which is measured by the A/D converter. The sensor circuit, which rectifies, filters and reduces the terminal voltage to 5V for comparison, whose transfer function is found experimentally and is given by:

\[
G_s(s) = \frac{B}{1 + \tau s}
\]  

(3.11)

Again, the time constant \( \tau \) of the sensor circuit is found to be 0.015s which is neglected as it is very small compared to the machine time constant. The sensor DC gain \( B \) is found to be \( 5V/240V = 0.0208 \). If using reference voltage \( V_{ref} \) as 1pu, the sensor gain is \( 0.0208/5 = 0.0042 \).

### 3.3 Discrete-time Analytical Design Method

For the digital voltage regulator design, an analytical design method that will force the error sequence, when subjected to a specific type of time-domain input, to become zero after a finite number of sampling periods and, in fact, to become zero
Chapter 3. Excitation Control System Design

and stay zero after the minimum possible number of sampling periods, has been employed.

The error signal $e(t)$, which is the difference between the input $V_{\text{ref}}(t)$ and output $V_i(t)$, is sampled every time interval $T$. The input to the digital controller is the error signal $e(kT)$. The output of the digital controller is the control signal $u(kT)$. The control signal $u(kT)$ is fed to the zero-order hold, and the output of the hold, $u(t)$, which is a piecewise continuous-time signal, is fed to the plant (Figure 3.2). It is desired to design a digital controller $G_{AVR}(z)$ such that the closed-loop control system will exhibit the minimum possible settling time with zero steady-state error in response to a step, a ramp, or an acceleration input. It is required that the output not exhibit inter-sampling ripple after the steady state is reached. The system must satisfy any other specifications, if required.

Let us define the z transform of the plant $G_p(s)$ which is preceded by the zero-order hold as $G(z)$, or

$$G(z) = Z\left[\frac{1 - e^{-Ts}}{s}G_p(s)\right]$$

(3.12)

Then, the open-loop pulse transfer function becomes $G_{AVR}(z)G(z)$. Next, define the desired closed-loop pulse transfer function as $F(z)$:

$$\frac{V_i(z)}{V_{\text{ref}}(z)} = \frac{G_{AVR}(z)G(z)}{1 + G_{AVR}(z)B(z)} = F(z)$$

(3.13)

Since it is required that the system exhibit a finite settling time with zero steady-state error, the system must exhibit a finite impulse response. Hence, the desired closed-loop pulse transfer function must be of the following form:

$$F(z) = a_0 z^N + a_1 z^{N-1} + \cdots + a_N$$

(3.14)

or

$$F(z) = a_0 + a_1 z^{-1} + \cdots + a_N z^{-N}$$

(3.15)
where $N \geq n$ and $n$ is the order of the system. To find the pulse transfer function $G_{AVR}(z)$ that will satisfy equation (3.13), it can be obtained

$$G_{AVR}(z) = \frac{F(z)}{G(z) - BG(z)F(z)}$$

(3.16)

The designed system must be physically realisable. The conditions for physical realisability place certain constraints on the closed-loop pulse transfer function $F(z)$ and the digital controller pulse transfer function $G_{AVR}(z)$. The conditions for physical realisability may be stated as follows [Ogata, 1987]:

1. The order of the numerator of $G_{AVR}(z)$ must be equal to or lower than the order of the denominator. (otherwise, the controller requires future input data to produce the current input.)

2. If the plant $G_{p}(s)$ involves a transportation lag $e^{-Lt}$, then the designed closed-loop system must involve at least the same magnitude of the transportation lag. (Otherwise, the closed-loop system would have to respond before an input was given, which is impossible for a physically realisable system.)

3. If $G(z)$ is expanded into a series in $z^{-1}$, the lowest-power term of the series expansion of $F(z)$ in $z^{-1}$ must be at least as large as that of $G(z)$. For example, if an expansion of $G(z)$ into a series in $z^{-1}$ begins with the $z^{-1}$ term, then the first term of $F(z)$ given by equation (3.15) must be zero, or $a_0$ must equal to 0; that is, the expansion has to be of the form

$$F(z) = a_1z^{-1} + a_2z^{-2} + \cdots + a_Nz^{-N}$$

(3.17)

where $N \geq n$ and $n$ is the order of the system. This means that the plant cannot respond instantaneously when a control signal of finite magnitude is applied: the response has a delay of at least one sampling period if the series expansion of $G(z)$ begins with a term in $z^{-1}$.

In addition to the physical realisability conditions, attention must be paid to the stability aspects of the system. Specifically, to avoid cancelling an unstable pole
of the plant by a zero of the digital controller. If such a cancellation is attempted, any error in the pole-zero cancellation will diverge as time elapses and the system will become unstable. Similarly, the digital controller pulse transfer function should not involve unstable poles to cancel plant zeros which lie outside the unit circle.

Since $e(kT) = V_{ref}(kT) - V_i(kT)$, referring to equation (3.13), it can be derived that

$$E(z) = V_{ref}(z) - V_i(z) = V_{ref}(z)[1 - F(z)]$$

(3.18)

Note that for a unit step input $V_{ref}(t) = 1(t)$, $V_{ref}(z) = 1/(1 - z^{-1})$, thus

$$E(z) = \frac{1 - F(z)}{1 - z^{-1}}$$

(3.19)

### 3.4 Digital Automatic Voltage Regulator (AVR) Design

For a system transfer function $G_p(s)$, the z-domain transfer function $G(z)$ of the plant which is preceded by the zero-order hold $G_h(s)$, can be obtained as follows:

$$G(z) = Z[G_h(s)G_p(s)] = Z[\frac{1 - e^{-Ts}}{s}, A \cdot \frac{0.6162 \times 0.4256}{1 + 0.2126s}] = Z[\frac{1 - e^{-Ts}}{s}, \frac{1.2337}{s + 4.704}]$$

$$G(z) = A \cdot (1 - z^{-1}) \cdot Z[\frac{0.2623}{s} - \frac{0.2623}{s + 4.704}]$$

$$G(z) = A \cdot (1 - z^{-1})[\frac{0.2623z}{z - 1} - \frac{0.2623}{z - e^{-4.704T}}]$$

(3.20)

**Sampling frequency selection:**

Since the design of AVR is in discrete time, the choice of sampling frequency is important. The rule of thumb for choosing the sampling frequency is to have the system 'activity' with three decades of the Nyquist frequency. If the sampling rate is increased beyond this, the activity effectively gets pushed to the left (on a Bode
This should not cause any problems, however, a digital system operates with fixed point precision, hence if the sampling rate is too high, the system can experience numerical problems during computations.

On dealing with the low frequency which is of the order of a fraction of 1 Hz to a few Hz for large scale power system and to satisfy the transient criteria, the sampling time has been chosen as 25 milliseconds which gives the step response of the open loop system rise time $t_r = 0.3$ seconds. From equation (3.12) and equation (3.20), it can be obtained that:

$$G(z) = A \frac{0.029z^{-1}}{1 - 0.889z^{-1}}$$  \hspace{1cm} (3.21)

From the given system transfer function the output sequence of the system can be expected to satisfy the transient criteria. It is required that the system exhibit a finite settling time with zero steady-state error.

It is required to derive the exponential curve of the system response to an unit step input.

$$V_i(t) = U \times A \times \mathcal{L}^{-1}\left[\frac{0.2623}{s + 4.704}\right] = U \times A \times \mathcal{L}^{-1}\left[\frac{0.2623 - 0.2623}{s + 4.704}\right] = U \times A \times 0.2623(1 - e^{-4.704t}) = 240V \hspace{1cm} (3.22)$$

$U$ is the control signal which will be applied to the generator field. The terminal voltage $V_i$ is equal to $240V$ (or 1 pu) when $t$ is equal to 0.3 seconds.

$$U = \frac{240}{A \times 0.2623(1 - e^{-4.704t})} \approx 48.4V$$  \hspace{1cm} (3.23)

If the desired settling time is 0.3 seconds, the required number of the sampling period:

$$K = \frac{\text{settling time}}{\text{sampling time}} = \frac{0.3}{0.025} = 12$$  \hspace{1cm} (3.24)
Chapter 3. Excitation Control System Design

The output sequences are designed as follows:

\[ V_t(kT) = 48.4 \times A \times 0.2623(1 - e^{-4.704kT}) \]  \hspace{1cm} (3.25)

\[ V_t(0) = V_t(0) = 0V \]
\[ V_t(T) = V_t(0.025) = 35.2V \]
\[ V_t(2T) = V_t(0.05) = 66.528V \]
\[ V_t(3T) = V_t(0.075) = 94.344V \]
\[ V_t(4T) = V_t(0.1) = 119.088V \]
\[ V_t(5T) = V_t(0.125) = 141.096V \]
\[ V_t(6T) = V_t(0.15) = 160.656V \]
\[ V_t(7T) = V_t(0.175) = 178.056V \]
\[ V_t(8T) = V_t(0.2) = 193.512V \]
\[ V_t(9T) = V_t(0.225) = 207.264V \]
\[ V_t(10T) = V_t(0.25) = 219.48V \]
\[ V_t(11T) = V_t(0.275) = 230.328V \]
\[ V_t(12T) = V_t(0.3) = 240V \]

The \( z \)-transform of the output sequences is:

\[ V_t(z) = 35.2z^{-1} + 66.528z^{-2} + 94.344z^{-3} + 119.088z^{-4} + 141.096z^{-5} + 160.656z^{-6} \]
\[ + 178.056z^{-7} + 193.512z^{-8} + 207.264z^{-9} + 219.48z^{-10} + 230.328z^{-11} + 240z^{-12} \]  \hspace{1cm} (3.26)

For an unit step input \( V_{ref}(z) = 1/(1 - z^{-1}) \), then the closed-loop transfer function between \( V_t(z) \) and \( V_{ref}(z) \) is:

\[ F(z) = \frac{V_t(z)}{V_{ref}(z)} = \frac{V_t(z)}{1 - z^{-1}} = \\
35.2z^{-1} + 31.328z^{-2} + 27.816z^{-3} + 24.744z^{-4} + 22.008z^{-5} + 19.56z^{-6} \]
\[ + 17.4z^{-7} + 15.456z^{-8} + 13.752z^{-9} + 12.216z^{-10} + 10.848z^{-11} + 9.672z^{-12} \]  \hspace{1cm} (3.27)
\[ BF(z) = 0.1467z^{-1} + 0.1304z^{-2} + 0.1160z^{-3} + 0.1031z^{-4} + 0.0917z^{-5} + 0.0815z^{-6} + 0.0725z^{-7} + 0.0644z^{-8} + 0.0573z^{-9} + 0.0509z^{-10} + 0.0453z^{-11} + 0.0402z^{-12} \] (3.28)

Using equation (3.16), equation (3.21) and equation (3.27), the AVR transfer function can be easily derived as

\[ G_{AVR}(z) = \frac{F(z)}{G(z) - BG(z)F(z)} = A\frac{5.0586 - 1.2345z^{-12}}{1 - BF(z)} \] (3.29)

The terminal voltage response corresponding to a unit step input in the voltage regulator loop is shown in Figure (3.3).

![Figure 3.3: Unit step response of the voltage regulator loop](image)

### 3.5 Experimental Test Results

Figures (3.4) to (3.14) are the implementation results. Figures (3.4) (a) to (3.9) (a) show the terminal voltage response subject to 1/2 and 3/4 rated sudden in-
ductive, capacitive or resistive load changes without the AVR respectively; Figures (3.4) (b) to (3.9) (b) show the terminal voltage corresponding to 1/2 and 3/4 rated inductive, capacitive and resistive load changes with the designed AVR respectively. Figures (3.10)-(3.12) present the control signals corresponding to the above sudden load changes. Figure (3.13) demonstrates the terminal voltage and control signal corresponding to a 10% step increase in the reference voltage sustained for 7.5 seconds. Figure (3.14) shows the terminal voltage and control signal in response to a three-phase to ground fault at A (Figure 2.2) sustained for 125 milliseconds. It can be seen that the system equipped with the designed AVR kept the output constant under both small (a 10% step change in the reference voltage) and large (sudden load change and three-phase fault) disturbance conditions. Extensive tests were conducted at various operating conditions and similar results were obtained. The performance of the digital AVR is then theoretically analysed and experimentally verified in this chapter.

Figure 3.4: Terminal voltage corresponding to 1/2 sudden inductive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR
3.6 Concluding Remarks

In this chapter, the design and experimental test of an AVR is discussed. The simplified linear mathematical model of single-machine infinite bus power system is described in Section 3.2. The design of the AVR is based on this model. The discrete time analytical design method is introduced in Section 3.3. Followed by the theoretical analysis of the AVR in Section 3.4, the designed AVR has been experimentally verified in real time. The designed AVR has been tested on a single-machine infinite bus power system as shown previously in Figure (2.1) under the following disturbance conditions:

- 1/2 rated and 3/4 rated inductive step load change;
- 1/2 rated and 3/4 rated capacitive step load change;
- 1/2 rated and 3/4 rated resistive step load changes;
- a 10% step change in reference voltage;
- a three-phase to ground fault;
- at various operating conditions with the above disturbances.

The designed AVR performs satisfactorily as the AVR kept the generator output voltage constant under normal operating conditions at various load levels. The dynamic performance satisfy IEEE standard of excitation control system dynamic performance indices [IEEE, 1978]. This is confirmed by both the simulation and real time implementation.
Figure 3.5: Terminal voltage corresponding to 3/4 sudden inductive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR.

Figure 3.6: Terminal voltage corresponding to 1/2 sudden capacitive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR.
Figure 3.7: Terminal voltage corresponding to 3/4 sudden capacitive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR

Figure 3.8: Terminal voltage corresponding to 1/2 sudden resistive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR
Figure 3.9: Terminal voltage corresponding to 3/4 sudden resistive load change without and with the AVR, (a)-without AVR, (b)-with the designed AVR

Figure 3.10: Control signals corresponding to 1/2 and 3/4 sudden inductive load changes with the AVR, (a)-1/2 rated inductive load change, (b)-3/4 rated inductive load change
Figure 3.11: Control signals corresponding to 1/2 and 3/4 sudden capacitive load changes with the AVR, (a)-1/2 rated capacitive load change, (b)-3/4 rated capacitive load change

Figure 3.12: Control signals corresponding to 1/2 and 3/4 sudden resistive load changes with the AVR, (a)-1/2 rated resistive load change, (b)-3/4 rated resistive load change
Figure 3.13: Terminal voltage and control signal corresponding to a 10% step increase in the reference voltage sustained for 7.5 seconds, (a)-terminal voltage, (b)-control signal.

Figure 3.14: Terminal voltage and control signal corresponding to a three-phase to ground fault at A (Figure 2.2) sustained for 125 milliseconds, (a)-terminal voltage, (b)-control signal.
Chapter 4

Proposed Design of Two Fuzzy Control Schemes

4.1 Introduction

In this chapter, proposed design of the fuzzy logic controller (FLC) and fuzzy logic based power system stabiliser (FLBPSS) are carried out. In Section 4.2, the structure of the FLC is demonstrated and explained. Two fuzzy control schemes, i.e., the FLC and the FLBPSS are designed as PSSs in Section 4.3 and 4.4 respectively. The basic concepts of fuzzy set theory, such as fuzzy sets and terminology, fuzzy set theoretical operations, fuzzy inference and composition are included in Appendix B.

4.2 Introduction to Fuzzy Logic Controller (FLC)

4.2.1 Structure of the FLC

The essential part of the FLC is a set of linguistic control rules related by the dual concepts of fuzzy implication and the compositional rule of inference. The FLC provides an algorithm which can convert the linguistic control strategy based on expert knowledge into an automatic control strategy. Figure (4.1) shows the basic
configuration of a FLC, which comprises four principle components: fuzzification interface, knowledge base (KB), decision-making logic, and defuzzification interface [Lee, 1990a], [Lee, 1990b].

Figure 4.1: Schematic diagram of a FLC

**Fuzzification Interface:** The function of the fuzzification interface involves:

- measures the values of input variables;
- performs a scale mapping that transfers the range of values of input variables into a corresponding normalised universes of discourse (normalised domain). It also maps the normalised value of the control output variable onto its physical domain (output denormalisation). When a non-normalised domain is used then there is no need for this function;
- performs the function of fuzzification that converts input (crisp) data into suitable linguistic values which may be viewed as labels of fuzzy sets, in order to make it compatible with the fuzzy set representation of the process state variable in the rule-antecedent.

**Knowledge Base:** The knowledge base comprises a knowledge of the application domain and the attendant control goals. This knowledge is classified as the data base and linguistic control rule base. The basic function of the data base is
to provide the necessary information for the proper functioning of the fuzzification interface, the rule base, and the defuzzification interface. This information includes:

- Fuzzy sets (membership functions) representing the meaning of the linguistic values of the process (plant) state and control output variables.

- Physical domains and their normalised counterparts together with the normalisation/denormalisation (scaling) factors.

If the continuous domains of the process (plant) state and control output variables have been discretised then the data base also contains information concerning the quantisation (discretisation) look-up tables defining the discretisation policy. For the case of continuous, normalised domains the design parameters of the data base include:

- Choice of membership functions;

- Choice of scaling factors.

The rule base characterises the control goals and control policy of the domain experts by means of a set of linguistic control rules. The design parameters involved in the construction of the rule base include:

- Choice of process state and control output variables;

- Choice of the contents of the rule-antecedent and the rule-consequent;

- Choice of the term-sets (ranges of linguistic values) for the process state and control output variables;

- Derivation of the set of rules.

**Decision Making Logic:** The decision making logic is the core of a FLC. It has the capability of simulating human decision making based on fuzzy concepts and of inferring fuzzy control actions employing fuzzy implication and the rules of inference in fuzzy logic. In the context the design parameters for the decision making logic are as follows:
Chapter 4. Proposed Design of Two Fuzzy Control Schemes

- Choice of representing the meaning of a single production rule;
- Choice of representing the meaning of the set of rules;
- Choice of inference engine.

**Defuzzification Interface:** The defuzzification interface performs the following functions:

- a scale mapping, which converts the range of values of output variables into corresponding universe of discourse. This is also called *demormalisation*. This function is not needed if non-normalised domains are used.
- defuzzification yields a non-fuzzy control action from an inferred fuzzy control action.

The design parameter of the defuzzification interface is:

- Choice of defuzzification operators.

**4.2.2 Data Base**

The concepts associated with a data base are used to characterise the fuzzy control rules and the data manipulation in the FLC. Some of the aspects relating to the data base will be discussed here.

- **Discretisation/Normalisation of Universe of Discourse**

  A universe of discourse can be discrete or continuous depending on the nature of the application. Sometimes it is necessary to change a continuous universe into a discrete one. This can be achieved by discretisation. Furthermore, a continuous universe may be mapped to another universe of different range by normalisation [Lee, 1990a].
1. **Discretisation of Universe of Discourse:**

Discretisation of a Universe is often referred to quantisation. Quantisation divides an universe into a number of segments called quantisation level. Each level is labelled as a generic element. A fuzzy set can be defined by assigning grade of membership values to each generic element of the new discrete universe. A table for quick reference is formed to define the output of the controller for every possible combination of the inputs. The number of quantisation level determines the fineness of a control. In other words, the controller will be more sensitive to the observed data if the number of quantisation level increases. In most cases, fuzzy logic operations are performed on computers. Therefore, the number of quantised level should be large enough to provide an adequate approximation of the original continuous universe and yet be small enough to save memory.

Discretisation can be viewed as a scale mapping of the measured data to the discrete universe. The scaled mapping can be linear or non-linear or a combination of both. It is common that coarse resolution is used for large errors and small resolution is used for small errors. In practice, due to discretisation, the performance of a FLC is less sensitive to small deviations in the values of the state variables.

2. **Normalisation of a Universe of Discourse:**

The normalisation of a universe of discourse requires a discretisation of the universe of discourse into finite number of segments, with each segment mapped into a suitable segment of the normalised universe. A fuzzy set is then defined by assigning an explicit function to its membership function.

The number of segments of the required number of fuzzy sets is a trade-off between the accuracy and the complexity of the model. The size of the relation matrix or number of fuzzy rules increases rapidly with increasing number of fuzzy sets. Since fuzzy modelling is an attempt at developing a mathematical representation of a linguistic description of a control process, this becomes meaningless if number of fuzzy sets becomes too large. It is also difficult to put sensible labels on more than
7 fuzzy sets for a variable. The trade-off against the accuracy of the model is that number of fuzzy sets increases with an increase in accuracy. However, more information is required to be able to specify a sensible model.

The two design parameters involved in the construction of the data base are:

- Choice of membership functions;
- Choice of scaling factors.

**Membership Function of a Fuzzy Set**

Fuzzy sets are defined in two ways, numerical or functional, depending whether the universe of discourse is continuous or discrete.

1. **Numerical**

   Fuzzy sets defined by numerical method have grade of membership function as a vector of numbers whose dimension depends on the degree of discretisation.

2. **Functional**

   A functional definition expresses the membership function of a fuzzy set in a functional form, typically a bell-shaped function, triangular-shaped function, trapezoid-shaped function, etc. Such functions are used in a FLC because they lead themselves to manipulation through the use of fuzzy arithmetic. The functional definition can readily be adapted to a change of the normalisation of a universe.

Either a numerical or functional definition can be used to assign the grades of membership to the fuzzy sets. There are few guidelines exist for defining the shape of fuzzy sets. The only necessary criterion to enable the fuzzy logic to work effectively is that a set of fuzzy sets should cover the operating range of the variable. Given that the set satisfy this, the choice of the actual shape described by the membership functions is entirely subjective. It may be noted that the linguistic label of the fuzzy set implies a particular shape for the set.
Choice of Scaling Factors

The use of normalised domains (universe of discourse) requires a scale transformation which maps the physical values of the process state variables into a normalised domain. This is called the input normalisation. Furthermore, output denormalisation maps the normalised value of the control output variables into their respective physical domains.

4.2.3 Rule Base

The most important element of a FLC is the set of linguistic statements based on expert knowledge. The expert knowledge is usually described in the form of if-then rules. They can be easily implemented using fuzzy conditional statements in fuzzy logic. The collection of fuzzy conditional rules forms the rule base of a FLC.

Choice of Process State Variables and Control Variables of Fuzzy Control Rules

Identifying and choosing suitable process state variables and control variables is essential to the characterisation of the operation of a fuzzy system. The assignment of linguistic variables and their membership function also have an influence on the structure of a FLC. The process of this selection depends heavily on the experience and the control engineering knowledge. The common linguistic variables used are the state, state error, state error derivative, state deviation and its derivative, etc.

Source of Fuzzy Control Rules

There are basically four methods of deriving a fuzzy control rule base [Takagi, 1983], [Sugeno, 1985], [Lee, 1990a], [Lee, 1990b]; these approaches are not mutually exclusive and in practice a combination of these methods are likely to be utilised.

1. Expert’s experience and knowledge
Fuzzy control rules specify the necessary action to be taken if certain conditions are satisfied. Since information and problems are described in linguistic rather than numerical in daily life, it should be obvious that fuzzy control rules provide a framework for the characterisation of human behaviour and decision analysis. There are two heuristic approaches which can be used to formulate fuzzy control rules. The most common one is the verbalisation of human expertise. Another approach involves forming a prototype of fuzzy control rules by gathering information from a number of experienced experts or operators. Whilst the approach is problem domain specific, non-generic and highly subjective, it has been applied with considerable success [Sugeno, 1985], [Larsen, 1980].

2. Modelling the operator’s control actions

In many industrial man-machine applications, the transfer function of the system cannot be found using classical control theory due to the complicated structure and insufficient precision of the system. However, very often those human operators are able to monitor such systems without actually understanding the actual model of the system. Therefore, it is possible to extract fuzzy control rules by expressing the operator’s control rules using linguistic variables. In practice, rules can be deduced from the observation of human controllers actions in terms of input-output operating data [Sugeno, 1985], [Harris, 1989b].

3. Modelling a process

A linguistic description of a dynamic characteristics of a controlled process can be viewed as a fuzzy model of the process. Fuzzy control rules can then be developed based on this fuzzy model to obtain desirable performance. This approach is more complicated than others but it is more reliable and yields better results. This approach has been successfully applied to car driving by Sugeno and Nishida [Sugeno, 1985].

4. Self organisation

Many of the FLCs built so far can only imitate human decision making. It is possible to design a FLC which has the ability to create fuzzy control
rules and to modify them based on experience. Procyk and Mamdani [Procyk, 1979] described the first self organisation controller (SOC) which consists of two rule bases. One of them is the general rule base of a FLC. The other is constructed so that it has the human-like learning ability to create and to modify the general rules based on the desired overall performance of the system. An example of a fuzzy rule based which has a learning capability is Sugeno’s fuzzy car [Sugeno, 1984], [Sugeno, 1985] which can be trained to park by itself.

4.2.4 Defuzzification Strategies

Defuzzification is required because many practical control actions are crisp in nature. Defuzzification is a mapping from a space of fuzzy control actions defined over a output universe of discourse into space of non fuzzy (crisp) control actions. There is still no systematic approach to defuzzification but there are a few ways of tackling this problem which are reviewed as follows:

- **Max-procedure**

  The first and simplest method relies on choosing the control value for which the membership function attains a maximum, namely:

  \[
  \max_{u \in U} U(u) = U(u_0) \tag{4.1}
  \]

  A difficulty arises when more than one element of \( U \) possesses this maximal value and thus \( u_0 \) is not uniquely determined. For instance, one can take randomly one of the elements with the highest grade of membership, or treat their average value as the representative one (means of maximum approach), thus:

  \[
  u_0 = \frac{1}{r} \sum_{i=1}^{r} u_i \tag{4.2}
  \]
where

\[ u^i \in \{ u \in U \mid \max_{u \in U} U(u) = U(u^i) \} \]

and this set consists of "r" elements.

- **Centre-of-gravity (centroid) procedure**

  The centre of gravity of the fuzzy control \( U \) is:

  \[ u_0 = \frac{\int_u u U(u)du}{\int_U U(u)du} \]  

  (it is assumed that both the integrals exist). Here, \( u_0 \) is determined bearing in mind a surface of the fuzzy set \( U \). In comparison to the max-procedure, it can be observed that \( u_0 = g(x) \) has no switching points, but a smooth transition between the control values for different \( x \) is visible.

- **Indexed max or centre-of-gravity method**

  Both Max and Centroid methods have been modified so that \( u_0 \) is computed according to

  \[ u_0 = \arg \max_{u \in U(\alpha)} U(u) \]  

  \[ u_0 = \frac{\int_{U(\alpha)} u U(u)du}{\int_{U(\alpha)} U(u)du} \]  

  with

  \[ U(\alpha) = \{ u \in U \mid U(u) \geq \alpha \} \]

  Where \( \alpha \) forms a parameter varying as \([0, 1]\). The idea is that the threshold level \( \alpha \) allows us to eliminate in the computation of \( u_0 \) those elements of the membership function that have non-significant grades of membership function (lower than \( \alpha \)), which may cause biased results. This threshold has to be
determined with respect to disturbances in the input data and the properties of the process controlled.

### 4.2.5 Design Parameters of the FLC

In summary, consideration are needed for several principal factors in designing a FLC. The principal factors are listed below:

- fuzzification strategies and the interpretation of a fuzzification operator;
- data base:
  1. discretisation/normalisation of universes of discourse,
  2. fuzzy partition of the input and output spaces,
  3. choice of membership function of a primary fuzzy set;
- rule base:
  1. choice of process state (input) variables and control (output) variables of fuzzy control rules,
  2. source and derivation of control rules,
  3. types of fuzzy control rules (Appendix B);
- decision making logic:
  1. definition of a fuzzy implication (see definition in Appendix B),
  2. definitions of a compositional operator (see definition in Appendix B),
  3. inference mechanism (see definition in Appendix B);
- defuzzification strategies and the interpretation of a defuzzification operator.

### 4.3 Design of a FLC as a PSS

The design of the FLC as a PSS can be separated into the following four steps:
• **Step 1).** Identify inputs and outputs

Define input and control variables, that is, determine which states of the process should be observed and which control actions are to be taken. When applying a FLC as a PSS, generator speed deviation $\Delta \omega$ and acceleration $\dot{\Delta \omega}$ have been chosen as the input signals of the FLC. The generator speed deviation $\Delta \omega$ can be readily obtained. The acceleration $\dot{\Delta \omega}$ can be obtained from the speed measured at two successive sampling instants using the following equation:

$$\dot{\Delta \omega}(k) = \frac{(\Delta \omega(k) - \Delta \omega(k - 1))/\Delta T}{(\Delta \omega(k) - \Delta \omega(k - 1))/\Delta T}$$  \hspace{1cm} (4.6)

where $\Delta T$ is the sampling interval. The control variable is the output from the FLC. The control signal from the FLC is fed to the summing junction of the excitation control loop.

• **Step 2).** Define input and output membership functions

This is fuzzification step which includes three sub-steps. Fuzzification strategies and interpretation of a fuzzification operator (fuzzifier), i.e. to transform crisp data into fuzzy sets.

• **Step 2.1).** Specify universe of discourse

Experts define universe of discourse in different ways. Some specify it within a very broad context as the range of all real numbers from minus infinity to positive infinity in units of the input/output variable under consideration. Others limit the universe of discourse to the range of interest to the application at hand.

To specify a universe of discourse for inputs $\Delta \omega$ and $\dot{\Delta \omega}$, the range should be carefully considered. If a specified range is too small, regularly occurring data will be "off scale", which may impact overall system performance. This can be shown in Figure (4.2).
Chapter 4. Proposed Design of Two Fuzzy Control Schemes

Figure 4.2: Inappropriate universe of discourse

If the top end of the acceleration range (Figure 4.2 (a)) is set at 0.5 instead of 0.6 and the acceleration in the region regularly exceeds that value, the system response will depend on the hardware implementation rather than a well-designed and simulated fuzzy logic model.

Conversely, if the universe of discourse for an input is too large, which is shown in Figure (4.2) (b), the temptation will often be to have large “flat response” membership functions on the right or left to capture the extreme input values. The input will always be fuzzified to the same value for all the acceleration signal higher than 0.4.

When designing a FLC as a PSS, the universe of discourse for speed deviation has been specified to be between -0.05pu and 0.05pu. Correspondingly, the universe of discourse for acceleration has been specified to be between -0.6 and 0.6. The lower and upper limit are both specified considering the effects of both small and large perturbations on the power system.

The range of the universe of discourse for the stabilising signal output must also be carefully considered. Problems will occur if the output universe of discourse is too large. In this case, one or both extremities will be far away from the boundary of “maximum meaningfulness” as shown in Figure (4.3). As with inputs, the
Figure 4.3: Inappropriate output universe of discourse

temptation will be to have large, "flat response" membership functions at each extremity. This problem manifests itself in defuzzification. Such disproportionately large membership functions will overpower the others by lending their entire mass to the defuzzification process. A similar effect can occur when singletons are disproportionately positioned to the extreme left or right. With disproportionately large membership functions, the result of defuzzification will be strongly biased by the mass of the large membership functions. This can be shown in Figure (4.4) in which centroid defuzzification method has been used.

The universe of discourse for the stabilising output signal has been specified evenly to be between -0.8 and 0.8.

- **Step 2.2).** Scale/Normalise universe of discourse

It is usually desirable and often necessary to scale or normalise the universe of discourse of an input or output variable. For example, the speed sensor is used to measure the speed signal from the synchronous machine shaft. The output voltage range from the sensor is between -12V and +12V, representing the corresponding shaft speed or rotor angle. However, the hardware component such as the A/D converter may only be able to accept input voltage between 0 and 5V with an 8bit
Figure 4.4: Disproportionately large output membership function resolution. Scaling is thus necessary to map the measured voltage into a different range.

- **Step 2.3).** Determine number and distribution of membership functions:

  There are several issues to consider when determining the number of membership functions and their overlap characteristics. The number of membership functions is quite often odd—generally, anywhere from 3 to 9. If too few membership functions have been chosen for a given application, the response may be too lethargic and may fail to provide the output control in time to recover from a small input changes. This may cause the system to oscillate around the desired value. Too many membership functions might rapidly fire different rules for small changes in input values, resulting in large output changes which could cause system instability.

  For this FLC design, 7 membership functions have been chosen for both inputs and output.

  The most common shapes for membership functions are monotonic, triangular and trapezoidal. Occasionally, bell-shaped MF’s are used. These are used to accommodate low-cost implementation hardware. The added smoothness provided by this shape is often not discernible in control applications.
Figure (4.5) shows the proposed functional membership function for the FLC input and output respectively.

Figure 4.5: Membership functions for both condition parts and consequent parts

Either a numerical definition or functional definition may be used to assign the grades of membership function to the primary fuzzy sets. The choice of grades of membership function is used on the subjective criteria of the decision. In particular, if the measurable data is disturbed by noise, the membership functions should be sufficiently wide to reduce the sensitivity to noise. This states the issue of the fuzziness or, more accurately, the efficiency of a membership function, which affects the robustness of a FLC.

- **Step 3).** Development of the control knowledge base.

The relationship between system inputs and system outputs is important in control engineering. Fuzzy relations describe the relationship between fuzzy input variables and fuzzy output variables of a control system. The fuzzy relations are defined in forms of fuzzy conditional statement. These conditional statements form the decision rule base with a set of control decision rules. Fuzzy control rules can take one of the two basic forms:
1. State based fuzzy control rules

For a system with linguistic state variables \( s_1, s_2, \ldots, s_n \) and control \( u \), defined on universes of discourse \((S_1, S_2, \ldots, S_n)\), and \( U \) respectively; fuzzy control rules that take the system state (e.g. error, change of error) at time \( k \) and evaluates the control action at time \( k \) as a function of the system states are of the form:

\[
R_i : \text{IF } s_1 \text{ is } S_1^i \text{ AND } s_2 \text{ is } S_2^i \text{ AND } \cdots \text{ AND } s_n \text{ is } S_n^i \quad \text{THEN } u \text{ is } f_i(s_1, s_2, \ldots, s_n)
\]

for \( i = 1, 2, \ldots, n \); where \((S_i^j)\) are the linguistic values of the linguistic variables \((s_1, \ldots, s_n)\), and \( f_i \) is in general a non-linear function of the multi-input single-output (MISO) system state variables-frequency \( f_i \) is linear and in most practical applications \( f_i = U_i \) a constant linguistic control qualifier. The connective between the \( n \) rules, \( R_i \) is ALSO (includes union connectives OR and ELSE). The majority of FLC are based upon a state evaluation rule base.

2. Object evaluation fuzzy control rules

Object evaluation fuzzy control or predictive fuzzy control, predicts current and future control actions and evaluates control objectives. The control rules are formulated from observing a skilled human operator or from his experience data base, rules are of the general form:

\[
R_i : \text{IF } u \text{ is } U_i \rightarrow (s_1 \text{ is } S_1^i \text{ AND } s_2 \text{ is } S_2^i \text{ AND } \cdots \text{ AND } s_n \text{ is } S_n^i)) \quad \text{THEN } u \text{ is } U_i
\]

for \( i = 1, 2, \ldots, n \); that is a control command is inferred from an evaluation of a fuzzy control in achieving the desired system states \( \{s_j\} \). The states \( \{s_j\} \) are considered as cost criteria for assessing the fuzzy rule \( R_i \), taking linguistic values such as 'good', 'poor' or 'bad'. The most suitable control is chosen from prediction \( \{s_j\} \) corresponding to every control command \( U_i \).

FLC are effective in formulating control actions for systems that are complex, uncertain and have multiple conflicting performance criteria. Whilst the state based
fuzzy control rule base does not directly emulate control actions of human operators, its simple structure and strong mathematical basis makes it highly attractive for practical implementation. Hence, when applying a FLC as a power system stabiliser to the excitation control loop, the state based fuzzy control rule base has been utilised. The fuzzy control objective is to enhance the damping characteristics of the power system including its external system through the application of a supplementary stabilising signal to the excitation control loop. Since there are seven linguistic variables describing each of the two inputs, there are a total of 49 decision rules through all possible combination. It is convenient to present these decision rules using a decision table as shown in Table (4.1) [Hsu, 1990].

<table>
<thead>
<tr>
<th>Δω</th>
<th>PB</th>
<th>ZR</th>
<th>PS</th>
<th>PM</th>
<th>ZR</th>
<th>PS</th>
<th>PM</th>
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</thead>
<tbody>
<tr>
<td>PB</td>
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<td>PB</td>
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<tr>
<td>PM</td>
<td>NS</td>
<td>ZR</td>
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<td>PS</td>
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<td>ZR</td>
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<td>NS</td>
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<td>NM</td>
<td>NS</td>
<td>ZR</td>
<td></td>
<td></td>
</tr>
</tbody>
</table>

Table 4.1: The decision table

The abbreviation used for linguistic variables above means:

PB: Positive Big
PM: Positive Medium
PS: Positive Small
ZR: Zero
NS: Negative Small
NM: Negative Medium
NB: Negative Big

The idea of a decision table is to provide a summary of reference for given inputs. From the decision table, the control algorithm for the action to be taken using shaft speed and acceleration can be summarised as follows:

- If the speed deviation and the acceleration are Zero (in the sense of the linguistic labels), the control applied is Zero (also in the sense of the respective
linguistic label of control).

- If speed deviation is **Positive Big** and the same as the acceleration, a **Positive Big** control has to be used to reach the state in which the change of speed and the acceleration are reduced to zero. (decelerating control is achieved by applying a positive stabilising signal to the excitation loop, as the electrical output can be increased by the positive stabilising signal).

- If the speed deviation is **Negative Big** and the same holds for the acceleration, the control is set to generate a **Negative** value (i.e., **Negative Big**). (Accelerating control of the study unit can be achieved by applying a negative stabilising signal to the excitation loop, as the electrical output of the study unit can be decreased by the negative stabilising signal).

The control actions in the decision table is symmetric about the main diagonal but in opposite sign. Furthermore, if the number of linguistic variable is increased, the fineness of the control actions is also increased. However, the use of large size of linguistic variable leads to an increase in the number of rules.

- **Step 4)** Determine the stabiliser output by using defuzzification.

The output of the fuzzy controller is a fuzzy set of control. As a power plant usually requires a non-fuzzy value of control, a “defuzzification stage” is needed. The membership function for the control signal was shown previously in Figure (4.5). Different defuzzification methods (described in Section 4.2.4) often give rise to various characteristics of a fuzzy control system. Table (4.2) provides characteristics of a few typical defuzzification methods in terms of memory requirement, speed and output quality [Motorola, 1992].

### Defuzzification method | Characteristics of the crisp output
--- | ---
COG (centroid) (with singleton output membership functions) | Memory requirement[1], Speed [5], Some output fluctuations
COG (centroid) (with non-singleton output membership functions) | Memory requirement [5], Speed [1], Smooth output
Maximum | Memory requirement [2], Speed [1], Optimistic output
Means of Maximum | Memory requirement [4], Speed [3], Optimistic output

Table 4.2: Comparison of the defuzzification methods

The means of maximum and centroid defuzzification methods have been used in the design of the FLC as a PSS.

## 4.4 Design of the Proposed Fuzzy Logic Based PSS (FLBPSS)

The proposed Fuzzy Logic Based Power System Stabiliser (FLBPSS) for a synchronous generator connected to an infinite bus utilises new non-linear membership functions to determine the resultant stabilising signal. For the FLBPSS design, the synchronous generator condition can be expressed with the quantities of speed deviation and acceleration in the phase plane. The phase plane is divided into two sectors as shown in Figure (4.6) [Hiyama, 1991].

The required control strategy becomes as follows for the sample point $A_1$, $A_2$, $A_3$ in the sector $A$.

1. Slight decelerating control should be applied to the study unit at sample point $A_1$ in sector $A$ to prevent excessive shift of the speed deviation to the positive side because the generator speed is approaching the desired speed from the negative side with relatively high acceleration. Therefore, the stabilising signal should be **Positive Small** at this state.

2. Strong decelerating control should be applied to the study unit at sample point $A_2$ in sector $A$ because both the generator speed and the acceler-
Figure 4.6: Two sectors in the phase plane

...tion are relatively large at the positive side. The stabilising signal should be **Positive Big** at this state.

3. Slight decelerating control should be applied to the study unit at point $A_3$ in sector $A$ to shift the generator speed to the desired one because the study unit is already in the region of slightly higher deceleration, but the generator speed is still large at the positive side. The stabilising signal should be **Positive Small** at this state.

4. In sector $B$, the situation is completely opposite to those in sector $A$. Therefore, the control strategy should be reversed. Namely, acceleration control should be applied to the study unit. The stabilising signal should be negative in sector $B$.

The stabilising signal $U_s(t)$ is given by:

$$U_s(t) = U_s(k), \quad (4.7)$$

for $k\Delta T \leq t < (k + 1)\Delta T$ in a discrete form, where $k$ indicates the time $k\Delta T$, and $\Delta T$ represents the sample interval. The generator condition at the time $t = k\Delta T$ is given by the point $p(k)$ in the phase plane (Figure 4.6) of speed deviation and
acceleration.

\[ p(k) = \frac{[\Delta \omega(k), \Delta \omega(k) - \Delta \omega(k - 1)]}{\Delta T} \]  

(4.8)

The origin in the phase plane is the desired equilibrium point. All the control effort should be directed to moving the current condition \( p(k) \) towards the origin as quickly as possible. Angle \( \beta \) represents the position of the switching line \( L \) which separates the two sectors \( A \) and \( B \). \( \beta = 0 \) degree corresponds to the switching line placed at \( \theta_i(k) = 135 \) degrees. \( \beta \) becomes negative if the switching line \( L \) is turned clockwise from \( \theta_i(k) = 135 \) around the equilibrium point \( O \) and \( \beta \) becomes positive if the switching line \( L \) is turned anti-clockwise. Angle \( \alpha \) represents the overlap between sectors \( A \) and \( B \) and \( \alpha \) has been divided equally by the switching line \( L \).

Two new fuzzy non-linear membership functions, \( N\{\theta_i(k)\} \) and \( P\{\theta_i(k)\} \), are defined for the proposed FLBPSS as shown in Figure (4.7) to represent both the sectors \( A \) and \( B \) respectively. Figures 4.7 (a) and (b) demonstrate the membership functions corresponding to \( \alpha = 90, \beta = 0 \) degrees and \( \alpha = 30, \beta = -40 \) degrees respectively.

The term \( \theta_i(k) \) indicates the phase angle of the point \( p_i(k) \) as shown in Figure (4.6). By using these membership functions, the stabilising signal is computed as follows:

\[ U_s(k) = G(k)\left[ N\{\theta_i(k)\}U_{max} - P\{\theta_i(k)\}U_{max}\right] \]

(4.9)

\[ U_s(k) = G(k)[2N\{\theta_i(k)\} - 1]U_{max} \]

(4.10)

where

\[ P\{\theta_i(k)\} = 1 - N\{\theta_i(k)\} \]

(4.11)
The term $G(k)$ indicates the gain factor at the time $t = k\Delta T$, and $G(k)$ is given by a non-linear function as shown in Figure (4.8).

The function $P\{\theta_i(k)\}$ as shown in Figure (4.7) can be expressed as follows:
where all the angles in the above equation are in degrees. The crossover points are $\theta_0 + \alpha/2$ and $\theta_0 + 180 + \alpha/2$.

The parameters to be optimised for the optimal setting of the proposed FLBPSS are the location of the switching line L (i.e., angle $\beta$) between the positive and the negative stabilising signals, the size of the cross-sections between the sectors A and B (i.e., angle $\alpha$) and the distance parameter $D_r$ (Figure 4.6) [Hiyama, 1991]. The maximum value of the stabilising signal $U_{max}$ depends on the generating unit studied.
A performance index $J$ is specified to investigate the time optimality of the study unit. According to the values of the performance index, the optimal setting of the FLBPSS can be determined. Namely, the parameters $D_r$, $\alpha$ and $\beta$ can be adjusted to their optimal values by minimising the performance index $J$.

4.5 Concluding Remarks

The basic structure of a FLC has been described and the design of a FLC as a PSS has been developed. The generator speed $\Delta \omega$ and acceleration $\Delta \dot{\omega}$ have been chosen as the input signals of the FLC. The triangular membership function shape has been chosen for both the input and output signal and the universe of discourse has been specified. A 49 rules decision table has been developed based on the theoretical knowledge. Different defuzzification methods have been introduced and the performance have been compared in terms of memory requirement, speed, etc. However, further tuning and modification of the input and output membership functions and the decision table are necessary in order to provide better performance.

The design of the FLBPSS has been presented and two new non-linear membership functions have been proposed which differ from the ones used in the past. The FLBPSS calculates the resultant stabilising output according to the fuzzy membership functions depending on the speed $\Delta \omega$ and acceleration $\Delta \dot{\omega}$ states of the synchronous generator.

The fine tuning of the proposed FLC membership functions and the optimisation of the parameter values of the proposed FLBPSS will be discussed in detail in the next chapter.
Chapter 5

Optimisation of the Fuzzy Control Strategy

5.1 Introduction

In order to achieve the best performance for the proposed FLC and the FLBPSS, the membership functions, rules or defuzzification method and the parameter settings have to be tuned, adjusted or compared according to a performance index. Two aspects of evaluating the PSS performance are maximum transient deviation and settling time. The performance index is defined as follows:

\[ J = \sum_{k=1}^{M} [t_k \Delta \omega(k)]^2 \] (5.1)

The speed deviation \( \Delta \omega(k) \) is weighted by the discrete time \( t_k = k \Delta T \). M in equation (5.1) stands for the total data number.

Comprehensive sensitivity analysis has been carried out to assess the robustness of the proposed fuzzy controllers for changes in system parameters and under different operating conditions for both small and large perturbations. The comparison study between the proposed FLBPSS and the Self-tuned FLBPSS (STFLBPSS) [Hassan, 1992] has also been investigated. Finally, the proposed two fuzzy control
schemes have been evaluated by comparing the performance indices and the dynamic responses.

5.2 Optimisation of the FLC by Observation of Model Behaviour

5.2.1 Optimisation of the FLC using Whole Overlap Ratio (WOR)

Based on observations, the membership functions, rules or defuzzification method have to be tuned for the proposed FLC.

By adjusting the shapes of the membership functions, i.e., by altering the shapes of the fuzzy sets defining the meaning of linguistic values, the performance of the FLC can be improved. The rule of adjusting the membership function is: the greater the control required (i.e. the more sensitive the stabilising signal to input $\Delta \omega$ and $\Delta \omega$ changes), the greater the membership function density in that input region. Figure (5.1) shows the membership function for both inputs and output after tuning.

The above membership function adjustment is based on trial and error. In order to improve the efficiency, the choice of a parameter to evaluate the width selection of the membership function is needed. The absolute value of the width is not proper for this goal as it does not compare the width of the separate membership function with the number of classes and the universe of discourse. Marsh [Motorola, 1992] has proposed two indices which meet this demand: the overlap ratio and the overlap robustness. These indices evaluate the width of the membership functions through the overlap of two adjacent functions. The idea is very fruitful because it allows comparison of the scope of the separate membership function with the universe of discourse and the number of classes.

Marsh [Motorola, 1992] considered only linear membership functions and these
indices work very well in this case. Their disadvantage is that although they can be easily calculated for membership functions with the limited discourse area, they cannot be calculated for functions with the infinite discourse area, for example the exponential (Gaussian) membership function. Moreover, the first index does not depend on the membership function shape at all and the second one depends on the shape in the overlap area only.

For these reasons, the index of the Whole Overlap Ratio (WOR) has been proposed which compares the width of the individual membership function with the universe of discourse and the number of classes [Reznik and Shi, 1993]:

\[
WOR = \frac{\int_{-\infty}^{\infty} MIN(\mu_1(x), \mu_2(x))\,dx}{\int_{-\infty}^{\infty} MAX(\mu_1(x), \mu_2(x))\,dx}
\]

(5.2)

where \(\mu_1(x)\) and \(\mu_2(x)\) are two adjacent membership functions. The evaluation formulas for this index and some usual membership functions are given in Table (5.1).

\[F(x) = \frac{1}{\sqrt{2\pi}} \int_{-\infty}^{x} exp\left(-\frac{u^2}{2}\right)\,du\]

used for deriving the formulas in Table (5.1) is the cumulative distribution function of a standardised normal random variable. Values of \(x\) corresponding to values of \(F(x)\) can be found in normal distribution normal
Table 5.1: Some usual membership functions and WOR evaluation formulas

<table>
<thead>
<tr>
<th>Membership function</th>
<th>Formula</th>
<th>Whole Overlap Ratio</th>
</tr>
</thead>
<tbody>
<tr>
<td>Linear</td>
<td>( \mu(x) = 1 - \text{abs}\left(\frac{x - m}{b}\right) )</td>
<td>( \frac{1}{1 - \left(\frac{m_2 - m_1}{2}\right)^2} )</td>
</tr>
<tr>
<td>Exponential (Gaussian)</td>
<td>( \mu(x) = \exp\left[-\left(\frac{x - m}{b}\right)^2\right] )</td>
<td>( \frac{1}{\sqrt{\frac{2}{\pi}} \left(\frac{m_2 - m_1}{2}\right)} - 1 )</td>
</tr>
<tr>
<td>Quadratic</td>
<td>( \mu(x) = \text{max}\left[0, 1 - \left(\frac{x - m}{b}\right)^2\right] )</td>
<td>( \frac{2 - \left(\frac{m_2 - m_1}{2}\right) + \left(\frac{m_3 - m_1}{2}\right)^3}{2 + \left(\frac{m_2 - m_1}{2}\right) - \left(\frac{m_3 - m_1}{2}\right)^3} )</td>
</tr>
</tbody>
</table>

The detail derivation of the above formulas can be found in Appendix C.

It can be seen that the index of the WOR can be easily calculated in the cases of membership functions with the unlimited discourse area as well as in the cases of simple functions with the limited area. Also it gives us the complete information about the width of membership function comparing it with the number of classes and the area of discourse.

Table (5.2) shows the performance index corresponding to changes of both input and output membership functions WOR in response to a 10% step increase in mechanical torque \( T_m \) followed by a 10% step increase in reference voltage \( V_{ref} \) and a 10% step decrease in \( V_{ref} \). It can be seen that the FLC gives best performance when the WOR is approximately from 12% to 15%.

Table (5.3) shows the performance index corresponding to changes of both input and output membership functions WOR in response to a 20% step increase in mechanical torque \( T_m \) followed by a 20% step increase in reference voltage \( V_{ref} \) and a 20% step decrease in \( V_{ref} \). It can be seen that the FLC gives best performance when the WOR is approximately from 12% to 15%.

<table>
<thead>
<tr>
<th>WOR %</th>
<th>30.95</th>
<th>26.78</th>
<th>24.27</th>
<th>21.95</th>
<th>18.79</th>
<th>15.98</th>
<th>15.12</th>
<th>14.7</th>
</tr>
</thead>
<tbody>
<tr>
<td>J %</td>
<td>1.36</td>
<td>0.96</td>
<td>0.73</td>
<td>0.70</td>
<td>0.66</td>
<td>0.58</td>
<td>0.54</td>
<td>0.51</td>
</tr>
<tr>
<td>J %</td>
<td>0.49</td>
<td>0.48</td>
<td>0.49</td>
<td>0.50</td>
<td>0.51</td>
<td>0.59</td>
<td>0.54</td>
<td>0.56</td>
</tr>
<tr>
<td>WOR %</td>
<td>9.3</td>
<td>8.7</td>
<td>8.1</td>
<td>7.6</td>
<td>5.1</td>
<td>3.2</td>
<td></td>
<td></td>
</tr>
<tr>
<td>J %</td>
<td>0.58</td>
<td>0.60</td>
<td>0.62</td>
<td>0.65</td>
<td>0.97</td>
<td>14.35</td>
<td></td>
<td></td>
</tr>
</tbody>
</table>

Table 5.2: The performance index corresponding to changes in WOR (10% step change in \( T_m \) and \( V_{ref} \))
Chapter 5. Optimisation of the Fuzzy Control Strategy

Table 5.3: The performance index corresponding to changes in WOR (20% step change in $T_m$ and $V_{ref}$)

<table>
<thead>
<tr>
<th>WOR %</th>
<th>J %</th>
</tr>
</thead>
<tbody>
<tr>
<td>30.95</td>
<td>4.31</td>
</tr>
<tr>
<td>26.78</td>
<td>3.51</td>
</tr>
<tr>
<td>24.27</td>
<td>2.82</td>
</tr>
<tr>
<td>21.95</td>
<td>2.79</td>
</tr>
<tr>
<td>18.79</td>
<td>2.74</td>
</tr>
<tr>
<td>15.98</td>
<td>2.63</td>
</tr>
<tr>
<td>15.12</td>
<td>2.58</td>
</tr>
<tr>
<td>14.7</td>
<td>2.54</td>
</tr>
</tbody>
</table>

<table>
<thead>
<tr>
<th>WOR %</th>
<th>J %</th>
</tr>
</thead>
<tbody>
<tr>
<td>14.45</td>
<td>2.52</td>
</tr>
<tr>
<td>14.29</td>
<td>2.50</td>
</tr>
<tr>
<td>13.48</td>
<td>2.53</td>
</tr>
<tr>
<td>12.72</td>
<td>2.56</td>
</tr>
<tr>
<td>11.98</td>
<td>2.59</td>
</tr>
<tr>
<td>11.27</td>
<td>2.63</td>
</tr>
<tr>
<td>10.58</td>
<td>2.67</td>
</tr>
<tr>
<td>9.93</td>
<td>2.71</td>
</tr>
</tbody>
</table>

<table>
<thead>
<tr>
<th>WOR %</th>
<th>J %</th>
</tr>
</thead>
<tbody>
<tr>
<td>9.3</td>
<td>2.76</td>
</tr>
<tr>
<td>8.7</td>
<td>2.82</td>
</tr>
<tr>
<td>8.1</td>
<td>2.88</td>
</tr>
<tr>
<td>7.6</td>
<td>2.94</td>
</tr>
<tr>
<td>5.1</td>
<td>3.50</td>
</tr>
<tr>
<td>3.2</td>
<td>12.83</td>
</tr>
</tbody>
</table>

Table 5.3: The performance index corresponding to changes in WOR (20% step change in $T_m$ and $V_{ref}$)

The means of maximum defuzzification method has been used to obtain the performance indices in Table (5.2) and (5.3).

Based on the definitions in Appendix B, many fuzzy implication functions may be generated by utilising the triangular norms and co-norms. For example, by using the definition of the fuzzy conjunction, Mamdani's [Mamdani, 1975] mini-fuzzy implication, $R_m$, is obtained if the intersection operator is used. Larsen's product fuzzy implication, $R_l$, is obtained if the algebraic product is used. A method for computing the generalised modus ponens and the generalised modus tollens laws of inference is described in [Baldwin, 1980]. Furthermore, fuzzy implication are also produced by employing bounded product and the drastic product, etc. However, when a FLC has been employed as a PSS in this project, only Mamdani’s and Larsen’s fuzzy implication methods were adopted.

Different defuzzification methods (Chapter 4 Section 4.2) have also been evaluated using the above performance index under various WOR values with a 20% step increase in mechanical torque $T_m$.

Table (5.4) shows the performance index corresponding to changes of both input and output membership functions WOR in response to a 20% step increase in mechanical torque $T_m$. When the centroid defuzzification method was used, it can be seen that the FLC gives optimal performance when the WOR is approximately from 12.72% to 14.29%. The same results were obtained with means of maximum defuzzification method which are also shown in this table where Means stands for Means of maximum.

Table (5.5) shows the performance index corresponding to changes of both
Chapter 5. Optimisation of the Fuzzy Control Strategy

### Table 5.4: The performance index corresponding to changes in WOR with different defuzzification methods (20% step change in $T_m$)

<table>
<thead>
<tr>
<th>WOR %</th>
<th>J % (Centroid)</th>
<th>J % (Means)</th>
</tr>
</thead>
<tbody>
<tr>
<td>30.95</td>
<td>1.05</td>
<td>1.05</td>
</tr>
<tr>
<td>24.27</td>
<td>0.78</td>
<td>0.78</td>
</tr>
<tr>
<td>18.79</td>
<td>0.75</td>
<td>0.75</td>
</tr>
<tr>
<td>14.29</td>
<td>0.69</td>
<td>0.69</td>
</tr>
<tr>
<td>13.48</td>
<td>0.69</td>
<td>0.69</td>
</tr>
<tr>
<td>12.72</td>
<td>0.69</td>
<td>0.69</td>
</tr>
<tr>
<td>10.58</td>
<td>0.71</td>
<td>0.74</td>
</tr>
<tr>
<td>7.6</td>
<td>0.74</td>
<td></td>
</tr>
</tbody>
</table>

### Table 5.5: The performance index corresponding to changes in WOR with different defuzzification methods (three-phase to ground fault)

<table>
<thead>
<tr>
<th>WOR %</th>
<th>J % (Centroid)</th>
<th>J % (Means)</th>
</tr>
</thead>
<tbody>
<tr>
<td>30.95</td>
<td>40.24</td>
<td>40.24</td>
</tr>
<tr>
<td>26.78</td>
<td>40.00</td>
<td>39.89</td>
</tr>
<tr>
<td>24.27</td>
<td>39.48</td>
<td>39.39</td>
</tr>
<tr>
<td>21.95</td>
<td>39.51</td>
<td>39.40</td>
</tr>
<tr>
<td>18.79</td>
<td>39.58</td>
<td>39.43</td>
</tr>
<tr>
<td>14.29</td>
<td>39.78</td>
<td>39.48</td>
</tr>
<tr>
<td>10.58</td>
<td>39.77</td>
<td>39.51</td>
</tr>
<tr>
<td>7.6</td>
<td>39.81</td>
<td>39.61</td>
</tr>
</tbody>
</table>

From Tables (5.4) and (5.5) it can be seen that the two defuzzification methods gave the same result under small perturbation (20% step change in $T_m$) and the means of maximum defuzzification method performed better in the case of a large perturbation (three-phase to ground fault) condition. Considering the system performance under both small and large perturbations, the best WOR has been chosen as **14.29%** and the defuzzification method chosen is **Means of maximum**.

The implication method utilised to obtain the performance indices in Table (5.2)-(5.5) is **Mamdani** method.

#### 5.2.2 Sensitivity to Nominal Parameter Variations and Robustness to Operating Condition Variations

The nominal operating point of the system is considered with real power $P = 1pu$ and power factor of 0.85 (lagging). The sensitivity test was performed by changing the nominal system parameters by ±20% and under different operating conditions and perturbations (small and large). Studies have also been carried out for changes in system parameters like inertia constant $H$, the d-axis open circuit transient time constant $\tau_d$, and transmission line reactance $X_e$.

The performance indices according to $J = \sum_{k=1}^{M} [t_k \Delta \omega(k)]^2$ are obtained for
## Chapter 5. Optimisation of the Fuzzy Control Strategy

### Table 5.6: The performance index corresponding to changes in WOR (Mamdani, Centroid, 20% step increase in mechanical torque)

<table>
<thead>
<tr>
<th>WOR %</th>
<th>30.95</th>
<th>24.27</th>
<th>18.79</th>
<th>14.29</th>
<th>10.58</th>
<th>7.6</th>
<th>5.1</th>
<th>3.2</th>
</tr>
</thead>
<tbody>
<tr>
<td>J%(H = 1s)</td>
<td>1.11</td>
<td>0.70</td>
<td>0.68</td>
<td>0.62</td>
<td>0.65</td>
<td>0.71</td>
<td>0.85</td>
<td>24.60</td>
</tr>
<tr>
<td>J%(H = 1s)</td>
<td>1.05</td>
<td>0.78</td>
<td>0.75</td>
<td>0.69</td>
<td>0.71</td>
<td>0.74</td>
<td>0.85</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(H = 0.8s)</td>
<td>1.01</td>
<td>0.84</td>
<td>0.82</td>
<td>0.77</td>
<td>0.78</td>
<td>0.80</td>
<td>0.86</td>
<td>2.18</td>
</tr>
<tr>
<td>J%(τ_0 = 0.414s)</td>
<td>1.26</td>
<td>0.93</td>
<td>0.90</td>
<td>0.81</td>
<td>0.84</td>
<td>0.89</td>
<td>1.02</td>
<td>3.83</td>
</tr>
<tr>
<td>J%(τ_0 = 0.345s)</td>
<td>1.05</td>
<td>0.78</td>
<td>0.75</td>
<td>0.69</td>
<td>0.71</td>
<td>0.74</td>
<td>0.85</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(τ_0 = 0.276s)</td>
<td>0.87</td>
<td>0.65</td>
<td>0.63</td>
<td>0.58</td>
<td>0.60</td>
<td>0.62</td>
<td>0.70</td>
<td>6.96</td>
</tr>
<tr>
<td>J%(X_e = 0.48pu)</td>
<td>1.17</td>
<td>0.87</td>
<td>0.84</td>
<td>0.77</td>
<td>0.79</td>
<td>0.83</td>
<td>0.93</td>
<td>47.62</td>
</tr>
<tr>
<td>J%(X_e = 0.4pu)</td>
<td>1.05</td>
<td>0.78</td>
<td>0.75</td>
<td>0.69</td>
<td>0.71</td>
<td>0.74</td>
<td>0.85</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(X_e = 0.32pu)</td>
<td>1.02</td>
<td>0.76</td>
<td>0.73</td>
<td>0.67</td>
<td>0.69</td>
<td>0.73</td>
<td>0.83</td>
<td>2.45</td>
</tr>
</tbody>
</table>

### Table 5.7: The performance index corresponding to changes in WOR (Mamdani, Means of maximum, 20% step increase in mechanical torque)

<table>
<thead>
<tr>
<th>WOR %</th>
<th>30.95</th>
<th>24.27</th>
<th>18.79</th>
<th>14.29</th>
<th>10.58</th>
<th>7.6</th>
<th>5.1</th>
<th>3.2</th>
</tr>
</thead>
<tbody>
<tr>
<td>J%(H = 1.2s)</td>
<td>1.11</td>
<td>0.70</td>
<td>0.68</td>
<td>0.62</td>
<td>0.65</td>
<td>0.71</td>
<td>0.85</td>
<td>24.60</td>
</tr>
<tr>
<td>J%(H = 1.2s)</td>
<td>1.05</td>
<td>0.78</td>
<td>0.75</td>
<td>0.69</td>
<td>0.71</td>
<td>0.74</td>
<td>0.85</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(H = 0.8s)</td>
<td>1.01</td>
<td>0.84</td>
<td>0.82</td>
<td>0.77</td>
<td>0.78</td>
<td>0.80</td>
<td>0.86</td>
<td>2.18</td>
</tr>
<tr>
<td>J%(τ_0 = 0.414s)</td>
<td>1.26</td>
<td>0.93</td>
<td>0.90</td>
<td>0.81</td>
<td>0.84</td>
<td>0.89</td>
<td>1.02</td>
<td>3.83</td>
</tr>
<tr>
<td>J%(τ_0 = 0.345s)</td>
<td>1.05</td>
<td>0.78</td>
<td>0.75</td>
<td>0.69</td>
<td>0.71</td>
<td>0.74</td>
<td>0.85</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(τ_0 = 0.276s)</td>
<td>0.87</td>
<td>0.65</td>
<td>0.63</td>
<td>0.58</td>
<td>0.60</td>
<td>0.62</td>
<td>0.70</td>
<td>6.96</td>
</tr>
<tr>
<td>J%(X_e = 0.48pu)</td>
<td>1.17</td>
<td>0.87</td>
<td>0.84</td>
<td>0.77</td>
<td>0.79</td>
<td>0.83</td>
<td>0.93</td>
<td>47.62</td>
</tr>
<tr>
<td>J%(X_e = 0.4pu)</td>
<td>1.05</td>
<td>0.78</td>
<td>0.75</td>
<td>0.69</td>
<td>0.71</td>
<td>0.74</td>
<td>0.85</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(X_e = 0.32pu)</td>
<td>1.02</td>
<td>0.76</td>
<td>0.73</td>
<td>0.67</td>
<td>0.69</td>
<td>0.73</td>
<td>0.83</td>
<td>2.45</td>
</tr>
</tbody>
</table>

system parameter changes under different values of WOR and different implication and defuzzification methods.

Table (5.6) shows the performance index corresponding to changes of both input and output membership functions WOR in response to a 20% step increase in mechanical torque $T_m$ with system parameter variations using the Mamdani implication method and the Centroid defuzzification method. It is seen that the WOR value chosen is insensitive to system parameter changes.

Table (5.7) shows the performance index corresponding to WOR values in response to a 20% step increase in mechanical torque with $\pm 20\%$ system parameter variations using the Mamdani implication method and the Means of maximum defuzzification method.

Table (5.8) shows the performance index corresponding to WOR values in
Table 5.8: The performance index corresponding to changes in WOR (Larsen, Centroid, 20% step increase in mechanical torque)

<table>
<thead>
<tr>
<th>WOR %</th>
<th>30.95</th>
<th>24.27</th>
<th>18.79</th>
<th>14.29</th>
<th>10.58</th>
<th>7.6</th>
<th>5.1</th>
<th>3.2</th>
</tr>
</thead>
<tbody>
<tr>
<td>J%(H = 1.2s)</td>
<td>1.00</td>
<td>0.71</td>
<td>0.70</td>
<td>0.67</td>
<td>0.72</td>
<td>0.81</td>
<td>1.07</td>
<td>24.60</td>
</tr>
<tr>
<td>J%(H = 1s)</td>
<td>0.98</td>
<td>0.78</td>
<td>0.76</td>
<td>0.72</td>
<td>0.76</td>
<td>0.82</td>
<td>1.00</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(H = 0.8s)</td>
<td>0.96</td>
<td>0.84</td>
<td>0.82</td>
<td>0.79</td>
<td>0.81</td>
<td>0.85</td>
<td>0.96</td>
<td>2.18</td>
</tr>
<tr>
<td>J%(τd0 = 0.414s)</td>
<td>1.17</td>
<td>0.92</td>
<td>0.91</td>
<td>0.86</td>
<td>0.91</td>
<td>0.99</td>
<td>1.20</td>
<td>3.83</td>
</tr>
<tr>
<td>J%(τd0 = 0.345s)</td>
<td>0.98</td>
<td>0.78</td>
<td>0.76</td>
<td>0.72</td>
<td>0.76</td>
<td>0.82</td>
<td>1.00</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(τd0 = 0.276s)</td>
<td>0.81</td>
<td>0.65</td>
<td>0.63</td>
<td>0.61</td>
<td>0.69</td>
<td>0.68</td>
<td>0.80</td>
<td>6.96</td>
</tr>
<tr>
<td>J%(Xe = 0.48pu)</td>
<td>1.08</td>
<td>0.87</td>
<td>0.85</td>
<td>0.81</td>
<td>0.84</td>
<td>0.91</td>
<td>1.09</td>
<td>47.62</td>
</tr>
<tr>
<td>J%(Xe = 0.4pu)</td>
<td>0.98</td>
<td>0.78</td>
<td>0.76</td>
<td>0.72</td>
<td>0.76</td>
<td>0.82</td>
<td>1.00</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(Xe = 0.32pu)</td>
<td>0.96</td>
<td>0.76</td>
<td>0.74</td>
<td>0.71</td>
<td>0.74</td>
<td>0.81</td>
<td>0.98</td>
<td>2.45</td>
</tr>
</tbody>
</table>

Table 5.9: The performance index corresponding to changes in WOR (Larsen, Means of maximum, 20% step increase in mechanical torque)

<table>
<thead>
<tr>
<th>WOR %</th>
<th>30.95</th>
<th>24.27</th>
<th>18.79</th>
<th>14.29</th>
<th>10.58</th>
<th>7.6</th>
<th>5.1</th>
<th>3.2</th>
</tr>
</thead>
<tbody>
<tr>
<td>J%(H = 1.2s)</td>
<td>1.00</td>
<td>0.71</td>
<td>0.70</td>
<td>0.67</td>
<td>0.72</td>
<td>0.81</td>
<td>1.07</td>
<td>24.60</td>
</tr>
<tr>
<td>J%(H = 1s)</td>
<td>0.98</td>
<td>0.78</td>
<td>0.76</td>
<td>0.72</td>
<td>0.76</td>
<td>0.82</td>
<td>1.00</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(H = 0.8s)</td>
<td>0.96</td>
<td>0.84</td>
<td>0.82</td>
<td>0.79</td>
<td>0.81</td>
<td>0.85</td>
<td>0.96</td>
<td>2.18</td>
</tr>
<tr>
<td>J%(τd0 = 0.414s)</td>
<td>1.17</td>
<td>0.93</td>
<td>0.91</td>
<td>0.86</td>
<td>0.91</td>
<td>0.99</td>
<td>1.20</td>
<td>3.83</td>
</tr>
<tr>
<td>J%(τd0 = 0.345s)</td>
<td>0.98</td>
<td>0.78</td>
<td>0.76</td>
<td>0.72</td>
<td>0.76</td>
<td>0.82</td>
<td>1.00</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(τd0 = 0.276s)</td>
<td>0.81</td>
<td>0.65</td>
<td>0.63</td>
<td>0.61</td>
<td>0.69</td>
<td>0.68</td>
<td>0.80</td>
<td>6.96</td>
</tr>
<tr>
<td>J%(Xe = 0.48pu)</td>
<td>1.08</td>
<td>0.87</td>
<td>0.85</td>
<td>0.81</td>
<td>0.84</td>
<td>0.91</td>
<td>1.09</td>
<td>47.62</td>
</tr>
<tr>
<td>J%(Xe = 0.4pu)</td>
<td>0.98</td>
<td>0.78</td>
<td>0.76</td>
<td>0.72</td>
<td>0.76</td>
<td>0.82</td>
<td>1.00</td>
<td>4.70</td>
</tr>
<tr>
<td>J%(Xe = 0.32pu)</td>
<td>0.96</td>
<td>0.76</td>
<td>0.74</td>
<td>0.71</td>
<td>0.74</td>
<td>0.81</td>
<td>0.98</td>
<td>2.45</td>
</tr>
</tbody>
</table>

response to a 20% step increase in mechanical torque with ±20% system parameter variations using the Larsen implication method and the Centroid defuzzification method.

Table (5.9) shows the performance index corresponding to WOR values in response to a 20% step increase in mechanical torque with ±20% system parameter variations using the Larsen implication method and the Means of max defuzzification method.

Table (5.10) shows the performance index corresponding to a three-phase to ground fault at A (Figure 2.2) sustained for 125 milliseconds with different WOR values when different implication and defuzzification methods have been used. Here M, L and Means in Table (5.10) stands for Mamdani, Larsen and Means of maximum respectively.
Chapter 5. Optimisation of the Fuzzy Control Strategy

Table 5.10: The performance index corresponding to changes in WOR with different implication and defuzzification methods, three-phase to ground fault

<table>
<thead>
<tr>
<th>Operating condition</th>
<th>P0</th>
<th>P1</th>
<th>P2</th>
<th>P3</th>
<th>P4</th>
</tr>
</thead>
<tbody>
<tr>
<td>Real power</td>
<td>1 pu</td>
<td>0.5 pu</td>
<td>0.8 pu</td>
<td>1.2 pu</td>
<td>1.5 pu</td>
</tr>
<tr>
<td>Power factor</td>
<td>0.85 (lag)</td>
<td>0.95 (lag)</td>
<td>0.95 (lag)</td>
<td>0.95 (lag)</td>
<td>0.95 (lag)</td>
</tr>
</tbody>
</table>

Similar studies as above have also been conducted under different operating conditions. Those operating conditions are shown in Table (5.11), where P0 is the nominal operating condition used before.

Table (5.12) shows the performance index corresponding to changes of both input and output membership functions WOR in response to a 20% step increase in mechanical torque \( T_m \) under different operating conditions with the *Mamdani* implication method. It can be seen that the WOR value chosen works well under various operating conditions.

Table (5.13) shows the performance index corresponding to changes of both input and output membership functions WOR in response to a 20% step increase in mechanical torque \( T_m \) under different operating conditions with the *Larsen* implication method. It shows that the WOR value chosen also works well under different operating conditions in this case.

<table>
<thead>
<tr>
<th>WOR %</th>
<th>30.95</th>
<th>24.27</th>
<th>18.79</th>
<th>14.29</th>
<th>10.58</th>
<th>7.6</th>
<th>5.1</th>
<th>3.2</th>
</tr>
</thead>
<tbody>
<tr>
<td>J % (P0)</td>
<td>1.05</td>
<td>0.78</td>
<td>0.75</td>
<td>0.69</td>
<td>0.71</td>
<td>0.74</td>
<td>0.85</td>
<td>4.70</td>
</tr>
<tr>
<td>J % (P1)</td>
<td>1.33</td>
<td>1.07</td>
<td>1.04</td>
<td>0.97</td>
<td>1.00</td>
<td>1.04</td>
<td>1.14</td>
<td>1.81</td>
</tr>
<tr>
<td>J % (P2)</td>
<td>0.97</td>
<td>0.73</td>
<td>0.70</td>
<td>0.64</td>
<td>0.66</td>
<td>0.70</td>
<td>0.80</td>
<td>1.72</td>
</tr>
<tr>
<td>J % (P3)</td>
<td>0.96</td>
<td>0.67</td>
<td>0.64</td>
<td>0.58</td>
<td>0.60</td>
<td>0.64</td>
<td>0.75</td>
<td>37.53</td>
</tr>
<tr>
<td>J % (P4)</td>
<td>5.01</td>
<td>2.02</td>
<td>1.92</td>
<td>1.70</td>
<td>1.75</td>
<td>1.86</td>
<td>2.33</td>
<td>96.50</td>
</tr>
</tbody>
</table>

Table 5.12: Performance index corresponding to changes in WOR under different operating conditions (*Mamdani*, Means of maximum or centroid, 20% step increase in mechanical torque)
Chapter 5. Optimisation of the Fuzzy Control Strategy

Table 5.13: Performance index corresponding to changes in WOR under different operating conditions (Larsen, Means of maximum or centroid, 20% step increase in mechanical torque)

<table>
<thead>
<tr>
<th>WOR %</th>
<th>30.95</th>
<th>24.27</th>
<th>18.79</th>
<th>14.29</th>
<th>10.58</th>
<th>7.6</th>
<th>5.1</th>
<th>3.2</th>
</tr>
</thead>
<tbody>
<tr>
<td>J % (P0)</td>
<td>0.98</td>
<td>0.78</td>
<td>0.76</td>
<td>0.72</td>
<td>0.76</td>
<td>0.82</td>
<td>1.00</td>
<td>4.70</td>
</tr>
<tr>
<td>J % (P1)</td>
<td>1.26</td>
<td>1.08</td>
<td>1.06</td>
<td>1.02</td>
<td>1.05</td>
<td>1.12</td>
<td>1.25</td>
<td>1.81</td>
</tr>
<tr>
<td>J % (P2)</td>
<td>0.91</td>
<td>0.73</td>
<td>0.71</td>
<td>0.68</td>
<td>0.71</td>
<td>0.78</td>
<td>0.92</td>
<td>1.72</td>
</tr>
<tr>
<td>J % (P3)</td>
<td>0.88</td>
<td>0.67</td>
<td>0.65</td>
<td>0.62</td>
<td>0.63</td>
<td>0.73</td>
<td>0.91</td>
<td>37.53</td>
</tr>
<tr>
<td>J % (P4)</td>
<td>3.37</td>
<td>2.01</td>
<td>1.92</td>
<td>1.79</td>
<td>1.89</td>
<td>2.18</td>
<td>15.84</td>
<td>96.50</td>
</tr>
</tbody>
</table>

Table 5.14: Performance index corresponding to changes in WOR under different operating conditions (Mamdani, Centroid, three-phase to ground fault)

<table>
<thead>
<tr>
<th>WOR %</th>
<th>30.95</th>
<th>24.27</th>
<th>18.79</th>
<th>14.29</th>
<th>10.58</th>
<th>7.6</th>
<th>5.1</th>
<th>3.2</th>
</tr>
</thead>
<tbody>
<tr>
<td>J % (P0)</td>
<td>40.24</td>
<td>40.00</td>
<td>39.48</td>
<td>39.58</td>
<td>39.78</td>
<td>39.77</td>
<td>39.81</td>
<td>39.97</td>
</tr>
<tr>
<td>J % (P2)</td>
<td>28.49</td>
<td>27.50</td>
<td>27.18</td>
<td>27.23</td>
<td>27.24</td>
<td>27.27</td>
<td>27.41</td>
<td>28.52</td>
</tr>
<tr>
<td>J % (P3)</td>
<td>52.19</td>
<td>49.81</td>
<td>49.53</td>
<td>48.62</td>
<td>48.62</td>
<td>48.64</td>
<td>48.69</td>
<td>79.24</td>
</tr>
<tr>
<td>J % (P4)</td>
<td>77.23</td>
<td>71.50</td>
<td>71.88</td>
<td>73.12</td>
<td>73.39</td>
<td>73.95</td>
<td>74.97</td>
<td>166.36</td>
</tr>
</tbody>
</table>

Table (5.14) shows the performance index corresponding to changes of both input and output membership functions WOR in response to a three-phase fault under different operating conditions with the *Mamdani* implication method and *Centroid* defuzzification method. It can be seen that the WOR value chosen also works well under different operating conditions.

Table (5.15) shows the performance index corresponding to changes of both input and output membership functions WOR in response to a three-phase fault under different operating conditions with *Mamdani* implication method and *means of maximum* defuzzification method. It can be observed that the WOR value chosen also works well under different operating conditions.

<table>
<thead>
<tr>
<th>WOR %</th>
<th>30.95</th>
<th>24.27</th>
<th>18.79</th>
<th>14.29</th>
<th>10.58</th>
<th>7.6</th>
<th>5.1</th>
<th>3.2</th>
</tr>
</thead>
<tbody>
<tr>
<td>J % (P0)</td>
<td>40.24</td>
<td>39.89</td>
<td>39.39</td>
<td>39.43</td>
<td>39.48</td>
<td>39.51</td>
<td>39.61</td>
<td>39.82</td>
</tr>
<tr>
<td>J % (P2)</td>
<td>28.38</td>
<td>27.09</td>
<td>27.05</td>
<td>27.23</td>
<td>27.23</td>
<td>27.26</td>
<td>27.43</td>
<td>28.53</td>
</tr>
<tr>
<td>J % (P3)</td>
<td>51.32</td>
<td>49.33</td>
<td>49.15</td>
<td>48.46</td>
<td>48.55</td>
<td>48.66</td>
<td>48.33</td>
<td>79.83</td>
</tr>
<tr>
<td>J % (P4)</td>
<td>77.23</td>
<td>71.70</td>
<td>71.95</td>
<td>73.17</td>
<td>73.48</td>
<td>74.03</td>
<td>74.79</td>
<td>166.36</td>
</tr>
</tbody>
</table>

Table 5.15: Performance index corresponding to changes in WOR under different operating conditions (Mamdani, Means of maximum, three-phase to ground fault)
5.3 Optimal Setting of the FLBPSS Parameters and Sensitivity Analysis

5.3.1 Optimal Setting of the FLBPSS Parameters

There are several parameters to be adjusted to their optimal values for the FLBPSS. The location of the switching line $L$ (i.e., angle $\beta$) between the positive and the negative stabilising signals, the size of the cross-sections between the sectors $A$ and $B$ (i.e., angle $\alpha$) and the distance parameter $D_r$ (Figure 4.6). The maximum value of the stabilising signal $U_{\text{max}}$ depends on the generating unit to be studied.

The parameters $\alpha$, $\beta$ and $D_r$ can be adjusted to their optimal values by minimising a performance index $J$ as defined in equation (5.1).

The performance index $J$ has been studied for different values of $\alpha$, $\beta$ and $D_r$ under nominal operating condition for both small and large perturbations. Figures (5.2)-(5.5) show the performance index $J$ as a function of $\alpha$ for different values of $D_r$ and a fixed value of $\beta$ corresponds to a small perturbation of a 20% step increase in mechanical torque $T_m$. Figures (5.2)-(5.5) illustrate the performance index with $\beta = -35, \beta = -38, \beta = -40$ and $\beta = -42$ degrees respectively. Figures (5.6)-(5.9) show the performance index $J$ as a function of $\alpha$ for different values of $D_r$ and a fixed value of $\beta$ corresponds to a large perturbation of a three-phase to ground fault at $A$ (Figure 2.2) sustained for 125 milliseconds under nominal operating condition. Figures (5.6)-(5.9) illustrate the performance index with $\beta = -35, \beta = -38, \beta = -40$ and $\beta = -42$ degrees respectively.

Similar studies as above were carried out for $\pm 20\%$ changes in certain system parameters like inertia constant $H$ and open circuit time constant $\tau'_{do}$ under both small and large perturbations. As an example, for $H = 1.2s$ ($+20\%$ variation in $H$), Figures (5.10)-(5.13) show the performance index $J$ as a function of $\alpha$ for different values of $D_r$ corresponds to a small perturbation of 20% step change in mechanical torque $T_m$ with $\beta = -35, \beta = -38, \beta = -40$ and $\beta = -42$ degrees respectively. For $H = 0.8s$ ($-20\%$ variation in $H$), Figures (5.14)-(5.17) show the performance index
Chapter 5. Optimisation of the Fuzzy Control Strategy

Figure 5.2: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition for a 20% step change in mechanical torque ($\beta = -35$)

Figure 5.3: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition for a 20% step change in mechanical torque ($\beta = -38$)
Figure 5.4: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition for a 20% step change in mechanical torque ($\beta = -40$)

Figure 5.5: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition for a 20% step change in mechanical torque ($\beta = -42$)
Figure 5.6: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition in response to a three-phase to ground fault ($\beta = -35$)

Figure 5.7: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition in response to a three-phase to ground fault ($\beta = -38$)
Figure 5.8: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition in response to a three-phase to ground fault ($\beta = -40$)

Figure 5.9: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values under the nominal operating condition in response to a three-phase to ground fault ($\beta = -42$)
Figure 5.10: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm20\%$ variation in inertia constant $H$ for a $20\%$ step change in mechanical torque ($H = 1.2s, \beta = -35$)

$J$ as a function of $\alpha$ for different values of $D_r$ corresponds to a small perturbation of a $20\%$ step change in mechanical torque $T_m$ with $\beta = -35, \beta = -38, \beta = -40$ and $\beta = -42$ degrees respectively.

The minimum value of the performance index $J$ can be found easily from the above figures and plots of such figures for a large range of $\beta$ are shown in Figures (5.18) and (5.19) respectively. Figure (5.18) shows all the minima versus $\beta$ for a nominal operating point and a $\pm20\%$ change in inertia constant $H$ under a small perturbation of $20\%$ step change in mechanical torque $T_m$. Figure (5.19) shows the case for the nominal operating condition under a large perturbation of a three-phase fault.
Figure 5.11: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm 20\%$ variation in inertia constant $H$ for a $20\%$ step change in mechanical torque ($H = 1.2s, \beta = -38$)

Figure 5.12: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm 20\%$ variation in inertia constant $H$ for a $20\%$ step change in mechanical torque ($H = 1.2s, \beta = -40$)
Figure 5.13: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $\pm 20\%$ variation in inertia constant $H$ for a 20\% step change in mechanical torque ($H = 1.2s, \beta = -42$)

Figure 5.14: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and $-20\%$ variation in inertia constant $H$ for a 20\% step change in mechanical torque ($H = 0.8s, \beta = -35$)
Figure 5.15: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and -20% variation in inertia constant $H$ for a 20% step change in mechanical torque ($H = 0.8s, \beta = -38$)

Figure 5.16: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and -20% variation in inertia constant $H$ for a 20% step change in mechanical torque ($H = 0.8s, \beta = -40$)
Chapter 5. Optimisation of the Fuzzy Control Strategy

Figure 5.17: Performance index corresponding to $\alpha$ changes $J = f(\alpha)$ with different $D_r$ values and -20% variation in inertia constant $H$ for a 20% step change in mechanical torque ($H = 0.8s, \beta = -42$)

Figure 5.18: Minimum performance index corresponding to changes in $\beta$ values $J_{min} = f(\beta)$ (20% step increase in mechanical torque)
Figure 5.19: Minimum performance index corresponding to changes in $\beta$ values $J_{\text{min}} = f(\beta)$ (three-phase to ground fault)
From the above figures it can be seen that the optimal performance can be achieved with $\beta = -42$ degrees. However, it is seen that when $\beta$ decreases marginally from $-42$ degrees the performance index becomes very high resulting in system instability. In order to provide a larger stability margin $\beta$ is set to $-40$ degrees.

On further examining Figures (5.4) and (5.8) for the chosen $\beta = -40$, it is seen that for a given value of $D_r$, starting from a higher value of $\alpha$, as $\alpha$ decreases, the performance index $J$ decreases, then starts increasing and abruptly becomes very high indicating instability.

All the minima for a different $D_r$ in Figures (5.4) and (5.8) do not differ much from each other and studies also reveal that there is not much difference in the dynamic responses for such values. As an example, there is hardly any difference in the dynamic responses for two $J_{\text{min}}$ (Figure 5.4) corresponding to $D_r = 0.2$ and $0.3$. This is corroborated by a plot of the responses shown in Figure (5.20).

![System response corresponding to a 20% step change in $T_m$ under two optimal settings](image)

Figure 5.20: System response corresponding to a 20% step change in $T_m$ under two optimal settings

Figure (5.8) shows the overall minimum $J$ is achieved for the settings: $D_r = 0.6, \beta = -40$ and $\alpha = 20$. Since a value of $\alpha$ little less than 20 can provide instability
because of high value of $J$, it is safer to choose for the three-phase fault situation a value of $\alpha$ somewhat greater than 20.

Considering Figures (5.4) and (5.8) for both small and large perturbations comprehensively, the optimal parameter settings can be chosen as $D_r = 0.6$, $\beta = -40$ and $\alpha = 30$.

The optimal setting of $\alpha$, $\beta$ and $D_r$ obtained by applying large perturbations such as a three-phase fault works well for a small perturbations of 20% step change in $T_m$, and vice versa. This is verified in Figure (5.21). Figure (5.21) shows (a) the system dynamic response under a 20% step change in mechanical torque $T_m$ and (b) the response under a three-phase to ground fault sustained for 125 milliseconds.

Figure 5.21: System response corresponding to a 20% step change in $T_m$ and a three-phase to ground fault, (a)-20% step increase in mechanical torque, (b)-three-phase to ground fault
5.3.2 Robustness to Operating Condition Variations and Sensitivity to Nominal Parameter Variations

The nominal operating point of the system is considered with real power $P = 1pu$ and power factor of 0.85 (lagging) for which the optimal settings of the FLBPSS have already been determined as $D_r = 0.6$, $\beta = -40$ and $\alpha = 30$. It is intended to investigate whether this optimal setting needs to be changed with changes in system operating conditions and parameters.

The performance of the proposed FLBPSS is studied under different operating conditions given in Table (5.11). Similar procedure has been adopted as described in the last section to obtain the optimal settings of $\alpha$, $\beta$ and $D_r$ for these operating conditions. As an example, Figures (5.22)-(5.25) show the performance index $J$ as a function of $\alpha$ for different value of $D_r$ and a fixed value of $\beta$ corresponds to small and large perturbations under operating conditions P1 and P4 respectively.

![Performance Index Graph](image)

Figure 5.22: Performance index corresponding to changes in $\alpha$ $J = f(\alpha)$ with different $D_r$ values in response to a 20% step increase in $T_m$ under operating condition P1 ($\beta = -40$)

The optimal settings of $\alpha$, $\beta$ and $D_r$ for these operating conditions are given
Figure 5.23: Performance index corresponding to changes in $\alpha$ $J = f(\alpha)$ with different $D_r$ values in response to a three-phase fault under operating condition P1 ($\beta = -40$)

Figure 5.24: Performance index corresponding to changes in $\alpha$ $J = f(\alpha)$ with different $D_r$ values in response to a 20% step increase in $T_m$ under operating condition P4 ($\beta = -40$)
Chapter 5. Optimisation of the Fuzzy Control Strategy

Three phase fault (P=1.5pu)

40 60 80 100

Angle alpha (beta=-40)

120 140

Figure 5.25: Performance index corresponding to changes in $\alpha J = f(\alpha)$ with different $D_r$ values in response to a three-phase fault under operating condition P4 ($\beta = -40$)

Table 5.16: Optimal settings of the FLBPSS for different operating conditions in Table (5.16).

Studies reveal that the optimal values of $\alpha$, $\beta$ and $D_r$ obtained at the nominal operating condition works well for wide variation in the operating conditions under both small or large perturbations. As an example, Figures 5.26(a) and 5.26(b) give system responses for an operating condition P4 with its optimal setting of $\alpha = 20$, $\beta = -40$ and $D_r = 0.6$ (solid line) and the nominal optimal setting of $\alpha = 30$, $\beta = -40$ and $D_r = 0.6$ (dashed line) for a small perturbation of 20% step change in mechanical torque and a large perturbation of three-phase fault at A (Figure 2.2) sustained for 125 milliseconds respectively.

Similar studies as aforementioned were carried out for $\pm 20\%$ changes in certain
system parameters like inertia constant $H$ and open circuit time constant $\tau_{do}$ under both small and large perturbations. Examination of the dynamic responses reveal that the nominal optimal setting of $\alpha$, $\beta$ and $D_r$ need not be changed following such changes in system parameters. As an example for $H = 1.2s$, Figure 27(a) provides the dynamic responses under 20% change in mechanical torque and Figure 27(b) provides the responses for a three-phase fault corresponding to both nominal operating setting and the corresponding optimal setting.

Figure (5.28) shows the system response corresponding to a three-phase fault at A (Figure 2.2) sustained for 125 milliseconds under different operating conditions using nominal optimal setting. Figure (5.28) (a) are the results under operating condition P0, P1, P2 and P4 with the proposed FLBPSS. The system response under operating condition P3 with and without the FLBPSS are shown in Figure (5.28) (b).

Figure (5.29) (a) and (b) shows the system response with ±20% change in inertia constant $H$ and d-axis open circuit transient time constant $\tau_{do}$ respectively for a 20% step increase in $T_m$ using the nominal optimal setting.

5.4 Comparison of the Proposed FLBPSS and Hassan’s Self-tuned FLBPSS

5.4.1 Review of Hassan’s Self-tuned FLBPSS (STFLBPSS)

Hassan et al [Hassan, 1992], [Hassan, 1993a], [Hassan, 1993b] have suggested a self-tuned FLBPSS (STFLBPSS) whose performance has been shown to be better than that of the FLBPSS proposed by Hiyama et al [Hiyama, 1991]. In this work, it is intended to compare the performance of the proposed FLBPSS with that of the STFLBPSS of Hassan et al.

The significant differences in the design concept of the STFLBPSS and the proposed FLBPSS are the following:
1. The proposed FLBPSS uses different membership functions (Figure 4.7) than those used by Hassan et al (Figure 5.30) [Hassan, 1992];

The membership functions shown in Figure (5.30) are defined below:

\[ S(x; a, b, c) = \begin{cases} 
0.0 & \text{for } x \leq a \\
2[(x - a)/(c - a)]^2 & \text{for } a < x \leq b \\
1 - 2[(x - c)/(c - a)]^2 & \text{for } b < x < c \\
1 & \text{for } x \geq c 
\end{cases} \] (5.3)

\[ \Pi(x; B, C) = \begin{cases} 
S(x; C - B, C - B/2, C) & \text{for } x \leq C \\
1 - S(x; C, C + B/2, C + B) & \text{for } x > C 
\end{cases} \] (5.4)

The membership functions \( P\{\theta_i(k)\} \) and \( N\{\theta_i(k)\} \) are expressed in terms of the above membership functions:

\[ P\{\theta_i(k)\} = \Pi(\theta, 2\pi - \theta_0, \theta_m) \] (5.5)

\[ N\{\theta_i(k)\} = \begin{cases} 
1 - S(x; \theta_0, \theta_{m1}, \theta_m) & \text{for } x \leq \theta_m \\
S(x; \theta_m, \theta_{m2}, 2\pi) & \text{for } x > \theta_m 
\end{cases} \] (5.6)

where \( \theta_m = (2\pi + \theta_0)/2, \theta_{m1} = (\theta_0 + \theta_m)/2, \) and \( \theta_{m2} = (2\pi + \theta_m)/2. \)

2. The proposed FLBPSS uses acceleration \( \Delta \omega \) as one of the input signal to the PSS whereas Hassan et al use \( \Delta \omega \) multiplied by a scaling factor \( F_a \):

3. In the proposed FLBPSS, \( D_r \) is optimised in a complete different manner than being self-tuned according to a strategy discussed by Hassan et al;

The value of \( D_r \) will be self tuned according to the amount of disturbance. A starting value \( D_{r0} \) will be assigned to \( D_r \) at the initialisation of the FLBPSS. The parameter \( D(k) \) in the phase plane as shown in Figure (4.6) will be calculated at each sampling time and compared to \( D_r \). If the value of \( D(k) \) will be less than \( D_r \), the value of \( D_r \) will be the same
as mentioned previously, otherwise, the value of $D_r$ will be chosen as:

$$D_r = 1.01(\max(D(k)))$$  \hspace{1cm} (5.7)

4. The proposed FLBPSS optimises the parameters $\alpha$ and $\beta$ (discussed in Section 5.3) whereas Hassan et al considered optimisation of $\theta$ and $F_a$ for the STFLBPSS [Hassan, 1992].

5.4.2 Optimal Setting of the STFLBPSS Parameters

The optimal settings of the STFLBPSS parameters are also evaluated by using the performance index as defined in equation (5.1). There are three parameters which need to be adjusted to their optimal values namely angle $\theta$, initial distance parameter $D_{r0}$ and scaling factor $F_a$. Studies reveal that at any operating point, the optimal values of $\theta$, $D_{r0}$ obtained by applying small perturbations of a 20% step change in $T_m$ differs from the ones for large perturbations such as a three-phase fault, and vice versa. Considering the system performance under different operating conditions with different perturbation (small or large) and system parameter variations, a compromise values of $\theta$ and $D_{r0}$ were chosen as 105 degrees and 0.7 respectively (the optimisation procedure is not shown here). For the chosen $\theta$ and $D_{r0}$, the performance index was also evaluated with different values of $F_a$. The optimal value of $F_a$ is found to be 0.8.

5.4.3 Comparison of the Performance Index

In order to compare the performance of the proposed FLBPSS and Hassan’s STFLBPSS, the following procedure is adopted:

For the system studied, we determine the optimal setting of $\alpha, \beta$ and $D_r$ parameters according to the strategy discussed in Section 5.3 for the nominal operating condition, and keep this setting the same for all other operating conditions as justified by the sensitivity analysis performed in Section 5.3.2. However, in STFLBPSS
Chapter 5. Optimisation of the Fuzzy Control Strategy

Table 5.17: Comparison of the performance index (small perturbation of a 20% step change in mechanical torque $T_m$)

<table>
<thead>
<tr>
<th>Operating Condition</th>
<th>P0</th>
<th>P1</th>
<th>P2</th>
<th>P3</th>
<th>P4</th>
</tr>
</thead>
<tbody>
<tr>
<td>J % (Proposed FLBPSS)</td>
<td>0.19</td>
<td>0.31</td>
<td>0.17</td>
<td>0.16</td>
<td>0.29</td>
</tr>
<tr>
<td>J % (STFLBPSS)</td>
<td>0.31</td>
<td>0.40</td>
<td>0.25</td>
<td>0.25</td>
<td>0.69</td>
</tr>
</tbody>
</table>

Table 5.18: Comparison of the performance index (large perturbation of a three-phase fault at A of Figure (2.2) sustained for 125 milliseconds)

<table>
<thead>
<tr>
<th>Operating Condition</th>
<th>P0</th>
<th>P1</th>
<th>P2</th>
<th>P3</th>
<th>P4</th>
</tr>
</thead>
<tbody>
<tr>
<td>J% (FLBPSS)</td>
<td>13.67</td>
<td>5.73</td>
<td>9.43</td>
<td>15.00</td>
<td>24.50</td>
</tr>
<tr>
<td>J% (STFLBPSS)</td>
<td>17.46</td>
<td>5.74</td>
<td>10.10</td>
<td>17.22</td>
<td>33.84</td>
</tr>
</tbody>
</table>

the optimal $\theta$, $F_a$ and $D_{ro}$ for different operating conditions are self-tuned according to the procedure of Hassan et al [Hassan, 1992]. The performance index according to $J = \sum_{k=1}^{M} [t_k \Delta \omega(k)]^2$ is obtained for different operating conditions for both FLBPSS and STFLBPSS under small and large perturbations (Tables 5.17 and 5.18). From the performance index, it is evident that the proposed FLBPSS performs better than the STFLBPSS.

Similar studies as aforementioned have also been carried out for changes in system parameters like inertia constant $H$, open circuit field time constant $\tau_d$, and transmission line reactance $X_e$. Investigations reveal that the proposed FLBPSS performs better than the STFLBPSS which is evident from Tables (5.19)-(5.22) by comparing the $J$ values.

### 5.4.4 Comparison of the Dynamic Response

A few typical responses for different operating conditions P1-P4 are provided in this section.

Figures (5.31) (a) and (b) show the system responses corresponding to a 20%
Chapter 5. Optimisation of the Fuzzy Control Strategy

<table>
<thead>
<tr>
<th>Parameters</th>
<th>$H = 1.2s$</th>
<th>$H = 1s$</th>
<th>$H = 0.8s$</th>
</tr>
</thead>
<tbody>
<tr>
<td>J% (FLBPSS)</td>
<td>12.51</td>
<td>13.67</td>
<td>17.21</td>
</tr>
<tr>
<td>J% (STFLBPSS)</td>
<td>16.56</td>
<td>17.46</td>
<td>20.57</td>
</tr>
</tbody>
</table>

Table 5.20: Comparison of the performance index for parameter changes (large perturbation of a three-phase fault at A of Figure (2.2) sustained for 125 milliseconds)

<table>
<thead>
<tr>
<th>Parameters</th>
<th>$\tau'_{do} = 0.414s$</th>
<th>$\tau'_{do} = 0.276s$</th>
<th>$X_e = 0.48pu$</th>
<th>$X_e = 0.32pu$</th>
</tr>
</thead>
<tbody>
<tr>
<td>J% (FLBPSS)</td>
<td>0.20</td>
<td>0.18</td>
<td>0.21</td>
<td>0.18</td>
</tr>
<tr>
<td>J% (STFLBPSS)</td>
<td>0.31</td>
<td>0.32</td>
<td>0.39</td>
<td>0.27</td>
</tr>
</tbody>
</table>

Table 5.21: Comparison of the performance index (small perturbation of a 20% step change in mechanical torque $T_m$)

step change in $T_m$ and a three-phase to ground fault under nominal operating condition with the proposed FLBPSS and the STFLBPSS respectively.

Figures (5.32) (a-d) show the system response corresponding to a 20% step increase in $T_m$ under different operating conditions P1-P4 respectively. Figures (5.33) (a-d) show the system response corresponding to a three-phase to ground fault at A (Figure 2.2) sustained for 125 milliseconds under different operating conditions P1-P4 respectively.

Figure (5.34) shows the system response corresponding to a 20% step change in $T_m$ with ±20% variations in inertia constant $H$. Figure (5.34) (a) shows the response with the proposed FLBPSS and STFLBPSS respectively when $H$ has been increased by 20% and Figure (5.34) (c) is the result when $H$ has been decreased by 20%. Figure (5.34) (b) is the response with no variation in $H$.

Figure (5.35) shows the system response corresponding to a 20% step change in $T_m$ with a ±20% variation in d-axis open circuit time constant $\tau'_{do}$. Figure (5.35) (a) shows the response with the proposed FLBPSS and STFLBPSS when $\tau'_{do}$ has been increased by 20% and Figure (5.35) (c) is the result when $\tau'_{do}$ has been decreased by 20%. Figure (5.35) (b) is the response with no variation in $\tau'_{do}$.

<table>
<thead>
<tr>
<th>Parameters</th>
<th>$\tau'_{do} = 0.414s$</th>
<th>$\tau'_{do} = 0.276s$</th>
<th>$X_e = 0.48pu$</th>
<th>$X_e = 0.32pu$</th>
</tr>
</thead>
<tbody>
<tr>
<td>J% (FLBPSS)</td>
<td>15.75</td>
<td>12.37</td>
<td>12.69</td>
<td>16.56</td>
</tr>
<tr>
<td>J% (STFLBPSS)</td>
<td>16.56</td>
<td>17.96</td>
<td>18.31</td>
<td>19.48</td>
</tr>
</tbody>
</table>

Table 5.22: Comparison of the performance index (large perturbation of a three-phase fault at A of Figure (2.2) sustained for 125 milliseconds)
Figure (5.36) shows the system response corresponding to a 20% step change in \( T_m \) with \( \pm 20\% \) variations in the transmission line reactance \( X_e \). Figure (5.36) (a) shows the response with the proposed FLBPSS and STFLBPSS respectively when \( X_e \) has been increased by 20\% and Figure (5.36) (c) is the result when \( X_e \) has been decreased by 20\%. Figure (5.36) (b) is the response with no variation in \( X_e \).

It is clearly seen from the above figures that the maximum transient deviation for both the FLBPSS and STFLBPSS are more or less the same, whereas the settling time for the proposed FLBPSS is much faster than that for the STFLBPSS.

### 5.5 Comparison Study of the Two Fuzzy Control Schemes

#### 5.5.1 Comparison of the Performance Index

The performance indices according to \( J = \sum_{k=1}^{M} [t_k \Delta \omega(k)]^2 \) are obtained for different operating conditions for both the proposed FLBPSS and FLC under both small and large perturbations.

Table (5.23) shows the performance index for the two fuzzy control schemes for different operating conditions under a 20\% step increase in mechanical torque \( T_m \).

<table>
<thead>
<tr>
<th>Fuzzy controller</th>
<th>P0</th>
<th>P1</th>
<th>P2</th>
<th>P3</th>
<th>P4</th>
</tr>
</thead>
<tbody>
<tr>
<td>J% (FLC)</td>
<td>0.42</td>
<td>0.64</td>
<td>0.39</td>
<td>0.35</td>
<td>0.89</td>
</tr>
<tr>
<td>J% (FLBPSS)</td>
<td>0.19</td>
<td>0.31</td>
<td>0.17</td>
<td>0.16</td>
<td>0.29</td>
</tr>
</tbody>
</table>

Table 5.23: Comparison of the performance index of the FLC and the FLBPSS (small perturbation of a 20\% step increase in mechanical torque)

Table (5.24) shows the performance index for the two fuzzy control schemes for different operating conditions under a three-phase fault.

From these tables it can be seen that the FLBPSS provides better performance than the FLC since the performance index for the FLBPSS is much smaller than...
Table 5.24: Comparison of the performance index of the FLC and the FLBPSS (large perturbation of a three-phase to ground fault)

<table>
<thead>
<tr>
<th>Fuzzy controller</th>
<th>P0</th>
<th>P1</th>
<th>P2</th>
<th>P3</th>
<th>P4</th>
</tr>
</thead>
<tbody>
<tr>
<td>J% (FLC)</td>
<td>39.48</td>
<td>13.58</td>
<td>27.23</td>
<td>48.46</td>
<td>73.17</td>
</tr>
<tr>
<td>J% (FLBPSS)</td>
<td>13.67</td>
<td>5.73</td>
<td>9.43</td>
<td>15.00</td>
<td>24.50</td>
</tr>
</tbody>
</table>

the performance index for the FLC. As an example, the performance index for the FLC under operating condition P0 is 2.2 times and 2.8 times larger than that of the FLBPSS for small and larger perturbations respectively.

5.5.2 Comparison of the Dynamic Response

Comparison of the dynamic responses for the FLBPSS and the FLC for different operating conditions P1-P4 under both small and large perturbations have been studied in this section. A few typical responses for operating condition P0 are provided in Figures (5.37)-(5.39). Figures (5.38)-(5.39) show the system dynamic performance under a 20% step change in mechanical torque $T_m$ followed by a 20% step increase in reference voltage $V_{ref}$ sustained for 7.5 seconds with the proposed FLBPSS and the FLC respectively. To demonstrate the effectiveness of the FLBPSS and the FLC, Figure (5.37) shows the speed deviation and rotor angle responses without the PSS in operation. It is clearly seen that the FLBPSS provides much better dynamic responses than the FLC since the maximum transient deviation and settling time are both smaller with the FLBPSS in operation.

5.6 Concluding Remarks

In this chapter, the optimisation of the FLC and the FLBPSS have been investigated and a performance index has been defined for this purpose.

The WOR has been proposed to evaluate the membership function shape for the FLC. It has been found that the FLC gives best performance when the WOR is approximately from 12% to 15%. Different implication methods, such as Mamdani and Larsen methods, and different defuzzification methods, such as Means of max
Chapter 5. Optimisation of the Fuzzy Control Strategy

and Centroid methods, have also been evaluated by using the performance index. Sensitivity test of the FLC has been demonstrated by varying the system parameters for ±20% and for various operating conditions under both small and large perturbations.

The optimal setting of the proposed FLBPSS parameters has also been evaluated by using the performance index. Two new non-linear membership functions have been proposed. The optimal settings of the FLBPSS parameters $\alpha$, $\beta$ and $D_r$ have been obtained either by applying small or large perturbations. The optimal setting chosen at the nominal operating condition is quite robust and need not be reset for a wide variation of operating conditions and parameters under both small and large perturbations. The optimal values of $\alpha$, $\beta$ and $D_r$ at one optimal point is sub-optimal at the other point with hardly any difference in the quality of the dynamic response.

STFLBPSS has also been introduced in order to compare with the FLBPSS. The optimal settings of $\theta$, $F_a$ and $D_{r_0}$ values have also been explored. It has been found that at any operating point, the optimal values of the above mentioned parameters obtained by applying small perturbations differ from that for large perturbations and vice versa. Considering the system performance under different operating conditions with different perturbations and the system parameter variations, a compromise values of $\theta$, $F_a$ and $D_{r_0}$ have been chosen.

Comparison study between the proposed FLBPSS and the STFLBPSS has been demonstrated through both the performance index and the dynamic response. Extensive study has been performed when the system is subject to small or large disturbances, variations in the system parameters and under wide variation of the operating conditions. The performance of the proposed FLBPSS is found to be superior to that of the STFLBPSS.

Comparison study between the proposed FLBPSS and the FLC has also been investigated through both the performance index and the dynamic response. Extensive study has been performed when the system is subject to small or large disturbances, variations in the system parameters and under wide variation of the
operating conditions. The performance index of the FLC is more than twice larger than that of the FLBPSS. From the dynamic response, it can be seen that the maximum transient deviation is smaller and the settling time is shorter when the system is equipped with the FLBPSS. Therefore, the FLBPSS has been chosen as the practical PSS for real time implementation.
Figure 5.26: System responses at operating condition P4 with the corresponding optimal settings (COS) and the nominal optimal settings (NOS), (a)-20% step increase in mechanical torque, (b)-three-phase to ground fault

Figure 5.27: System responses at P0 with inertia constant parameter variation $H = 1.2\text{s}$ with the corresponding optimal settings (COS) and the nominal optimal settings (NOS), (a)-20% step increase in mechanical torque, (b)-three-phase to ground fault
Chapter 5. Optimisation of the Fuzzy Control Strategy

Figure 5.28: System response corresponding to three-phase to ground fault under different operating conditions with the nominal optimal settings (NOS), (a)-operating conditions P0, P1, P2 and P4, (b)-operating condition P3

Figure 5.29: System response corresponding to a 20% step increase in mechanical torque with the nominal optimal settings (NOS) for different system parameter changes, (a)-±20% variation in $H$, (b)-±20% variation in $\tau_{d0}'$.
Chapter 5. Optimisation of the Fuzzy Control Strategy

Figure 5.30: Membership functions used for the STFLBPSS

Figure 5.31: System response corresponding to a 20% step change in mechanical torque and a three-phase fault under the nominal operating condition, (a)-20% step increase in mechanical torque, (b)-three-phase fault
Figure 5.32: System response corresponding to a 20% step change in mechanical torque under different operating conditions, (a)-(d) provide the speed deviation responses under operating conditions P1-P4 respectively.

Figure 5.33: System response corresponding to a three-phase to ground fault under different operating conditions, (a)-(d) provide the speed deviation responses under operating conditions P1-P4 respectively.
Figure 5.34: System response corresponding to a 20% step change in mechanical torque with ±20% variation in inertia constant $H$, (a) $H = 1.2s$, (b) $H = 1s$, (c) $H = 0.8s$

Figure 5.35: System response corresponding to a 20% step change in mechanical torque with ±20% variation in $r^o$, (a) $r^o = 0.414s$, (b) $r^o = 0.345s$, (c) $r^o = 0.276s$
Figure 5.36: System response corresponding to a 20% step change in mechanical torque with ±20% variation in $X_e$, (a) $X_e = 0.48pu$, (b) $X_e = 0.4pu$, (c) $X_e = 0.32pu$

Figure 5.37: System response corresponding to a 20% step change in mechanical torque and reference voltage change (without PSS)
Figure 5.38: System response corresponding to a 20% step change in mechanical torque and reference voltage change (with the FLC)

Figure 5.39: System response corresponding to a 20% step change in mechanical torque and reference voltage change (with the FLBPSS)
Chapter 6

Implementation Study

6.1 Introduction

In order to verify the design for the optimised FLBPSS as well as the simulation results, the digital AVR and the FLBPSS were implemented and tested on the single-machine infinite bus system in the power laboratory. The configuration of the single-machine infinite bus power system was shown previously in Figures (2.1) and (2.2). The synchronous generator is a salient pole type with a damping winding on the rotor shaft and driven by a DC motor. The generator was synchronised and connected to the infinite bus.

The implementation of the optimised FLBPSS is tested on the single-machine infinite bus power system. The hardware development is described in Section 6.2. The sensor circuit which has been used to transform the three-phase line voltages of 400V into a reduced magnitude proportional DC signal is presented in Section 6.2.1. In Section 6.2.2 and 6.2.3, the A/D and D/A converter and the field drive unit are described. An optical shaft encoder which has been used for rotor position measurement is described in detail in Section 6.2.4. The software development is presented in Section 6.3 which includes a description of the main program, the driver routines, the interrupt set up and the handling routine, the AVR routine and the FLBPSS as well as other features. The flow chart of the software is illustrated in Section 6.3.7.
The implementation test results are presented in Section 6.4. In order to test the robustness of the optimised FLBPSS, three kinds of disturbances were applied to the system, a 10% step change in the reference voltage as a small perturbation, a sudden load change and a three-phase to ground fault as large perturbations. The real time evaluation has also been tested under a wide range of operating conditions which is also shown in Section 6.4.

6.2 Hardware Development

6.2.1 Sensor

The three-phase line voltages of 400V are transformed into DC by a six-pulse three-phase rectifier circuit. The rectified voltage is reduced to 5V using a potential divider and then filtered to get a smooth DC voltage, which is the input to an A/D converter. The transducer output, a voltage between 0V and 5V, which represents a phase to phase voltage input between 0V and 400V, is fed directly into the multiplexer of the A/D converter. Figure (6.1) shows the rectifier, the potential divider and the filter circuit.

![Sensor circuit of rectifier, potential divider and filter circuit](image)

Figure 6.1: Sensor circuit of rectifier, potential divider and filter circuit
6.2.2 A/D and D/A Adapter

The IBM data acquisition adapter card is used for all A/D and D/A functions. A DT2801 card has been used as the means to perform A/D and D/A conversions. The data acquisition adapter which provides eight analog input channels multiplexed into an Analog to Digital converter and two analog output channels, all with 12 bit resolution.

6.2.3 Field Drive Unit

The field drive unit is used to model the exciter circuit. The control signal from the computer was sent out at each sample time through the D/A converter and amplified by the field drive unit to obtain the generator field voltage.

6.2.4 Rotor Position Measurement by Using an Optical Shaft Encoder

The machine is fitted with an incremental type position encoder which generates 720 pulses per revolution for a 4 pole machine. It implies 360 pulses per 360 electrical degrees, or 1 electrical degrees per pulse. By counting the number of pulses the amount of incremental movement can be accurately measured. The pulses were sent to an 8 bit hardware counter to keep track of the rotor position. A reference pulse is provided by the encoder to enable a reference position to be obtained. This occurs once per revolution in the rotary encoder. Direction can be detected enabling up/down counting to take place with regard to the reference counting.

The digital signal is then passed through a hardware D/A converter to produce a voltage signal which is proportional to the rotor position angle. The calibration test revealed that 1V is equivalent to 5 mechanical degrees or 10 electrical degrees. The computer reads the rotor position through the A/D converter and enables calculation of the speed deviation and acceleration at each sampling period.
6.3 Software Development

The functions of the PC and A/D, D/A converters are to read the terminal voltage and rotor angle, calculate the speed deviation and acceleration signal, compute the stabilising signal and excitation control signal. The excitation control signal has hence been amplified by the field drive unit to control the field voltage. The software used to achieve these objectives was arranged as a background Main program which provided the user interface, an interrupt routine which handled interrupts from the internal timer.

Turbo Pascal version 5.0 has been used as the programming language to implement the AVR and the FLBPSS. The DT2801 card was used as the means to perform the A/D and D/A conversions. Other necessary units such as the DT2801 drivers, graphics drivers etc. were incorporated in the program. Assembly language was used for the DT2801 A/D and D/A converter in order to achieve optimum conversion speed.

6.3.1 The Main Program

In the main program, the initialisation part of the program initialised the timer for a designed sampling rate of 25 milliseconds and also initialised the A/D and D/A ports. Once initialisation was completed, A/D conversions were performed on the data obtained. The initialisation procedure was included as a subroutine in the background main program.

The analog inputs, i.e., the terminal voltage, the rotor position, the real power and reactive power, etc. were obtained via the A/D converter. The results were stored in memory locations ready for use by the appropriate interrupt routine as required.
6.3.2 The Driver Routines

A separate unit called DT2801 contained all the necessary driver routines for the DT2801 card. Procedures AD-READ and DA-WRITE were used to perform the following functions:

1. Stop and reset the A/D converter;
2. Read the terminal voltage and rotor angle and convert them into digital signal;
3. Convert the calculated control signal into analog form and send it out to the field drive unit.

6.3.3 The Interrupt Set up and Handling Routines

The system timer and interrupt routines were used for the purpose of interrupting the software at each sampling instant. The interrupt was initialised at the beginning of the program and was restored at the end of the program.

6.3.4 The FLBPSS Routine

Procedure FLBPSS was used in order to calculate the stabilising signal. This procedure was used to perform the following functions:

1. Set up optimal parameters for $\alpha$, $\beta$ and $D_r$;
2. Calculate the speed deviation from the measured rotor angle;
3. Filter the speed deviation using a 4th-order digital filter with a 12 Hz cut-off frequency, and then calculate the acceleration;
4. Calculate the stabilising signal.
6.3.5 The AVR Routine

The CONTROLLER procedure was used in order to calculate the control signal. Since the D/A card can output a maximum of ±10V, precaution was taken so that control signal never exceeded this limit. This was realised by using if-then statement to test and adjust the control signal before it was sent out to the D/A converter.

6.3.6 Screen Graphics

A separate unit called SCRNPLT5 was used for drawing the trend plots for data logging. An OUTPUT-MENU procedure was also used to display the menus distinctively.

6.3.7 Other Features

A parallel I/O port was used to send the control signal out to switch the relay on and off in order to perform sudden load changes and three-phase to ground fault. The software was written user friendly. The user has the option of selecting reference voltage and testing time.

6.3.8 The Block Diagram of the Software

The software block diagrams are shown in Figures (6.2) and (6.3).

6.4 Implementation Tests

In order to test the robustness of the optimised FLBPSS, the following types of disturbances were applied:

- a 10% step increase in the reference voltage sustained for 7.5 seconds;
Chapter 6. Implementation Study

Figure 6.2: Software diagram (Part I)

Figure 6.3: Software diagram (Part II)
• 3/4 rated load increase sustained for 7.5 seconds;
• three-phase to ground fault at A (Figure 2.2) sustained for 125 milliseconds.

6.4.1 Step Change in the Reference Voltage

The speed deviation and rotor angle corresponding to a 10% step increase in the reference voltage sustained for 7.5 seconds are shown in Figures (6.4)-(6.6). Figures (6.4) and (6.5) provide the result under nominal operating condition \( P = 1 \text{pu}, \ \text{power factor} = 0.866 \text{ lag} \) without and with the FLBPSS respectively. Figure (6.6) shows the control signal applied to the generator field without and with the FLBPSS respectively. It can be seen that the rotor angle and speed deviation oscillations are damped out very quickly (within 2 cycles) when the system is equipped with the FLBPSS, whereas the rotor angle and speed deviation oscillated and damped out in 8 cycles without the FLBPSS.

Similar results as above were obtained (not shown here) under various operating conditions as listed in Table (6.1).

6.4.2 Sudden Load Change

The performance of the FLBPSS has been evaluated under various operating conditions as shown in Table (6.1).

<table>
<thead>
<tr>
<th>Operating condition</th>
<th>OC1</th>
<th>OC2</th>
<th>OC3</th>
<th>OC4</th>
</tr>
</thead>
<tbody>
<tr>
<td>Real power</td>
<td>0.52 pu</td>
<td>0.9 pu</td>
<td>1.4 pu</td>
<td>0.86 pu</td>
</tr>
<tr>
<td>Power factor</td>
<td>0.95 (lag)</td>
<td>0.866 (lag)</td>
<td>0.42 (lag)</td>
<td>0.99 (lead)</td>
</tr>
</tbody>
</table>

Table 6.1: Operating conditions for single-machine infinite bus power system

Figures (6.7)-(6.8) show the rotor angle and speed deviation corresponding to 3/4 rated resistive load change without and with the FLBPSS under operating condition P1. The oscillation of the rotor angle and speed deviation have been damped out within 2 cycles with the FLBPSS in operation and the maximum transient deviation has also been reduced. Without the FLBPSS, the corresponding
Chapter 6. Implementation Study

Figure 6.4: Rotor angle and speed deviation corresponding to a 10% step increase in the reference voltage sustained for 7.5 seconds (without the FLBPSS), (a)-rotor angle, (b)-speed deviation

outputs oscillated and damped out in 8 cycles. A number of tests were conducted for inductive and capacitive load changes and similar results were obtained. Figures (6.9)-(6.10) show the rotor angle and speed deviation corresponding to 3/4 rated inductive load change without and with the FLBPSS at operating condition P1. Figures (6.11)-(6.12) show the rotor angle and speed deviation corresponding to 3/4 rated capacitive load change without and with the FLBPSS under operating condition P1. The system oscillations resulted from the inductive, capacitive and resistive load changes have been damped out very quickly (within 1.5 to 2 cycles) and the maximum transient deviation has been reduced substantially in the presence of the FLBPSS. From the above results, it can be concluded that the FLBPSS performance is robust with different types and values of step load changes.

Figures (6.13)-(6.18) show the rotor angle and speed deviation in response to 3/4 rated resistive load change without and with the FLBPSS under operating condition P2, P3 and P4 respectively. Under the above operating conditions, the
maximum transient deviation has been reduced and the settling time is 4 times smaller when the FLBPSS was used. From these results, it can be seen that the FLBPSS works satisfactorily over a variety of operating conditions.

6.4.3 Three-phase to Ground Fault

A three-phase to ground fault was applied at the generator side of the transmission line (see Figure 2.2) and removed after 125 milliseconds. Figures (6.19) and (6.20) demonstrate the rotor angle and speed deviation in response to the three-phase to ground fault under the nominal operating condition \((\text{real power } P = 1 \text{ pu, power factor } = 0.866 \text{ lag})\) without and with the FLBPSS respectively. It can be observed that the speed deviation and rotor angle are damped out in 3 cycles by using the FLBPSS, whereas the oscillations are damped out in 9 cycles without the FLBPSS in operation. It takes a longer settling time in the three-phase to ground fault
Figure 6.6: Control signal corresponding to a 10% step increase in the reference voltage sustained for 7.5 seconds, (a)-without the FLBPSS and (b)-with the FLBPSS condition since the excitation control signal reached the hardware limit.

Similar results as above for a three-phase to ground fault were also obtained (not shown here) under various operating conditions P1-P4.

In the experimental results for the system studied, although the overall trend of the experimental results followed closely the simulation results, yet discrepancies were observed. The experimental value of $D_r$ was found to be 2 whereas it was 0.6 by simulation (which is more than 3 times). This difference are not only due to the uncertainty in the system parameters measured, but also very low $D_r$ requires almost bang-bang control due to the saturation in the controller. The increased value of $D_r$ indicates that the effect of saturation is reduced and accordingly, better performance was achieved in the experiment.
Figure 6.7: Rotor angle and speed deviation corresponding to sudden resistive load change without the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation

Figure 6.8: Rotor angle and speed deviation corresponding to sudden resistive load change with the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation
Figure 6.9: Rotor angle and speed deviation corresponding to sudden inductive load change without the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation

Figure 6.10: Rotor angle and speed deviation corresponding to sudden inductive load change with the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation
Figure 6.11: Rotor angle and speed deviation corresponding to sudden capacitive load change without the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation

Figure 6.12: Rotor angle and speed deviation corresponding to sudden capacitive load change with the FLBPSS (operating condition OC1), (a)-rotor angle, (b)-speed deviation
Figure 6.13: Rotor angle and speed deviation corresponding to sudden resistive load change without the FLBPSS (operating condition OC2), (a)-rotor angle, (b)-speed deviation

Figure 6.14: Rotor angle and speed deviation corresponding to sudden resistive load change with the FLBPSS (operating condition OC2), (a)-rotor angle, (b)-speed deviation
6.5 Concluding Remarks

The implementation of the optimised FLBPSS was tested on a single-machine infinite bus power system. The hardware and software development were described in detail in this chapter. The implementation test was carried out under different perturbations such as a 10% step change in the reference voltage as a small perturbation, a 3/4 rated sudden resistive, inductive and capacitive load changes and a three-phase to ground fault as large perturbations. The real time evaluation has also been tested under a wide range of operating conditions. The implementation results reveals that the optimised FLBPSS works well when the system is subject to either small or large perturbations. The performance of the optimised FLBPSS is robust with different types of step load changes (inductive, capacitive and resistive load). The optimised FLBPSS also works satisfactorily under a wide range of operating conditions without tuning or resetting of any parameters of the FLBPSS.
Figure 6.15: Rotor angle and speed deviation corresponding to sudden resistive load change without the FLBPSS (operating condition OC3), (a)-rotor angle, (b)-speed deviation

Figure 6.16: Rotor angle and speed deviation corresponding to sudden resistive load change with the FLBPSS (operating condition OC3), (a)-rotor angle, (b)-speed deviation
Figure 6.17: Rotor angle and speed deviation corresponding to sudden resistive load change without the FLBPSS (operating condition OC4), (a)-rotor angle, (b)-speed deviation

Figure 6.18: Rotor angle and speed deviation corresponding to sudden resistive load change with the FLBPSS (operating condition OC4), (a)-rotor angle, (b)-speed deviation
Figure 6.19: Rotor angle and speed deviation corresponding to a three-phase fault at A (Figure 2.2) sustained for 125 milliseconds (without the FLBPSS), (a)-rotor angle, (b)-speed deviation

Figure 6.20: Rotor angle and speed deviation corresponding to a three-phase fault at A (Figure 2.2) sustained for 125 milliseconds (with the FLBPSS), (a)-rotor angle, (b)-speed deviation
Chapter 7

Application of the FLBPSS to Multi-machine Systems

7.1 Introduction

The interconnection of electric power systems is almost universal throughout the world. Basically, the electric power systems interconnect to each other because the interconnected systems is more reliable, it is a better system to operate and it may be operated at less cost than if left as separate parts. The merits of integrated power systems are summarised as follows [Wood, 1984]:

1. The maximum demand of an integrated system is much less than the sum of the individual non-coincident maximum demand of the sub-system comprising the system. The individual maximum demand occurs at different point of time because of diversity of the type of load, the lighting up time and the special characteristics of the systems.

2. The reserve on the system wide basis is reduced, and this means less economic operation.

3. During emergency, power can flow from surplus area to deficit areas. This makes the interconnections more reliable, since the loss of a generating unit in one of them can be made up from spinning reserve among units.
throughout the interconnection. Thus, if a unit is lost in a control area, governing action from units in all connected areas will increase generation outputs to make up the deficit until standby units can be brought on-line. If a power system were to run isolated and lose a large unit, the chance of the other units in that isolated system being able to make up the deficit are greatly reduced.

4. It is possible to use large unit sizes which have better thermal efficiency so that the operating cost can be reduced.

5. The peak consumer demands can be economically distributed between the constituent sub-systems.

6. New generation size can be selected on a system wide basis rather than on local basis resulting in saving capital cost.

7. Maintenance is economical on a system wide basis which means the capital cost can be reduced.

8. For any given local demand, the cost of generation can be minimised and economic local dispatch can function most effectively.

However, it is observed that one of the most important stability problems arising from large scale electric power system interconnections is the low-frequency oscillations of interconnected systems. The frequency is of the order of a fraction of 1 Hz to a few Hz. The oscillations may be sustained for minutes and grow to cause system separation if no adequate damping at the system oscillating frequency is available.

In this project, the FLBPSS was used to damp the oscillations for a two-machine infinite bus power system.

This chapter is organised as follows:

In Section 7.2, the AVRs are designed for the two generators. The transfer function of the AVR for generator 1 is the same as in Chapter 3. The AVR for generator 2 is designed in Section 7.2.2. The practical evaluation of the AVRs are presented in Section 7.2.3. Three kinds of disturbances are applied to the system in
order to test the performance of the designed AVRs. The design and optimisation of the FLBPSS is reviewed in Section 7.3. In section 7.4, simulation studies of the designed AVRs and the FLBPSS are demonstrated. The implementation results on the two-machine infinite bus power system are presented in Section 7.5 followed by the concluding remarks. A mathematical model of a three-machine power system can be found in Appendix D.

7.2 AVR Design

7.2.1 Design of the AVR for Generator 1

The design of the AVR for generator 1 in the two-machine infinite bus system was the same as in the single-machine infinite bus power system which was described previously in Chapter 3. The AVR transfer function for generator 1 can be rewritten as:

$$G_{AVR1}(z) = \frac{5.0586 - 1.2345z^{-12}}{1 - BF(z)}$$  \hspace{1cm} (7.1)

$$BF(z) = 0.1467z^{-1} + 0.1304z^{-2} + 0.1160z^{-3} + 0.1031z^{-4} + 0.0917z^{-5} + 0.0815z^{-6} + 0.0725z^{-7} + 0.0644z^{-8} + 0.0573z^{-9} + 0.0509z^{-10} + 0.0453z^{-11} + 0.0402z^{-12}$$  \hspace{1cm} (7.2)

The sensor DC gain $B$ was found to be $5/240 = 0.0208$ and $A$ is the gain of the field drive unit and was found to be 25 in this case.

7.2.2 Design of the AVR for Generator 2

Again the dynamic behaviour of the generator is described by a simplified linear model. The resulting block diagram was shown previously in Figure (3.1). The system parameters have been measured according to the IEEE test procedure for
a 5kVA, 240V synchronous machine at the Power System Laboratory. The K parameters under one nominal operating condition (real power $P = 1$pu, power factor $PF = 0.85$ lag) are shown as follows:

- $K_1 = 1.1158$
- $K_2 = 1.1825$
- $K_3 = 0.4347$
- $K_4 = 0.3453$
- $K_5 = 0.1161$
- $K_6 = 0.8204$
- $M = 2H = 2 \times 0.524s$
- $\tau_{d0} = 0.56s$
- $D = 2$

Considering the single voltage-regulator loop in the block diagram of Figure (3.2), a simplified first order approximation voltage loop of the machine is given by

$$G_v(s) = \frac{0.637}{1 + 0.28s} \quad (7.3)$$

Using discrete time analytical design methods described in Section 3.3 of Chapter 3, the transfer function for AVR2 can be expressed as in the following equation:

$$G_{AVR2}(z) = A \frac{N(z)}{1 - BF(z)} \quad (7.4)$$

where the sample time used is also 25 milliseconds and the gain $A$ for the field drive unit is 25.

$$N(z) = 6.69 + 0.038z^{-1} - 0.038z^{-2} + 0z^{-3} + 0z^{-4} - 0.006z^{-5} + 0.045z^{-6}$$
$$+ 0.025z^{-7} + 0.025z^{-8} - 0.045z^{-9} + 0z^{-10} + 0.064z^{-11} - 3.95z^{-12} \quad (7.5)$$
Chapter 7. Application of the FLBPSS to Multi-machine Systems

\[ BF(z) = 0.105z^{-1} + 0.101z^{-2} + 0.096z^{-3} + 0.092z^{-4} + 0.088z^{-5} + 0.084z^{-6} \]
\[ + 0.081z^{-7} + 0.077z^{-8} + 0.074z^{-9} + 0.07z^{-10} + 0.067z^{-11} + 0.065z^{-12} \] (7.6)

7.2.3 Practical Evaluation of the Designed AVRs

The performance of the designed AVRs was tested experimentally in the power laboratory. The following disturbances were applied to the system in order to test the performance of the AVRs.

- a 10% step increase in the reference voltage at generator 1 side sustained for 7.5 seconds;
- 3/4 rated load increase at generator 1 side sustained for 7.5 seconds;
- a three-phase to ground fault at B (Figure 2.4) sustained for 125 milliseconds.

Test of AVRs on a step change in generator reference voltage

A small perturbation of a 10% step increase in the reference voltage sustained for 7.5 seconds has been applied at generator 1 side in order to test the performance of the designed AVRs on a two-machine infinite bus power system. Figure (7.1) shows the voltage response for both generators in response to the disturbance. From this figure it can be seen that the voltage is tracking the reference voltage value with no steady state error. The overshoot and settling time all satisfy the IEEE standards on excitation control [IEEE, 1978].

Test of AVRs in response to rated load change

Figures (7.2)-(7.4) show the terminal voltage response corresponding to a 3/4 rated sudden inductive, capacitive and resistive load change with the designed AVRs; it can be seen that the system equipped with the designed AVRs kept the terminal voltage output constant under various loading conditions. The performance of the digital AVRs is then theoretically analysed and experimentally verified.
Test of AVRs in response to a three-phase to ground fault

Figures (7.5)-(7.6) show the terminal voltages and control signals in response to a three-phase to ground fault at B (Figure 2.4) sustained for 125 milliseconds. It can be seen that the excitation control signals reached the ceiling (i.e., the hardware limit ±10V) very quickly when the system was subject to such a large disturbance. The terminal voltage of generator 1 reduced towards zero during the fault and has been brought back to its original value as soon as the fault was cleared. The fault occurred at generator 1 terminal, however, the terminal voltage at generator 2 has also been affected due to the interconnection.

7.3 The Design and Optimisation of the FLBPSS

The design of the proposed FLBPSS was presented previously in Chapter 4. The optimisation strategy is the same as presented in Chapter 5. For the optimisation and implementation study, only generator 1 was equipped with the proposed FLBPSS. The optimal values of $\alpha$, $\beta$ and $D_r$ were found to be 30, -40 and 0.6 respectively.

7.4 Simulation Results for the FLBPSS

Figures (7.7)-(7.8) show the speed deviation of generators 1 and 2 corresponding to a 10% step increase in the reference voltage followed by a 10% step increase in the mechanical torque. Figures (7.9)-(7.10) show the speed deviation of generators 1 and 2 corresponding to a 20% step increase in reference voltage followed by a 20% step increase in the mechanical torque. Figures (7.7) and (7.9) demonstrate the results without the FLBPSS. Figures (7.8) and (7.10) show the results with the FLBPSS. Figures (7.7)-(7.10) (a) show the system response for generator 1 and Figures (7.7)-(7.10) (b) for generator 2. From those figures, it can be seen that the FLBPSS is very effective in damping the system oscillations.
7.5 Implementation and Test Results for the FLBPSS

The disturbances applied to the experimental two-machine infinite bus power system were:

- a 10% step increase in the reference voltage at generator 1 side sustained for 7.5 seconds;
- 3/4 rated load increase at generator 1 side sustained for 7.5 seconds;
- a three-phase to ground fault at B (Figure 2.4) sustained for 125 milliseconds;
- the transmission line loss between generators 1 and 2.

Generators 1 and 2 were both equipped with the designed digital AVRs. During all the tests, only generator 1 was equipped with the optimised FLBPSS.

7.5.1 Step Change in the Reference Voltage at Generator 1 Side

Figures (7.11)-(7.14) show the rotor angle and speed deviation in response to a 10% step increase in the reference voltage sustained for 7.5 seconds at generator 1 side under the nominal operating condition (real power $P_1 = 1pu, P_2 = 1pu$, power factor $PF_1 = 0.95$ (lag), $PF_2 = 0.85$ (lag)). Figures (7.11) and (7.12) show the results without and with the FLBPSS respectively for generator 1. Figures (7.13) and (7.14) demonstrate the results without and with the FLBPSS respectively for generator 2. It can be seen that the oscillation has been damped out very quickly (within 2 cycles) for both machines although only one machine was equipped with the optimised FLBPSS.

7.5.2 Rated Load Change

Figures (7.15)-(7.26) show the rotor angle and speed deviation corresponding to a 3/4 rated load change under the nominal operating condition (real power $P_1 =$,
1pu, $P_2 = 1pu$, power factor $PF_1 = 0.95$ (lag), $PF_2 = 0.85$ (lag)). Figures (7.15) and (7.16) show the results corresponding to 3/4 rated sudden resistive load change for generator 1 without and with the FLBPSS respectively. Figures (7.17) and (7.18) show the results for generator 2 in response to 3/4 sudden resistive load change without and with the FLBPSS respectively. Studies were also carried out for different load changes such as inductive and capacitive load changes. Figures (7.19)-(7.22) show the results corresponding to sudden inductive load change and Figures (7.23)-(7.26) show the results corresponding to sudden capacitive load change. Figures (7.19) and (7.20) show the rotor angle and speed deviation corresponding to 3/4 sudden inductive load change without the FLBPSS for generators 1 and 2 respectively. Figures (7.21) and (7.22) show the rotor angle and speed deviation corresponding to 3/4 sudden inductive load change with the FLBPSS for generators 1 and 2 respectively. Figures (7.23) and (7.24) show the rotor angle and speed deviation corresponding to 3/4 sudden capacitive load change without the FLBPSS for generators 1 and 2 respectively. Figures (7.25) and (7.26) show the rotor angle and speed deviation corresponding to 3/4 sudden capacitive load change with the FLBPSS for generators 1 and 2 respectively. It can be seen from the above figures that the optimised FLBPSS damped the system oscillations out very effectively.
Figure 7.1: Terminal voltage corresponding to a 10% step change in reference voltage at generator 1 side, (a)-terminal voltage for generator 1, (b)-terminal voltage for generator 2

Figure 7.2: Terminal voltage corresponding to 3/4 rated inductive load change, (a)-terminal voltage for generator 1, (b)-terminal voltage for generator 2
Figure 7.3: Terminal voltage corresponding to 3/4 rated capacitive load change, (a)-terminal voltage for generator 1, (b)-terminal voltage for generator 2

Figure 7.4: Terminal voltage corresponding to 3/4 rated resistive load change, (a)-terminal voltage for generator 1, (b)-terminal voltage for generator 2
Chapter 7. Application of the FLBPSS to Multi-machine Systems

Figure 7.5: Terminal voltage corresponding to a three-phase to ground fault, (a)-terminal voltage for generator 1, (b)-terminal voltage for generator 2

Figure 7.6: Excitation control signal corresponding to a three-phase to ground fault, (a)-control signal for generator 1, (b)-control signal for generator 2
Figure 7.7: System response corresponding to a 10% step change in reference voltage and mechanical torque without PSS, (a)-speed deviation for generator 1, (b)-speed deviation for generator 2

Figure 7.8: System response corresponding to a 10% step change in reference voltage and mechanical torque with the FLBPSS, (a)-speed deviation for generator 1, (b)-speed deviation for generator 2
Figure 7.9: System response corresponding to a 20% step change in reference voltage and mechanical torque without the FLBPSS, (a)-speed deviation for generator 1, (b)-speed deviation for generator 2.

Figure 7.10: System response corresponding to a 20% step change in reference voltage and mechanical torque with the FLBPSS, (a)-speed deviation for generator 1, (b)-speed deviation for generator 2.
Figure 7.11: Rotor angle and speed deviation for generator 1 corresponding to a 10% step increase in the reference voltage at generator 1 sustained for 7.5 seconds (without the FLBPSS), (a)-rotor angle, (b)-speed deviation

Figure 7.12: Rotor angle and speed deviation for generator 1 corresponding to a 10% step increase in the reference voltage at generator 1 sustained for 7.5 seconds (with the FLBPSS), (a)-rotor angle, (b)-speed deviation
Figure 7.13: Rotor angle and speed deviation for generator 2 corresponding to a 10% step increase in the reference voltage at generator 1 sustained for 7.5 seconds (without the FLBPSS), (a)-rotor angle, (b)-speed deviation

Figure 7.14: Rotor angle and speed deviation for generator 2 corresponding to a 10% step increase in the reference voltage at generator 1 sustained for 7.5 seconds (with the FLBPSS), (a)-rotor angle, (b)-speed deviation
Figure 7.15: Rotor angle and speed deviation for generator 1 corresponding to sudden resistive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation

Figure 7.16: Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden resistive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation
Figure 7.17: Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden resistive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation

Figure 7.18: Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden resistive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation
7.5.3 Test Results Under Different Operating Conditions

The performance of the FLBPSS corresponding to a 10% step change in reference voltage and sudden load change has also been tested under different operating conditions (OC) as shown in Table (7.1). However, only the system response corresponding to resistive load change under operating condition $P_1$ is shown here. Figures (7.27)-(7.30) show the rotor angle and speed deviation for both generators corresponding to a 3/4 rated resistive load change under operating condition $P_1$. Figures (7.27) and (7.29) show the results without the FLBPSS for generators 1 and 2 respectively. Figures (7.28) and (7.30) show the results with the FLBPSS for generators 1 and 2 respectively. It can be seen that the FLBPSS works well under different operating conditions. Similar test results were also obtained (not shown here) for inductive and capacitive load changes at different operating conditions.

<table>
<thead>
<tr>
<th>OC</th>
<th>$P_1 = 1\text{pu}, P_2 = 1\text{pu}$</th>
<th>$P_1 = 0.6\text{pu}, P_2 = 1\text{pu}$</th>
<th>$P_1 = 0.42\text{pu}, P_2 = 1\text{pu}$</th>
</tr>
</thead>
<tbody>
<tr>
<td>$P_F$</td>
<td>$P_{F1} = 0.95, P_{F2} = 0.85$</td>
<td>$P_{F1} = 0.98, P_{F2} = 0.84$</td>
<td>$P_{F1} = 0.707, P_{F2} = 0.85$</td>
</tr>
</tbody>
</table>

Table 7.1: Operating conditions for two-machine infinite bus power system

7.5.4 Three-phase to Ground Fault

The system response corresponding to a three-phase to ground fault at B (Figure 2.4) sustained for 125 milliseconds under the nominal operating condition are shown in Figures (7.31)-(7.34). Figures (7.31) and (7.33) show the rotor angle and speed deviation without the FLBPSS for generator 1 and 2 respectively. Figures (7.32) and (7.34) demonstrate the rotor angle and speed deviation with the FLBPSS for generators 1 and 2 respectively. Comparing Figures (7.32) and (7.34) with Figures (7.31) and (7.33), it can be seen that the FLBPSS works well when the system was subject to such large disturbances. Similar results were obtained (not shown here) under different operating conditions as listed previously in Table 7.1.
Figure 7.19: Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden inductive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation.

Figure 7.20: Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden inductive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation.
Figure 7.21: Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden inductive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation

Figure 7.22: Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden inductive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation
Figure 7.23: Rotor angle and speed deviation for generator 1 corresponding to $3/4$ rated sudden capacitive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation

Figure 7.24: Rotor angle and speed deviation for generator 2 corresponding to $3/4$ rated sudden capacitive load change (without the FLBPSS), (a)-rotor angle, (b)-speed deviation
Figure 7.25: Rotor angle and speed deviation for generator 1 corresponding to $3/4$ rated sudden capacitive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation

Figure 7.26: Rotor angle and speed deviation for generator 2 corresponding to $3/4$ rated sudden capacitive load change (with the FLBPSS), (a)-rotor angle, (b)-speed deviation
Figure 7.27: Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden resistive load change without the FLBPSS (Operating condition OC1), (a)-rotor angle, (b)-speed deviation

Figure 7.28: Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden resistive load change without the FLBPSS (Operating condition OC1), (a)-rotor angle, (b)-speed deviation
Figure 7.29: Rotor angle and speed deviation for generator 1 corresponding to 3/4 rated sudden resistive load change with the FLBPSS (Operating condition OC1), (a)-rotor angle, (b)-speed deviation

Figure 7.30: Rotor angle and speed deviation for generator 2 corresponding to 3/4 rated sudden resistive load change with the FLBPSS (Operating condition OC1), (a)-rotor angle, (b)-speed deviation
Chapter 7. Application of the FLBPSS to Multi-machine Systems

Figure 7.31: Rotor angle and speed deviation for generator 1 corresponding to a three-phase fault at B (Figure 2.4) sustained for 125 milliseconds (without the FLBPSS), (a)-rotor angle, (b)-speed deviation

Figure 7.32: Rotor angle and speed deviation for generator 1 corresponding to a three-phase fault at B (Figure 2.4) sustained for 125 milliseconds (with the FLBPSS), (a)-rotor angle, (b)-speed deviation
Figure 7.33: Rotor angle and speed deviation for generator 2 corresponding to a three-phase fault at B (Figure 2.4) sustained for 125 milliseconds (without the FLBPSS), (a)-rotor angle, (b)-speed deviation.

Figure 7.34: Rotor angle and speed deviation for generator 2 corresponding to a three-phase fault at B (Figure 2.4) sustained for 125 milliseconds (with the FLBPSS), (a)-rotor angle, (b)-speed deviation.
7.5.5 Transmission Line Loss Between Generators 1 and 2

The oscillation occurred when the system was subject to a transmission line loss between generators 1 and 2. This happens when a power system is subject to a fault and the circuit breaker at each end of the transmission line will trip resulting the transmission line loss. The FLBPSS can also be used to damp out this kind of oscillation. Figures (7.35) and (7.36) show the rotor angle and speed deviation in response to the transmission loss under the nominal operating condition without the FLBPSS for both generators 1 and 2 respectively. Figures (7.37) and (7.38) show the corresponding results with the FLBPSS for generators 1 and 2 respectively. It is obvious from these figures that the oscillation has been damped out very effectively by using the FLBPSS.

Figure 7.35: Rotor angle and speed deviation for generator 1 corresponding to the loss of the transmission line (without the FLBPSS), (a)-rotor angle, (b)-speed deviation
Figure 7.36: Rotor angle and speed deviation for generator 2 corresponding to the loss of the transmission line (without the FLBPSS), (a)-rotor angle, (b)-speed deviation.

Figure 7.37: Rotor angle and speed deviation for generator 1 corresponding to the loss of the transmission line (with the FLBPSS), (a)-rotor angle, (b)-speed deviation.
Figure 7.38: Rotor angle and speed deviation for generator 2 corresponding to the loss of the transmission line (with the FLBPSS), (a)-rotor angle, (b)-speed deviation

7.6 Concluding Remarks

In this chapter the merits of the interconnection of electric power systems have been summarised. The design of the AVRs for the two synchronous generators have been introduced. The performance of the designed AVRs have been tested in real time. The test results show that the AVRs control the terminal voltage value according to the reference voltage. The overshoot and settling time all satisfy the IEEE standard for excitation control. The terminal voltages have been kept constant under various sudden load change conditions. The performance of the AVRs is robust against different step changes in loading. Experimental results have also been obtained when the system was subject to a three-phase to ground fault.

The simulation and implementation studies of the optimised FLBPSS have also been carried out for the two-machine infinite bus power system. The simulation test has been demonstrated when a step change in the reference voltage and mechanical torque have been applied to the system. The rotor angle and speed deviation oscillations for both generators have been damped out within one and half cycles.
although only generator 1 was equipped with the FLBPSS. The implementation test has been carried out under different disturbance and operating conditions. Four different kinds of disturbances such as a 10% step change in the reference voltage, a 3/4 rated load (inductive, capacitive and resistive) change, a three-phase to ground fault and a transmission line loss have been applied to the system in order to test the robustness of the FLBPSS. All the test results reveal that the oscillations resulted from the above mentioned disturbances have been damped out within either one and half to two cycles in the presence of the optimised FLBPSS. The maximum transient deviation has also been reduced substantially. For three-phase to ground fault, it takes a longer time to damp the oscillation out due to the hardware limitation of the control signal. The performance of the FLBPSS has also been tested under different operating conditions.

From the simulation and implementation results, it can be concluded that the FLBPSS works satisfactorily without resetting and tuning of the optimised parameters under different disturbances at various operating conditions for the two-machine infinite bus power system.
Chapter 8

Rules Reduction for the FLC Using Neural Networks

8.1 Introduction

The previously designed Fuzzy Logic Controller (FLC) is not very efficient in comparison with the Fuzzy Logic Based Power System Stabiliser (FLBPSS) because it uses too many rules but provides poorer performance. By using neural network techniques, the rules can be reduced, fine tuned and also the FLC performance can be improved.

Neural networks are trained to give a certain output based on a certain input through the use of learning methods. Generally, a node of a neural network contains an activation level which during training is increased or decreased based on how “close” the node is to the current input being trained for. Training methods are used to change the value of the node based on this “closeness”.

In the literature, Neural Networks (NN) are used for learning rules from input/output data. Such an example is given in Kosko [Kosko, 1992] for obtaining rules to stabilise an inverted pendulum. Consider a system which has a simple inverted pendulum free to rotate in the plane on a pivot attached to the cart. A human operator is taking actions in order to keep the pendulum vertical at all times.
by applying a restoring force $F(t)$ (control signal) to the cart at some discrete time $t$ in response to change in both linear and angular positions $(x(t), \theta(t))$ and velocity $(\dot{x}(t), \dot{\theta}(t))$ of the pendulum. The set of input and output (operator’s action) pairs are the data fed into a NN to perform Adaptive Vector Quantisation (AVQ).

The obtained rules in correlation with the predefined membership functions are used to define a fuzzy system for which the control surface is approximately the one used by the human operator in stabilising the pendulum.

**TILGen** [Tilgen, 1991] is a tool that automatically generates a fuzzy expert system from a set of inputs and required outputs. **TILGen** is a combination of two techniques: a neural network to learn the input-output function described by the set of inputs and outputs, and a technique to decode the neural network to generate the rules for the fuzzy expert system. **TILGen** creates a neural network by partitioning the input space of the fuzzy rule base being generated. This partitioning is based upon the number of input variables and the number of membership functions defined for each variable.

In **TILGen** any one of the three learning algorithms can be adopted: *unsupervised competitive learning, supervised competitive learning, or differential competitive learning*. The methods work by first initialising the n nodes of the neural network with the first n test vectors. Then, each remaining vector is compared with the n nodes and the node (or nodes) which most closely match the input vector are found. These nodes are commonly known as the winning nodes. The nodes are then updated according to the learning method used.

When *unsupervised competitive learning* is used, the winning nodes are rewarded by having their activation levels increased. When *supervised competitive learning* is used, the winning nodes are rewarded by increasing their activation levels and the non-winning nodes are punished by decreasing their activation levels. When *differential competitive learning* is used, the winning nodes are found and the closest winning node is rewarded and the other winning nodes are punished. It should be noted that *unsupervised competitive learning and differential competitive learning* are similar in that they do not punish losing nodes; they are only concerned
with winning nodes. *Unsupervised competitive learning* and *differential competitive learning* tend to produce similar results and *differential competitive learning* is guaranteed to converge exponentially quickly, while *unsupervised competitive learning* is not guaranteed to converge. The neural networks with *supervised competitive learning* algorithm tend to need more time and information to train.

### 8.2 Rules Reduction for the FLC Using Neural Networks

In the case when the FLC has been used as power system stabiliser, it is difficult to have a predefined desired control surface. The idea was to approximate the FLC in order to possibly simplify its structure (reduce rules). The input signals which were generated by applying disturbances such as a 20% step change in mechanical torque $T_m$ and a 20% step change in reference voltage $V_{ref}$ to the power system have been applied to the original 49-rule FLC to obtain the output control signal. Thus the input/output pairs were not obtained from a human-based control but from the excitation of the initial FLC. Using this input-output data, the Neural Network facility of TILGen has led to a simplified version of the FLC.

#### System Inputs

TILGen takes input as two files: an input Fuzzy Programming Language (FPL) file and an input data vector file.

The input FPL file must be a properly defined FPL file capable of being loaded by the TILShell [Tilshell, 1991] or run through one of the TIL compilers such as the Fuzzy-C Compiler. A FUZZY object for which TILGen will generate a fuzzy rule base has been defined in this file. A VAR objects (including their membership functions) which will be the inputs and outputs of the FUZZY object and the CONNECT objects which define the input/output relationships between the FUZZY object and the VAR objects have also been defined in the FPL file. The only object which will be modified by TILGen is the FUZZY object. It will have its current
The structure of the input data vector file is crucial for the proper execution of TILGen. The structure of the vector file is simply that each line of the vector file must contain one and only one entry for each input and output variable defined in the input FPL file separated by either a comma, space or tab. The entries should be ordered with the input variables in alphabetical order followed by the output variables in alphabetical order. The data vector file contains input variables \texttt{aSpeed} and \texttt{bAcceleration} and output variable \texttt{Control} which was generated by applying disturbances such as a 20\% step change in mechanical torque $T_m$ and a 20\% step change in reference voltage $V_{ref}$ to the original 49-rule FLC.

In order to guarantee proper training there have to be enough vectors in the vector file. As a rule of thumb, there must be at least twice as many vectors as the number of nodes used in the neural network. The number of nodes in the neural network varies depending upon the number of variables and the number of membership functions defined for each variable. To compute the number of nodes in the neural network, compute the combined product of the number of membership functions for each variable in the system. There are two inputs (speed and acceleration) and one output (stabilising signal) in the system and there are 7 membership functions for both inputs and output. The number of nodes in the neural network is $7 \times 7 \times 7$ or 343 [Tilgen, 1991]. Therefore, 1000 data vectors have been used which is almost three times the number of nodes. The input and output data have been multiplied by 10000 to get large values in order to guarantee proper training.

**Executing TILGen to generate fuzzy rule base**

When executing TILGen a few command line options have to be specified. Some of the options are explained as follows:

- **Specify the learning method**

  The differential competitive learning algorithm has been adopted in order to guarantee the convergence and reduce training time.
• Specify the cell threshold

The cell threshold value can be specified for whether or not to emit a rule based upon how many neurones converge to that point in the input space. The default setting for this value is 5 and range from 1 to 100. This value does not usually have a large effect on the output of the system as the neural network nodes tend to clump into a few areas of the input space. As a result, there are not areas in the input space which only one or two nodes have been trained to. Instead of that there are areas where twenty or more nodes have been trained to. To ensure all areas of the input space containing nodes generate rules, the threshold can be set to one. With the threshold of one, a rule will be generated for an area of the input space when at least one node has been trained to that area. This option works with the number of winners option to give the user more control over how many rules are to be generated from TILGen. Setting this value very low and the number of winners very high causes more rules to be generated because more nodes will be rewarded, causing less convergence to take place. The default value 5 has been chosen for this option.

• Specify the number of winners

The number of winning nodes in the neural network being trained can be specified using this option. How these winning nodes are rewarded varies with the learning method used. If unsupervised competitive learning is specified, the winning nodes have their activation levels increased. If supervised competitive learning is specified, the winning nodes have their activation levels increased and the losing nodes have their activation levels decreased. If differential competitive learning is specified, the closest winning node is rewarded by having its activation level increased and the other winning nodes have their activation levels decreased. The default value 3 has been chosen for this option. However, this value can be ranged from 1 to 100.

The generated rule base is shown in Appendix E.2.

The rule base is summarised in Table (8.1).
Table 8.1: The decision table after learning

<table>
<thead>
<tr>
<th>$\Delta \omega$</th>
<th>$\Delta \omega$</th>
</tr>
</thead>
<tbody>
<tr>
<td>PB</td>
<td></td>
</tr>
<tr>
<td>PM</td>
<td>ZR PM PM PB</td>
</tr>
<tr>
<td>PS</td>
<td>NS ZR PS PM PB</td>
</tr>
<tr>
<td>ZR</td>
<td>NM NM ZR PM</td>
</tr>
<tr>
<td>NS</td>
<td>NB NM NS ZR</td>
</tr>
<tr>
<td>NM</td>
<td>NM NM NB</td>
</tr>
<tr>
<td>NB</td>
<td>NB NB NB</td>
</tr>
</tbody>
</table>

The **TILGen** generated 24 rules by using neural network technique. Therefore, the original decision table which contains 49 rules has been simplified.

### 8.3 Comparison Study

The comparison study between the original 49-rule FLC and the simplified 24-rule FLC presented here were obtained on the single-machine infinite bus power system.

Table (8.2) shows the performance index corresponding to a changes of membership function whole overlap ratio (WOR) in response to a 20% step increase in mechanical torque $T_m$ followed by a 10% step increase in reference voltage $V_{ref}$ and a 10% step decrease in $V_{ref}$ with the original 49-rule FLC and the 24-rule FLC. From Table (8.2), it can be seen that the optimal WOR is 14.29% and the corresponding performance index for the original FLC and the reduced rule FLC are 2.50% and 1.78% respectively. The performance index of the FLC has been improved substantially by using the 24-rule FLC.

Table (8.3) shows the performance index corresponding to different mechanical torque changes with the original FLC and the reduced rule FLC (WOR=14.29%). It can be observed that the performance index has been reduced substantially with the 24-rule FLC.

The dynamic results using this simplified FLC are compared with the initial one as can be observed in Figure (8.1) to (8.4). Figures (8.1) and (8.3) show the results with the original 49-rule FLC. Figures (8.2) and (8.4) show the result with
Chapter 8. Rules Reduction for the FLC Using Neural Networks

<table>
<thead>
<tr>
<th>WOR%</th>
<th>49-rule</th>
<th>24-rule</th>
</tr>
</thead>
<tbody>
<tr>
<td>30.95</td>
<td>3.04</td>
<td>2.39</td>
</tr>
<tr>
<td>26.78</td>
<td>2.82</td>
<td>1.91</td>
</tr>
<tr>
<td>24.27</td>
<td>2.79</td>
<td>1.90</td>
</tr>
<tr>
<td>21.95</td>
<td>2.74</td>
<td>1.88</td>
</tr>
<tr>
<td>18.79</td>
<td>2.63</td>
<td>1.84</td>
</tr>
<tr>
<td>15.98</td>
<td>2.58</td>
<td>1.82</td>
</tr>
<tr>
<td>15.12</td>
<td>2.54</td>
<td>1.80</td>
</tr>
</tbody>
</table>

<table>
<thead>
<tr>
<th>WOR%</th>
<th>49-rule</th>
<th>24-rule</th>
</tr>
</thead>
<tbody>
<tr>
<td>14.45</td>
<td>2.52</td>
<td>1.79</td>
</tr>
<tr>
<td>14.29</td>
<td>2.50</td>
<td>1.78</td>
</tr>
<tr>
<td>13.48</td>
<td>2.53</td>
<td>1.80</td>
</tr>
<tr>
<td>12.72</td>
<td>2.56</td>
<td>1.82</td>
</tr>
<tr>
<td>11.98</td>
<td>2.59</td>
<td>1.85</td>
</tr>
<tr>
<td>11.27</td>
<td>2.63</td>
<td>1.88</td>
</tr>
<tr>
<td>10.58</td>
<td>2.67</td>
<td>1.91</td>
</tr>
<tr>
<td>9.93</td>
<td>2.71</td>
<td>1.94</td>
</tr>
</tbody>
</table>

<table>
<thead>
<tr>
<th>WOR%</th>
<th>49-rule</th>
<th>24-rule</th>
</tr>
</thead>
<tbody>
<tr>
<td>9.3</td>
<td>2.76</td>
<td>1.98</td>
</tr>
<tr>
<td>8.7</td>
<td>2.82</td>
<td>2.02</td>
</tr>
<tr>
<td>8.1</td>
<td>2.88</td>
<td>2.07</td>
</tr>
<tr>
<td>7.6</td>
<td>2.94</td>
<td>2.12</td>
</tr>
<tr>
<td>5.1</td>
<td>3.50</td>
<td>2.56</td>
</tr>
<tr>
<td>3.2</td>
<td>12.83</td>
<td>9.56</td>
</tr>
</tbody>
</table>

Table 8.2: The performance index corresponding to changes in WOR (20% step increase in mechanical torque followed by a 10% step increase in the reference voltage sustained for 7.5 seconds)

<table>
<thead>
<tr>
<th>$T_m$</th>
<th>original FLC with 49 rules</th>
<th>FLC with 24 rules</th>
</tr>
</thead>
<tbody>
<tr>
<td>0.01pu</td>
<td>$8.0347 \times 10^{-4}$</td>
<td>$4.7945 \times 10^{-4}$</td>
</tr>
<tr>
<td>0.2pu</td>
<td>0.69</td>
<td>0.42</td>
</tr>
<tr>
<td>0.5pu</td>
<td>5.41</td>
<td>3.63</td>
</tr>
</tbody>
</table>

Table 8.3: The performance index corresponding to different mechanical torque changes

the 24-rule FLC. Figures (8.1) and (8.2) demonstrate the speed deviation and rotor angle corresponding to 0.1pu step change in mechanical torque and reference voltage. Figures (8.3) and (8.4) demonstrate the speed deviation and rotor angle corresponding to a 0.2pu step change in mechanical torque and reference voltage. It can be seen that the simplified 24-rule FLC gives better performance. The maximum transient deviation of the speed deviation and rotor angle are smaller and the oscillations corresponding to the mechanical torque change are less with the 24-rule FLC.

The explanation for this is that the starting FLC was not shaping an optimal control surface. Some of the cells of the starting FLC are just an extrapolation/interpolation of the cells filled in by experience. The decision table was a complete starting table.
Figure 8.1: Speed deviation and rotor angle corresponding to a 10% step increase in mechanical torque followed by a 10% step increase in the reference voltage sustained for 7.5 seconds with the original 49-rule FLC.

Figure 8.2: Speed deviation and rotor angle corresponding to a 10% step increase in mechanical torque followed by a 10% step increase in the reference voltage sustained for 7.5 seconds with the 24-rule FLC.
Figure 8.3: Speed deviation and rotor angle corresponding to a 20% step increase in mechanical torque followed by a 20% step increase in the reference voltage sustained for 7.5 seconds with the original 49-rule FLC.

Figure 8.4: Speed deviation and rotor angle corresponding to a 20% step increase in mechanical torque followed by a 20% step increase in the reference voltage sustained for 7.5 seconds with the 24-rule FLC.
8.4 Concluding Remarks

TILGen which uses neural network techniques to learn the input-output function described by the set of inputs and outputs, and a technique to decode the neural network to generate the rules for the fuzzy expert system has been employed for rule reduction for the FLC. 24 rules has been generated using differential competitive learning when the system is subject to small disturbances. Both the performance index and the dynamic response have been improved substantially with the reduced rule FLC for the dynamic stability study.
Chapter 9

Conclusions

9.1 A Retrospective Overview of the Thesis

In this thesis, research has been conducted on the design, analysis, optimisation, and laboratory evaluation of two types of fuzzy controllers, namely the FLBPSS, and the FLC for power system stabilisation. Robustness and sensitivity analysis of the two fuzzy control schemes have been investigated. In addition, an AVR has been designed using discrete time analytical design method to assist in the assessment of the fuzzy controllers as mentioned above. Neural network techniques have been adopted to simplify the rule base of the second type of fuzzy controller. In particular, the designed AVR and optimised fuzzy controllers have been implemented in real time firstly on a single-machine infinite bus and secondly on a two-machine infinite bus power system.

The development of fuzzy controllers as power system stabilisers is motivated by the fact that a power system is a highly non-linear system, and the design of the most widely used conventional PSS is based on linearised fixed parameter models which are derived from the linearisation of the power system at a given operating point. The gain settings of these conventional PSS are usually determined off-line based on a particular operating condition and fixed in field applications. The use of a conventional PSS will result in shortcomings since the operating point of a
power system will change with varying system load. Moreover, drastic changes in system operating conditions will result when the system is subject to a major disturbances such as a three-phase fault. Hence, the best dynamic performance cannot be achieved by a fixed gain PSS under varying operating conditions. The self-tuning and adaptive PSSs have been developed to improve the damping characteristics of a power system over a wide range of operating conditions. In the self-tuning or adaptive PSS, the system model is first identified in real-time using the measured system input and output variables. The gain settings are then computed and adjusted based on the identified system model and the adaptation law. A major disadvantage of the self-tuning or adaptive PSS is that the system model parameters need to be identified in real time which is very time consuming. The situation is worsened by the fact that the self-tuning PSS must be implemented by a microcomputer with limited computational capacity. The need to eliminate the above shortcomings suggests the use of fuzzy control approach which can yield good damping characteristics over a wide range of operating conditions and does not require model identification as the self-tuning PSS does in real time.

In order to carry out an investigation into the design of fuzzy controllers as power system stabilisers, the following four stages are essential:

- analyse the circuit of the single-machine and two-machine infinite bus power system;
- model the non-linear experimental power systems;
- design the AVR;
- evaluate the designed AVR in real time.

The above aspects have been discussed (in Chapter 2 and 3) prior to the design, analysis, optimisation, and also implementation of the fuzzy controllers.

Firstly, the single-machine and two-machine infinite bus power system used in the power laboratory has been introduced. The experimental circuits have been analysed and the generator parameters have been provided.
Secondly, the mathematical model of the single-machine infinite bus power system has been developed. The development of the simplified linear model facilitates the design of the AVR in this chapter. The parameters of the mathematical model for the experimental power system have been derived (see Section 3.2).

Thirdly, the discrete time analytical design method has been analysed under the requirements essential for the design of the AVR. The digital AVR hence has been designed for the single-machine infinite bus power system according to the chosen control law.

Fourthly, the designed AVR has been experimentally verified in real time followed by the theoretical analysis of the AVR. The designed AVR has been tested under the following disturbance condition:

1. 1/2 rated and 3/4 rated inductive step load change;
2. 1/2 rated and 3/4 rated capacitive step load change;
3. 1/2 rated and 3/4 rated resistive step load changes;
4. a 10% step change in reference voltage;
5. a three-phase to ground fault;
6. at various operating conditions with the above disturbances.

The designed AVR performs satisfactorily as the AVR kept the generator output voltage constant under normal operating conditions at various load levels. The dynamic performance satisfy the IEEE standard of excitation control system dynamic performance indices. This is confirmed by both the simulation and real time implementation.

The completion of the above four stages establishes a valid basis for the excitation control on which the fuzzy controllers have been investigated.

The proposed design of two fuzzy control schemes has been investigated (see Chapter 4). The basic structure of a FLC has been described and the design of a FLC as a PSS has been developed. The generator speed $\Delta \omega$ and acceleration $\Delta \dot{\omega}$ have been chosen as the input signals of the FLC. The triangular membership
function shape has been chosen for both the input and output signal and the universe of discourse has been specified. A 49-rule decision table has been developed based on the theoretical knowledge. Different defuzzification methods have been introduced and the performance have been compared in terms of memory requirement, speed, etc.

The design of the FLBPSS has been presented and new two non-linear membership functions have been proposed. The resultant stabilising output is computed according to the fuzzy membership functions depending on the speed $\Delta \omega$ and acceleration $\Delta \dot{\omega}$ states of the synchronous generator.

The main features of the FLC and the FLBPSS are:

- the stabilising signal is updated on line depending on the speed $\Delta \omega$ and acceleration $\Delta \dot{\omega}$ of the synchronous generator, and hence provides optimal performance under a wide range of operating conditions;

- the design of the FLC and the FLBPSS does not necessitate the use of the mathematical model of the power system.

In order to optimise the fuzzy control strategy, the following five steps have to be performed (see Chapter 5):

- optimisation of the designed FLC;

- investigation of the optimal parameter settings for the proposed FLBPSS;

- introduction of the STFLBPSS and the optimisation of its parameter settings;

- comparison study between the proposed FLBPSS and the STFLBPSS;

- comparison study between the proposed FLC and the proposed FLBPSS.

Firstly, in order to optimise the designed FLC, the Whole Overlap Ratio (WOR) has been proposed to evaluate the membership function shape for the FLC.
It has been found that the FLC gives best performance when the WOR is approximately from 12% to 15%. Different implication methods, such as the Mamdani and Larsen methods, and different defuzzification methods, such as Means of max and Centroid, have also been evaluated by using the performance index. Sensitivity test of the FLC has been carried out to assess the robustness of the FLC by varying the system parameters for ±20% and under various operating conditions for both small and large perturbations.

Secondly, the optimal setting of the FLBPSS parameters has also been evaluated by using the performance index. The optimal settings of the proposed FLBPSS parameters $\alpha$, $\beta$ and $D_r$ have been obtained either by applying small or large perturbations. The best value of $\alpha$, $\beta$ and $D_r$ chosen for the nominal condition works well with a ±20% change in the nominal parameters. Thus no resetting or tuning of these parameters are needed with deviation of the parameters from the nominal conditions. Although the optimal values for different operating conditions are found to be different, investigation reveals that the optimal values of $\alpha$, $\beta$ and $D_r$ obtained at the nominal operating condition works satisfactorily for a wide variation of the operating conditions under both small and large perturbations. The optimal values of $\alpha$, $\beta$ and $D_r$ at one optimal point is sub-optimal at the other point with hardly any difference in the quality of the dynamic response.

Thirdly, a STFLBPSS has also been introduced in order to compare with the FLBPSS. The optimal settings of $\theta$, $F_a$ and $D_r$ values have also been explored. It has been found that at any operating point, the optimal values of the above mentioned parameters obtained by applying small perturbations differs from that for large perturbations and vice versa. Considering the system performance under different operating conditions with different perturbations and the system parameter variations, a compromise values of $\theta$, $F_a$ and $D_r$ have been chosen.

Fourthly, comparison study between the proposed FLBPSS and the STFLBPSS has been demonstrated through both the performance index and the dynamic response. Extensive study has been performed when the system is subject to small or large disturbances, variations in the system parameters and under wide variation of the operating conditions. Both the performance index and the dynamic response
show that the proposed FLBPSS gives better performance than the STFLBPSS.

Lastly, a comparison study between the proposed FLBPSS and the proposed FLC has also been demonstrated through both the performance index and the dynamic response. Extensive study has been performed when the system is subject to both small and large disturbances, variations in the system parameters and under wide variation of the operating conditions. The performance index of the FLC is 2 times larger than that of the FLBPSS. From the dynamic response, it can be seen that the maximum transient deviation is smaller and the settling time is shorter when the system is equipped with the FLBPSS. Therefore, the FLBPSS has been chosen as the practical PSS for real time implementation.

The implementation of the optimised FLBPSS was tested on a single-machine infinite bus power system (see Chapter 6). The implementation results reveal that:

- the optimised FLBPSS works well when the system is subject to either small (10% step change in the reference voltage) or large (three-phase to ground fault) perturbations;
- the performance of the optimised FLBPSS is robust with different types of step load changes (inductive, capacitive and resistive load);
- the FLBPSS also works satisfactorily under a wide range of operating conditions without tuning or resetting of any parameters of the optimised FLBPSS.

To demonstrate the effectiveness of the FLBPSS for multi-machine power system, the single-machine infinite bus power system has been extended to two-machine infinite bus power system due to the equipment limitation. The AVRs for the two synchronous generators have been designed (see Chapter 7) in order to carry on the research. The performance of the designed AVRs have been tested in real time. The test results show that:

- The AVRs control the terminal voltage value according to the reference voltage;
The overshoot and settling time both satisfy the IEEE standard for excitation control;

The terminal voltages have been kept constant under various sudden load change conditions; The performance of the AVRs is robust against different kinds of step change in loading. The AVRs also works satisfactorily when the system was subject to a three-phase to ground fault.

The effectiveness of the proposed FLBPSS for the two-machine infinite bus power system has been demonstrated by both simulation and implementation studies. The simulation test has been evaluated when a step change in the reference voltage and mechanical torque have been applied to the system. The rotor angle and speed deviation oscillations for both machines have been damped out very quickly (within one and half cycles) although only generator 1 was equipped with the FLBPSS. The implementation test has been carried out under different disturbance and operating conditions. Four different kinds of disturbances such as a 10% step change in the reference voltage, a 3/4 rated load (inductive, capacitive and resistive) change, a three-phase to ground fault and a transmission line loss have been applied to the system in order to test the robustness of the FLBPSS. All the test results reveal that the oscillations resulted from the above mentioned disturbances have been damped out within either one and half or two cycles. The maximum transient deviation has also been reduced substantially. For a three-phase to ground fault, it takes a longer time to damp the oscillation out due to the hardware limitation of the control signal. The performance of the FLBPSS has also been tested under different operating conditions.

From the simulation and implementation results, it can be concluded that the FLBPSS works satisfactorily without resetting and tuning of the optimised parameters under different disturbances at various operating conditions for the two-machine infinite bus power system.

In conclusion, the FLBPSS is an appropriate and practical approach for damping single-machine and two-machine infinite bus power system oscillations and improving both the dynamic and transient power system stability.
Chapter 9. Conclusions

Finally, neural network techniques have been used to improve the dynamic performance of the original 49-rule FLC (see Chapter 8). 24 rules have been generated when the single-machine infinite bus power system is subject to a step change in mechanical torque and reference voltage. Both the performance index and the dynamic response have been improved with the reduced rule FLC for dynamic stability study.

9.2 Avenues to be Explored in Further Work

The studies reported in this thesis involve the design, optimisation, simulation, and implementation of the fuzzy controllers for power system stabilisation. The following aspects relating to future research into the fuzzy control strategies in the design of power system stabilisers are suggested:

- Mathematically, the self-tuning control algorithm is much more complicated due to parameter identification, state observation and feedback gain computation which require extensive computing power, whereas the fuzzy logic based algorithm is very simple and easy to implement. Comprehensive comparison study of the performance of the self-tuning PSS and the FLBPSS need to be explored in future work.

- An adaptive FLC can be developed with a number of sets of parameters such as the scaling factors for each variable, the fuzzy set representing the meaning of linguistic values (the Whole Overlap Ratio of the membership functions) and the if-then rules altered on-line to achieve the optimal performance. The development of the so called self-tuning FLC and self-organising FLC need to be studied in detail in further work.

- Fuzzy if-then rules have been formulated with the predefined membership functions which are needed for calibration using neural network techniques. The performance of the FLC with the generated rules by using input-output data pairs and the defined membership functions has been improved for the dynamic
response under small perturbations. However, the 24-rule FLC does not work well when the system is subject to a large disturbance such as a three-phase to ground fault. Therefore, the complete decision table is needed for transient stability studies. In order to improve the performance of the FLC for both small and large perturbations under various operating conditions, neural network learning techniques can be used to produce the mapping rules from the empirical training sets, but the mapping rules in the neural network is not visible and is difficult to understand. It is also difficult to determine and to tune the rules in the FLC since the fuzzy sets does not have learning and adaptation capability. In order to solve these difficulties, the neural networks and the fuzzy sets can be combined to form **Fuzzy Neural Networks (FNN)** which is believed to have considerable potential in improving the performance of the FLC. There are two types of the synthesis of the fuzzy sets and the neural networks:

1. **The Neural Network and the Fuzzy Set:** The fuzzy set and the neural network are used independently in fuzzy control system or either one serves as a preprocessor for the other. For example, the fuzzy set can be used as a supervisor for the neural network in order to improve convergence of learning. The learning rate is determined by using fuzzy rules.

2. **The Neural-like Fuzzy Set:** The neural network uses the fuzzy neurons that are described by fuzzy sets, instead of the non-fuzzy neuron. In this case, antecedents and consequents in the 'if-then” rules are treated as fuzzy sets.

The work of using FNN to improve the overall performance of the FLC need to be studied in the future.

- Fuzzy control systems are essentially non-linear systems. For this reason it is difficult to obtain general results on the analysis and design of the fuzzy controller. In the fuzzy control literature, the stability analysis of fuzzy controller is usually done in the context of the following two views of the system under control:
1. Classical non-linear dynamic systems theory: the system under control is a non-fuzzy system, and the fuzzy controller is a particular class of non-linear controller;

2. Dynamic fuzzy systems.

Although the optimised fuzzy controllers work satisfactorily in practice in this research work, mathematical studies of controllability and stability in fuzzy control systems need to be investigated in depth in further work.

- Although the optimised fuzzy controller has been experimentally implemented in the Power Laboratory, the algorithm and methodology need to be implemented in the actual power system in the future.
Appendix A

Mathematical Model of the Synchronous Machine

A.1 Mathematical Model of the Synchronous Machine

In this section a brief introduction is given to the mathematical model of a synchronous machine connected to a very large power system through transmission lines for use in the design of the AVR.

Two models have been developed [Anderson, 1977]:

- Current model, using the currents as state variables;
- Flux linkage model, using the fluxes as state variables.

The synchronous machine under consideration is assumed to have:

- three stator windings sa-fa, sb-fb, and sc-fc;
- one field winding F-F';
- two amortisseur (damper) windings D-D' and Q-Q'.
These six windings are magnetically coupled. The type of the generator used is a salient pole type.

Let the positive directions of stator currents be the directions of leaving the machine terminals. The sign convention of torque is that a positive (driving) torque $T_m(t)$ accelerates the shaft, whereas a positive electrical (retarding or load) torque $T_e(t)$ decelerates the shaft. The definition of the position of the $d$-axis and $q$-axis is described in detail in [Anderson, 1977].

For the six-winding salient-pole synchronous generator, it is assumed that:

- There is no saturation and there is no distributed material in which eddy currents can flow [Adkins, 1975];
- The harmonics above second-order can be neglected, thus all the inductances vary sinusoidally with an additional constant term in some cases [Adkins, 1975], [Rafian, 1987];
- The machine is operating under balanced conditions [Anderson, 1977].

In the following equations all quantities are normalised in per unit except that time $t$ is in seconds. The mechanical torque $T_m(t)$ and the electrical torque $T_e(t)$ are normalised on a three-phase base.

### A.1.1 Flux Linkage Equations

The flux linkage equation for the six windings are as shown in equation (A.1):

$$
\begin{bmatrix}
\lambda_a(t) \\
\lambda_b(t) \\
\lambda_c(t) \\
\lambda_F(t) \\
\lambda_D(t) \\
\lambda_Q(t)
\end{bmatrix} =
\begin{bmatrix}
L_{aa} & L_{ab} & L_{ac} & L_{aF} & L_{aD} & L_{aQ} \\
L_{ba} & L_{bb} & L_{bc} & L_{bF} & L_{bD} & L_{bQ} \\
L_{ca} & L_{cb} & L_{cc} & L_{cF} & L_{cD} & L_{cQ} \\
L_{Fa} & L_{Fb} & L_{Fc} & L_{FF} & L_{FD} & L_{FQ} \\
L_{Da} & L_{Db} & L_{Dc} & L_{DF} & L_{DD} & L_{DQ} \\
L_{Qa} & L_{Qb} & L_{Qc} & L_{QF} & L_{QD} & L_{QQ}
\end{bmatrix}
\begin{bmatrix}
i_a(t) \\
i_b(t) \\
i_c(t) \\
i_F(t) \\
i_D(t) \\
i_Q(t)
\end{bmatrix}
$$

(A.1)
where $L_{jk} = \begin{cases} 
\text{self-inductance} & \text{when } j = k \\
\text{mutual inductance} & \text{when } j \neq k 
\end{cases}$

and

where $L_{jk} = L_{kj}$ in all cases.

Note that in equation (A.1) lower-case subscripts are used for stator quantities and upper-case subscripts are used for rotor quantities. Most of the inductances in equation (A.1) are functions of the rotor position angle $\theta(t)$. Also observe that nearly all terms in the matrix of equation (A.1) are time-varying, since $\theta$ is a function of time. The time varying inductances can be simplified by referring all quantities to a rotor frame of reference through Park’s transformation [Anderson, 1977]. After utilising Park’s transformation, the flux linkage equation can be expressed in the following equation:

\[
\begin{bmatrix}
\lambda_0(t) \\
\lambda_d(t) \\
\lambda_q(t) \\
\lambda_F(t) \\
\lambda_D(t) \\
\lambda_Q(t)
\end{bmatrix} =
\begin{bmatrix}
L_0 & 0 & 0 & 0 & 0 & 0 \\
0 & L_d & 0 & kM_F & kM_D & 0 \\
0 & 0 & L_q & 0 & 0 & kM_Q \\
0 & kM_F & 0 & L_F & M_R & 0 \\
0 & kM_D & 0 & M_R & L_D & 0 \\
0 & 0 & kM_Q & 0 & 0 & L_Q
\end{bmatrix}
\begin{bmatrix}
i_0(t) \\
i_d(t) \\
i_q(t) \\
i_F(t) \\
i_D(t) \\
i_Q(t)
\end{bmatrix} \tag{A.2}
\]

where

- $\lambda_d$ is the flux linkage on the d-axis of the rotor;
- $\lambda_q$ is the flux linkage on the q-axis of the rotor;
- $\lambda_0$ is completely uncoupled from the other circuits;
- $M_R$ is the mutual inductance between windings $F$ and $D$;
- $M_F$ is the mutual inductance between stator and rotor windings;
- $M_D$ is the mutual inductance between phase windings to damper winding $D$;
- $M_Q$ is the mutual inductance between phase windings to damper winding $Q$;
- $k = \sqrt{3}/2$
Appendix A. Mathematical Model of the Synchronous Machine

It can also be observed that the inductance matrix of equation (A.2) is a matrix of constants (all quantities have only one subscript). The advantage of Park’s transformation is such that it removes the time-varying coefficients.

A.1.2 Voltage Equations

The generator voltage equations are of the form [Anderson, 1977]:

\[ v(t) = \pm \sum r i(t) \pm \sum \dot{\lambda}(t) \]  

(A.3)

where \( \lambda(t) \) is the flux linkage, \( r \) is the winding resistance, and \( i(t) \) is the current. The matrix equation can be written in equation (A.4):

\[
\begin{bmatrix}
  v_a(t) \\
  v_b(t) \\
  v_c(t) \\
  -v_F(t) \\
  0 \\
  0 \\
\end{bmatrix} =
\begin{bmatrix}
  r_a & 0 & 0 & 0 & 0 \\
  0 & r_b & 0 & 0 & 0 \\
  0 & 0 & r_c & 0 & 0 \\
  0 & 0 & 0 & r_F & 0 \\
  0 & 0 & 0 & 0 & r_Q \\
\end{bmatrix}
\begin{bmatrix}
  i_a(t) \\
  i_b(t) \\
  i_c(t) \\
  i_F(t) \\
  i_Q(t) \\
\end{bmatrix} -
\begin{bmatrix}
  \dot{\lambda}_a(t) \\
  \dot{\lambda}_b(t) \\
  \dot{\lambda}_c(t) \\
  \dot{\lambda}_F(t) \\
  \dot{\lambda}_Q(t) \\
\end{bmatrix} +
\begin{bmatrix}
  V_a(t) \\
  0 \\
\end{bmatrix}  
\]

(A.4)

For balanced conditions \( r = r_a = r_b = r_c \). The equation (A.4) is complicated by the presence of time-varying coefficients in the \( \dot{\lambda}(t) \) term, but these terms can be eliminated by applying a Park’s transformation to the stator partition. The resulting equation is shown below:
For balanced conditions the zero-sequence voltage is zero and equation (A.5) can be written as:

\[
\begin{bmatrix}
\lambda_0(t) \\
\dot{\lambda}_d(t) \\
\dot{\lambda}_q(t) \\
\dot{\lambda}_F(t) \\
\dot{\lambda}_D(t) \\
\dot{\lambda}_Q(t)
\end{bmatrix}
= 
\begin{bmatrix}
0 & -\omega(t)\lambda_q(t) & 0 \\
-\omega(t)\lambda_d(t) & \omega(t)\lambda_d(t) & 0 \\
0 & 0 & 0 \\
0 & 0 & 0 \\
0 & 0 & 0
\end{bmatrix}
\begin{bmatrix}
\dot{i}_d(t) \\
\dot{i}_q(t) \\
\dot{i}_F(t) \\
\dot{i}_D(t) \\
\dot{i}_Q(t)
\end{bmatrix}
- 
\begin{bmatrix}
3r_n\dot{i}_d(t) + 3L_n\dot{i}_0(t) \\
0 \\
0 \\
0 \\
0
\end{bmatrix}
\] (A.5)

A.1.3 Torque and Power Equations

Expressing the total accelerating torque as

\[
T_a(t) = 2H\dot{\omega}(t) = T_m(t) - T_e(t) - T_d(t)
\] (A.7)

where

* $T_e(t)$ is the electrical torque,
\( T_d(t) = D\omega(t) \) \hspace{1cm} (A.8)

where \( D \) is the damping constant.

\[
T_s(t) = i_q(t)\lambda_d(t) - i_d(t)\lambda_q(t)
\] \hspace{1cm} (A.9)

The electrical power \( P_e(t) \) is shown in the following equation:

\[
P_e(t) = T_e(t)\omega(t)
\] \hspace{1cm} (A.10)

### A.1.4 Swing Equation

The swing equation is written as

\[
\delta(t) = \omega_0\omega(t),
\] \hspace{1cm} (A.11)

\[
\dot{\omega}(t) = \frac{1}{2H}(T_m(t) - T_s(t) - D\omega(t))
\] \hspace{1cm} (A.12)

where

\[
T_m(t) = \frac{P_m(t)}{\omega(t)}
\] \hspace{1cm} (A.13)

### A.1.5 Load Equation

The external connection of the synchronous generator to the infinite bus can be described by the following equations

\[
\delta(t) = \delta_0 + \int_{\omega_0}^{\omega(t)}(\omega(t) - \omega_0)dt
\] \hspace{1cm} (A.14)
in radians or

\[ \dot{\delta}(t) = \omega(t) - 1 \]  

(A.15)

in pu.

\[ v_{0dq}(t) = V_{\infty} \sqrt{3} \begin{bmatrix} 0 \\ -\sin(\delta(t) - \alpha) \\ \cos(\delta(t) - \alpha) \end{bmatrix} + R_e i_{0dq}(t) + L_e i_{0dq}(t) - \omega(t) L_e \begin{bmatrix} 0 \\ -i_q(t) \\ i_d(t) \end{bmatrix} \]  

(A.16)

Expressing the synchronous machine terminal voltage \( V_t \) in rms equivalent variables

\[ V_t(t) = \sqrt{V_d(t)^2 + V_q(t)^2} \]  

(A.17)

where \( V_d(t) = v_d(t)/\sqrt{3}, \ V_q(t) = v_q(t)/\sqrt{3} \).

\[ I_t(t) = \sqrt{I_d(t)^2 + I_q(t)^2} \]  

(A.18)

where \( I_d(t) = i_d(t)/\sqrt{3}, \ I_q(t) = i_q(t)/\sqrt{3} \).

### A.1.6 Formulation of State-Space Equations

The objective is to derive a set of equations describing the synchronous machine in the form of equation (A.19)

\[ \dot{x} = f(x, u, t) \]  

(A.19)

where

- \( x \) is a vector of the state variables;
- \( u \) is the system driving function;
- \( f \) is a set of nonlinear function.
Appendix A. Mathematical Model of the Synchronous Machine

If the equations describing the synchronous machine are linear, equation (A.19) is of the well known form

\[ \dot{x} = Ax + Bu \tag{A.20} \]

Examining equation (A.6), it can be seen that this represents a set of first order differential equations. On putting this set in the form of the equation (A.20), it can be noted that equation (A.6) contains flux linkages and currents as variables.

### A.1.7 Current Model

From equation (A.2), compute the values of $\lambda$ and $\dot{\lambda}$. Substituting these results into equation (A.6) to replace the terms in $\lambda$ and $\dot{\lambda}$ by terms in $i$ and $\dot{i}$ and rearranging

\[
\begin{bmatrix}
v_d(t) \\
-v_F(t) \\
v_q(t) \\
0
\end{bmatrix}
= \begin{bmatrix}
r & 0 & 0 & (\omega(t)L_q & (\omega(t)kM_Q) \\
0 & r_F & 0 & 0 & 0 \\
-\omega(t)L_d & -\omega(t)kM_F & -\omega(t)kM_D & 0 & 0 \\
0 & 0 & 0 & 0 & r_Q
\end{bmatrix}
\begin{bmatrix}
i_d(t) \\
i_F(t) \\
i_D(t) \\
i_q(t)
\end{bmatrix}
\]

Using matrix notation, equation (A.21) is written as

\[
v(t) = -(R + \omega(t)N)i(t) - Li(t) \tag{A.22}
\]
If the inverse of the inductance matrix exists, it can be assumed that

\[ \dot{i}(t) = -L^{-1}(R + \omega(t)N)i - L^{-1}v(t) \] (A.23)

This equation has the desired state-space form.

From equation (A.2) the flux linkage can be expressed in terms of current

\[ \lambda_d(t) = L_d i_d(t) + k M_F i_F(t) + k M_D i_D(t), \quad \lambda_q(t) = L_q i_q(t) + k M_Q i_Q(t) \] (A.24)

Thus the electrical torque equation can be written as

\[
T_e(t) = \begin{bmatrix}
L_d i_d(t) & k M_F i_q(t) & k M_D i_q(t) & -L_q i_d(t) & -k M_Q i_d(t)
\end{bmatrix}
\begin{bmatrix}
i_d(t) \\
i_F(t) \\
i_D(t) \\
i_q(t) \\
i_Q(t)
\end{bmatrix}
\] (A.25)

By substituting equation (A.25) into equation (A.7), the swing equation may be written as

\[ \dot{\omega}(t) = \frac{T_m(t)}{2H} + \]

\[
\begin{bmatrix}
-\frac{L_d i_d(t)}{2H} & -\frac{k M_F i_q(t)}{2H} & -\frac{k M_D i_q(t)}{2H} & -\frac{L_q i_d(t)}{2H} & -\frac{k M_Q i_d(t)}{2H} & -\frac{D}{2H}
\end{bmatrix}
\begin{bmatrix}
i_d(t) \\
i_F(t) \\
i_D(t) \\
i_q(t) \\
i_Q(t) \\
\omega(t)
\end{bmatrix}
\] (A.26)

Define \( K = \sqrt{3}V_\infty \) and \( \gamma(t) = \delta(t) - \alpha \) and let

\[ \hat{R} = r + R_e, \quad \hat{L}_d = L_d + L_e, \quad \hat{L}_q = L_q + L_e \] (A.27)
Incorporating the above equations into equation (A.22), the current model is shown in the following state-space equation:

\[
\begin{bmatrix}
\dot{i}_d(t) \\
\dot{i}_F(t) \\
\dot{i}_D(t) \\
\dot{i}_q(t) \\
\dot{i}_Q(t) \\
\dot{\omega}(t) \\
\dot{\delta}(t)
\end{bmatrix} =
\begin{bmatrix}
-L_{a2}(t) - k_{M_F a2}(t) - L_{a d}(t) - k_{M_F a d}(t) & -kM_{D i2}(t) - kM_{Q i2}(t) & 0 & 0 \\
0 & -\hat{L}^{-1}(\hat{R} + \omega(t)\hat{N}) & 0 & 0 \\
0 & 0 & 1 & 0 \\
0 & 0 & 0 & 1 \\
0 & 0 & 0 & 1 \\
0 & 0 & 0 & 1 \\
0 & 0 & 0 & 1
\end{bmatrix}
\begin{bmatrix}
i_d(t) \\
i_F(t) \\
i_D(t) \\
i_q(t) \\
i_Q(t) \\
\omega(t) \\
\delta(t)
\end{bmatrix}
\]

\[
+ \begin{bmatrix}
-K \sin(\gamma(t)) \\
-v_F(t) \\
K \cos(\gamma(t)) \\
0 \\
T_m(t) \\
-1
\end{bmatrix}
\]

The system described by the above equation is in the state-space form of \( \dot{x} = Ax + Bu \) where \( u \) contains the system driving functions \( v_F(t) \) and \( T_m(t) \). The state \( x \) equal to \([i_d(t) \ i_F(t) \ i_D(t) \ i_q(t) \ i_Q(t) \ \omega(t) \ \delta(t)]\). The loading effect of the transmission line is incorporated in the matrix \( \hat{R}, \hat{L}, \) and \( \hat{N} \). The infinite bus voltage \( V_{\infty} \) appears in the term \( K \sin(\gamma(t)) \) and \( K \cos(\gamma(t)) \).

Similar procedure can be adopted to derive the flux linkage model [Anderson, 1977].


A.2 Linearisation of the Non-linear Power System Model

In this section the non-linear current power system model derived in Section A.1 is linearised.

For the power system described previously, the non-linearities are mainly characterised by the product non-linearities and the trigonometric non-linearities.

Most methods for the design of power system controllers in the literature are based on linearised models of power systems. Linearisation of the non-linear power system about a steady-state operating point provides information on the small-perturbation dynamic behaviour of the system at the specified operating point. When a power system is subject to a small perturbation, it tends to acquire a new operating state. During the transition between the initial state and the new state the system behaviour is oscillatory. If the two states are such that all the state variables change slightly, the system is operating near the initial state. The initial operating condition may be considered as a quiescent operating condition for the system. The linear equations thus derived are assumed to be valid in a region near the quiescent condition.

A.2.1 Linearisation of the Generator State-Space Current Model

Let the state-space vector $x$ have an initial state $x_0$ at time $t = t_0$. At the occurrence of a small disturbance, the state will change slightly from their previous values

$$x = x_0 + x_\Delta$$

(A.29)

The state-space model is in the form

$$\dot{x} = Ax + Bu$$

(A.30)
by substituting equation (A.29) into equation (A.30)

$$\dot{x}_0 + \dot{x}_\Delta = A(x_0)(x_0 + x_\Delta) + B(x_0)u = A(x_0)x_0 + A(x_0)x_\Delta + B(x_0)u \quad (A.31)$$

since $\dot{x}_0 = A(x_0)x_0$, the linearised state-space equation can be obtained as

$$\dot{x}_\Delta = A(x_0)x_\Delta + B(x_0)u \quad (A.32)$$

The linearised system equation for a synchronous machine (not including the load equation) can be expressed as in equation (A.33):

$$
\begin{bmatrix}
v_{d\Delta}(t) \\
v_{F\Delta}(t) \\
v_{\phi\Delta}(t) \\
T_{m\Delta}(t)
\end{bmatrix} =
\begin{bmatrix}
r & 0 & 0 & \omega_0 L_q & \omega_0 k M_Q & \lambda_{q0} & 0 \\
0 & r_F & 0 & 0 & 0 & 0 & 0 \\
0 & 0 & r_D & 0 & 0 & 0 & 0 \\
-\omega_0 L_q & -\omega_0 k M_F & -\omega_0 k M_D & r & 0 & -\lambda_{d0} & 0 \\
0 & 0 & 0 & 0 & r_Q & 0 & 0 \\
0 & 0 & 0 & 0 & 0 & 0 & -D
\end{bmatrix}
\begin{bmatrix}
i_{d\Delta}(t) \\
i_{F\Delta}(t) \\
i_{\phi\Delta}(t) \\
T_{m\Delta}(t)
\end{bmatrix}$$

$$
\begin{bmatrix}
i_{d\Delta}(t) \\
i_{F\Delta}(t) \\
i_{\phi\Delta}(t) \\
\omega_{\Delta}(t) \\
\delta_{\Delta}(t)
\end{bmatrix} =
\begin{bmatrix}
L_d & k M_F & k M_D & 0 & 0 & 0 & 0 \\
k M_F & L_F & M_R & 0 & 0 & 0 & 0 \\
k M_D & M_R & L_D & 0 & 0 & 0 & 0 \\
0 & 0 & 0 & L_q & k M_Q & 0 & 0 \\
0 & 0 & 0 & k M_Q & L_Q & 0 & 0 \\
0 & 0 & 0 & 0 & 0 & -2 H & 0
\end{bmatrix}
\begin{bmatrix}
i_{d\Delta}(t) \\
i_{F\Delta}(t) \\
i_{\phi\Delta}(t) \\
\omega_{\Delta}(t) \\
\delta_{\Delta}(t)
\end{bmatrix} \quad (A.33)
$$

### A.2.2 Linearisation of the Load Equation for the Single-machine Infinite Bus Power System

Equation (A.16) is repeated here for convenience:
$$v_d(t) = -K \sin(\delta(t) - \alpha) + R_e i_d(t) + L_e \dot{i}_d(t) + \omega(t) L_e i_q(t),$$

$$v_q(t) = K \cos(\delta(t) - \alpha) + R_e i_q(t) + L_e \dot{i}_q(t) - \omega(t) L_e i_d(t) \quad (A.34)$$

where $K = \sqrt{3} V_\infty$ and $\alpha$ is the angle of $\tilde{V}_\infty$.

The linearised load equation is expressed as

$$v_{d\Delta}(t) = -K \cos(\delta_0 - \alpha) \delta(t) + R_e i_{d\Delta}(t) + \omega_0 L_e i_{q\Delta}(t) + i_{q0} L_e \omega(t) + L_e \dot{i}_{d\Delta}(t),$$

$$v_{q\Delta}(t) = -K \sin(\delta_0 - \alpha) \delta(t) + R_e i_{q\Delta}(t) + L_e \dot{i}_{q\Delta}(t) - \omega_0 L_e i_{d\Delta}(t) - i_{d0}(t) L_e \omega(t) \quad (A.35)$$

By substituting and rearranging, the linearised system equation can be obtained as:
Note that the only driving functions in the system equation (A.36) are the field voltage $v_{F\Delta}(t)$ and the mechanical torque $T_{m\Delta}(t)$.

### A.3 Simplified Linear Model

A simplified linear model for a synchronous machine connected to an infinite bus through a transmission line having resistance $R_e$ and inductance $L_e$ (or a reactance $X_e$) can be developed [Hefron, 1952], [DeMello, 1969]. Let the following assumptions
Appendix A. Mathematical Model of the Synchronous Machine

be made:

1. Amortisseur effects are neglected;
2. Stator winding resistance is neglected;
3. The $\lambda_d$ and $\lambda_q$ terms in the stator and load voltage equations are neglected compared to the speed voltage terms $\omega\lambda_q$ and $\omega\lambda_d$;
4. The terms $\omega\lambda$ in the stator and load voltage equations are assumed to be approximately equal to $\omega_R\lambda$;
5. Balanced conditions are assumed and saturation effects are neglected.

Based on the above assumptions, the simplified linear model can be achieved by using a number of steps which are described below.

**Step 1: The $E'$ equation**

The field equation are given by

$$v_F(t) = r_Fi_F(t) + \lambda_F(t), \quad \lambda_F(t) = L_Fi_F(t) + kM_Fi_d(t) \quad (A.37)$$

Eliminating $i_F(t)$

$$v_F(t) = \frac{r_F}{L_F}(\lambda_F(t) - kM_Fi_d(t)) + \lambda_F(t) \quad (A.38)$$

Let $e_q'(t) = \sqrt{3}E_q'(t)$ be the stator $EMF$ proportional to the main winding flux linkage the stator; i.e., $\sqrt{3}E_q'(t) = \omega_RkM_F\lambda_F(t)/L_F$. Also let $E_{FD}(t)$ be the stator $EMF$ that is produced by the field current and corresponds to the field voltage $v_F(t)$; i.e.,

$$\sqrt{3}E_{FD}(t) = \omega_RkM_Fv_F(t)/r_F \quad (A.39)$$

Using the above definition and the definition of $\tau_{d0}'$, equation (A.38) can be expressed in the $s$ domain

$$E_{FD} = (1 + \tau_{d0}'s)E_q' - (x_d - x_d')I_d \quad (A.40)$$
where $I_d = i_d / \sqrt{3}$.

Using the above definition for $E'_q$, the second equation in (A.37) can be arranged as follows

$$E'_q(t) = \omega R_k M_F i_F(t) / \sqrt{3} + (x_d - x'_d) I_d(t) = E(t) + (x_d - x'_d) I_d(t) \quad (A.41)$$

From the voltage equation and the assumptions made in the simplified model, voltage $v_d$ and $v_q$ for infinite bus loading can be computed

$$v_d(t) = -\omega R_d i_q(t) = -\sqrt{3} V_\infty \sin(\delta(t) - \alpha) + R_e i_d(t) + \omega R_L i_q(t)$$
$$v_q(t) = \omega R_d i_d(t) + \omega R_k M_F i_F(t) = \sqrt{3} V_\infty \cos(\delta(t) - \alpha) + R_e i_q(t) - \omega R_L i_d(t) \quad (A.42)$$

Linearising equation (A.42),

$$0 = -R_e i_q(t) + (x_d + X_e) i_d(t) + \omega R_k M_F i_F(t) + [K \sin(\delta(t) - \alpha)] \delta(t)$$
$$0 = -R_e i_d(t) - (x_q + X_e) i_q(t) + [K \cos(\delta(t) - \alpha)] \delta(t) \quad (A.43)$$

where $K = \sqrt{3} V_\infty$ and $V_\infty$ is the infinite bus voltage to neutral.

Rearranging equation (A.41) and equation (A.43),

$$-(x'_d + X_e) I_d(t) + R_e I_q(t) = E'_q(t) + [V_\infty \sin(\delta(t) - \alpha)] \delta(t)$$
$$R_e I_d(t) + (x_q + X_e) I_q(t) = [V_\infty \cos(\delta(t) - \alpha)] \delta(t) \quad (A.44)$$

Solving equation (A.44) for $I_d(t)$ and $I_q(t)$

$$\begin{bmatrix} I_d(t) \\ I_q(t) \end{bmatrix} = K_I \begin{bmatrix} -(x_q + X_e) R_e \cos(\delta(t) - \alpha) - (x_q + X_e) \sin(\delta(t) - \alpha) \\ R_e (x'_d + X_e) \cos(\delta(t) - \alpha) + R_e \sin(\delta(t) - \alpha) \end{bmatrix} \begin{bmatrix} E'_q(t) \\ V_\infty \delta(t) \end{bmatrix} \quad (A.45)$$
where

\[ K_I = \frac{1}{R_e^2 + (x_q + X_e)(x'_d + X_e)} \]  \hspace{1cm} (A.46)

Substituting \( I_d \) into an incremental version of equation (A.40) to compute

\[ E_{FD} = \frac{1}{K_3 + \tau_{d0}s}E'_q\Delta + K_4\delta_\Delta \]  \hspace{1cm} (A.47)

where \( K_3 \) and \( K_4 \) are defined as follows:

\[ K_3 = \frac{1}{[1 + K_I(x_d - x'_d)(x_q + X_e)]} \]  \hspace{1cm} (A.48)

\[ K_4 = V_\infty K_I(x_d - x'_d)[(x_q + X_e)\sin(\delta_0 - \alpha) - R_e\cos(\delta_0 - \alpha)] \]  \hspace{1cm} (A.49)

where \( K_3 \) is an impedance factor that takes into account the loading effect of the external impedance. \( K_4 \) is related to the demagnetizing effect of a change in the rotor angle; i.e.,

\[ K_4 = \frac{1}{K_3}\frac{E'_q}{\delta_\Delta}|_{E_{FD}=\text{constant}} \]  \hspace{1cm} (A.50)

From equations (A.47), (A.48) and (A.49), the following s domain relation can be derived

\[ E'_q\Delta = \frac{K_3}{1 + K_3\tau_{d0}s}E_{FD\Delta} - \frac{K_3K_4}{1 + K_3\tau_{d0}s}\delta_\Delta \]  \hspace{1cm} (A.51)
Step 2: Electrical torque equation

The pu electrical torque $T_e(t)$ is numerically equal to the three-phase power. Therefore,

$$T_e(t) = \frac{1}{3}(v_d(t)i_d(t) + v_q(t)i_q(t)) \quad (A.52)$$

Under the assumptions used in this model

$$V_d(t) = -x_qI_q(t), \quad V_q(t) = x_dI_d(t) + \omega_RkM_Fi_F(t)/\sqrt{3} \quad (A.53)$$

Using equation (A.41) in the second equation of equation (A.42),

$$V_d(t) = -x_qI_q(t), \quad V_q(t) = x_dI_d(t) + E'_q(t) \quad (A.54)$$

From equation (A.54) and equation (A.52)

$$T_e(t) = [E'_q(t) - (x_q - x_q')I_d(t)]I_q(t) \quad (A.55)$$

Linearising equation (A.55)

$$T_e\Delta(t) = I_{q0}E'_q\Delta(t) + [E'_q - (x_q - x_q')I_{q0}]I_{q\Delta}(t) - (x_q - x_q')I_{q0}I_{d\Delta}(t)$$
$$= I_{q0}E'_q\Delta(t) + E_{qao}I_{q\Delta}(t) - (x_q - x_q')I_{q0}I_{d\Delta}(t) \quad (A.56)$$

where $E_{qao}(t) = E(t) + (x_d - x_q)I_d(t)$ with $E$ taken from equation (A.41) to write the initial condition

$$E_{qao} = E_0 + (x_d - x_q)I_{d0}$$
$$= E'_q - (x_d - x_d')I_{d0} + (x_d - x_q)I_{d0}$$
$$= E'_q - (x_q - x_d')I_{d0} \quad (A.57)$$
The incremental torque can be computed by substituting equation (A.45) and equation (A.46) into equation (A.56)

\[ T_e \Delta(t) = K_1 V_{\infty} \{ E_{q0} [R_e \sin(\delta_0 - \alpha) + (x'_d + X_e) \cos(\delta_0 - \alpha)] + 
\]

\[ I_q [x_q - x'_d] [(x_q + X_e) \sin(\delta_0 - \alpha) - R_e \cos(\delta_0 - \alpha)] \} \delta(t) + 
\]

\[ K_1 \{ I_q [R_e^2 + (x_q + X_e)^2] + E_{q0} R_e \} E_{q0}'(t) \equiv K_1 \delta(t) + K_2 E_{q0}'(t) \] (A.58)

Where \( K_1 \) is the change in electrical torque for a small change in rotor angle at constant \( d \)-axis flux linkage.

\[ K_1 = \frac{T_e \Delta(t)}{\delta \Delta(t)} \bigg|_{E_{q0}=E_{q0}'} = K_1 V_{\infty} \{ E_{q0} [R_e \sin(\delta_0 - \alpha) + (x'_d + X_e) \cos(\delta_0 - \alpha)] + 
\]

\[ (i_q / \sqrt{3}) (x_q - x'_d) [(x_q + X_e) \sin(\delta_0 - \alpha) - R_e \cos(\delta_0 - \alpha)] \} \] (A.59)

\( K_2 \) is the change in electrical torque for a small change in \( d \)-axis flux linkage at constant rotor angle.

\[ K_2 = \frac{T_e \Delta(t)}{E_{q0}'(t)} \bigg|_{\delta = \delta_0} = \frac{K_1 \{ R_e E_{q0} + (i_q / \sqrt{3}) [R_e^2 + (x_q + X_e)^2] \} \} \] (A.60)

**Step 3: Terminal voltage equation**

The synchronous machine terminal voltage \( V(t) \) is given by equation (A.17). This equation is linearised to obtain

\[ V_{t \Delta}(t) = (V_{d0}/V_{q0}) V_{d \Delta}(t) + (V_{q0}/V_{q0}) V_{q \Delta}(t) \] (A.61)
Substituting equation (A.54) in equation (A.61),

\[ V_{\Delta}(t) = -(V_{d0}/V_{t0})x_qI_{\Delta}(t) + (V_{q0}/V_{t0})(x'_dI_{\Delta}(t) + E'_{q\Delta}(t)) \]  (A.62)

Substituting for \( I_q(t) \) and \( I_d(t) \) from equation (A.45),

\[ V_{\Delta}(t) = \left\{ (K_1V_{\infty}x'_dV_{q0}/V_{t0})[R_e \cos(\delta_0 - \alpha) - (x_q + X_e) \sin(\delta_0 - \alpha)] \right. \\
- (K_1V_{\infty}x_qV_{d0}/V_{t0})[(x'_d + X_e) \cos(\delta_0 - \alpha) + R_e \sin(\delta_0 - \alpha)] \right\} \delta_{\Delta}(t) \\
+ \{(V_{q0}/V_{t0})[1 - K_1x'_d(x_q + X_e)] - (V_{d0}/V_{t0})K_1x_qR_e\}E'_{q\Delta}(t) \\
\equiv K_5\delta_{\Delta}(t) + K_EE'_{q\Delta}(t) \]  (A.63)

\( K_5 \) is the change in the terminal voltage \( V_{\Delta}(t) \) for a small change in rotor angle at constant \( d \)-axis flux linkage.

\[ K_5 = \frac{V_{\Delta}(t)}{\delta_{\Delta}(t)} |_{E'_q=E'_{q\delta}} = \left\{ (K_1V_{\infty}x'_dV_{q0}/\sqrt{3}V_{t0})[R_e \cos(\delta_0 - \alpha) - (x_q + X_e) \sin(\delta_0 - \alpha)] \right. \\
- (K_1V_{\infty}x_qV_{d0}(\sqrt{3}V_{t0})[(x'_d + X_e) \cos(\delta_0 - \alpha) + R_e \sin(\delta_0 - \alpha)] \right\} \]  (A.64)

\( K_6 \) is the change in the terminal voltage \( V_{\Delta}(t) \) for a small change in the \( d \)-axis flux linkage at constant rotor angle.

\[ K_6 = \frac{V_{\Delta}(t)}{E'_{q\Delta}(t)} |_{\delta=\delta_0} = \left\{ (K_1V_{\infty}x'_dV_{q0}/\sqrt{3}V_{t0})\{(V_{q0}/\sqrt{3}V_{t0})[1 - K_1X'_d(X_q + X_e)] - (V_{d0}/\sqrt{3}V_{t0})K_1X_qR_e\} \right. \\
\]  (A.65)

This model is a substantial improvement over the classical model since it accounts for the demagnetizing effects of the armature reaction through the change in \( E'_{q\Delta}(t) \) due to change in \( \delta_{\Delta}(t) \).
Appendix B

Introduction to Fuzzy Set Theory

B.1 Fuzzy Sets and Terminology

A fuzzy set is an extension of a crisp set. Fuzzy sets allow partial membership. An element may partially belong to a set.

In a crisp set membership of an element $u$ in a set $F$ is described by a characteristic function $\mu_F(u)$, where

$$\mu_F(u) = \begin{cases} 1 & \text{if } u \in F \\ 0 & \text{if } u \notin F \end{cases} \quad (B.1)$$

Let $U$ be a collection of objects whose generic elements are denoted by $u$, which could be discrete or continuous, $U$ is called the Universe of Discourse.

Fuzzy Set

A fuzzy set $F$ in a universe of discourse $U$ is characterised by a membership function $\mu_F$ which takes values in the interval $[0,1]$ namely, $\mu_F : U \to [0,1]$. A fuzzy set may be viewed as a generalisation of the concept of an ordinary crisp set whose membership function takes only two values $\{0, 1\}$. Thus a fuzzy set $F$ in $U$ may be represented as a set of ordered pairs of a generic element $u$ and its grade of
member function $\mu_F(u)$:

$$F = \{(u, \mu_F(u) \mid u \in U\} \quad (B.2)$$

When $U$ is continuous, a fuzzy set $F$ can be written concisely as

$$F = \int u \mu_F(u)/u \quad (B.3)$$

When $U$ is discrete, a fuzzy set $F$ can be represented as

$$F = \sum_{i=1}^{n} \mu_F(u_i)/u_i \quad (B.4)$$

It should be noted that the positive (+) sign in the summation in equation (B.4) denotes the union rather than the arithmetic sum.

**Support, Crossover Point and Fuzzy Singleton:**

The *support* of a fuzzy set $F$ is the crisp set of all points $u$ in $U$ such that $\mu_F(u) > 0$. In particular, the element $u$ in $U$ at which $\mu_F = 0.5$, is called the *crossover point* and a fuzzy set whose support is a single point in $U$ with $\mu_F = 1.0$ is referred to as *fuzzy singleton*.

**\( \alpha \)-cut of a Fuzzy Set \( F \):**

To exhibit an element $u \in U$ that typically belongs to a fuzzy set $F$, it may be demanded that its membership value to be greater than some threshold $\alpha \in [0, 1]$. The ordinary set of such elements is the $\alpha$-cut $F_\alpha$ of $F$,

$$F_\alpha = \{u \in U, \mu_F(u) \geq \alpha\} \quad (B.5)$$

One also define the strong $\alpha$-cut as:

$$F_\delta = \{u \in U, \mu_F(u) > \alpha\} \quad (B.6)$$
Height of a Fuzzy Set:

By a height of a fuzzy set, $\text{height}(F)$, it means a supremum of its membership function

$$\text{height}(F) = \sup_{u \in U} \mu_F(u) \tag{B.7}$$

If $\text{height}(F) = 1$, the set $F$ is called a normalised fuzzy set.

Fuzzy Number:

A fuzzy number $F$ in a continuous universe $U$ is a fuzzy set $F$ in $U$ which is normal and convex, i.e.,

$$\max_{u \in U} \mu_F(u) = 1 \quad \text{(normal)}$$

$$\mu_F(\lambda u_1 + (1 - \lambda)u_2) \geq \min(\mu_F(u_1), \mu_F(u_2)), \ u_1, u_2 \in U, \lambda \in [0, 1] \quad \text{(convex)} \tag{B.8}$$

B.2 Fuzzy Set Theoretical Operations

Let $A$ and $B$ be two fuzzy sets in $U$ with membership functions $\mu_A$ and $\mu_B$, respectively. The membership function is the crucial components of a fuzzy set. Therefore, the set theoretical operations of union, intersection and complement, etc., for fuzzy sets are defined via their membership functions.

- **Union (OR):**

  The membership function $\mu_{A \cup B}$ of the union $A \cup B$ is pointwise defined for all $u \in U$ by

  $$\mu_{A \cup B}(u) = \max\{\mu_A(u), \mu_B(u)\} \tag{B.9}$$

- **Intersection (AND):**

  The membership function $\mu_{A \cap B}$ of the intersection $A \cap B$ is pointwise defined for all $u \in U$ by
\[\mu_{A \cap B}(u) = \min\{\mu_A(u), \mu_B(u)\}\]  
\hspace{1cm} (B.10)

- **Complement (NOT):**

  The membership function \(\mu_A\) of the complement of a fuzzy set \(A\) is pointwise defined for all \(u \in U\) by

  \[\mu_A(u) = 1 - \mu_A(u)\]  
  \hspace{1cm} (B.11)

- **Cartesian Product:**

  If \(A_1, \cdots, A_n\) are fuzzy sets in \(U_1, \cdots, U_n\), respectively, the Cartesian product of \(A_1, \cdots, A_n\) is a fuzzy set in the product space \(U_1 \times \cdots \times U_n\) with the membership function

  \[\mu_{A_1 \times \cdots \times A_n}(u_1, u_2, \cdots, u_n) = \min\{\mu_{A_1}(u_1), \cdots, \mu_{A_n}(u_n)\}\]  
  \hspace{1cm} (B.12)

  or

  \[\mu_{A_1 \times \cdots \times A_n}(u_1, u_2, \cdots, u_n) = \mu_{A_1}(u_1) \cdot \mu_{A_2}(u_2) \cdots \mu_{A_n}(u_n)\]  
  \hspace{1cm} (B.13)

- **Triangular Norms or T-norms:**

  The triangular norm or \(t\)-norm \(*\) is a two-place function \([0, 1] \times [0, 1] \rightarrow [0, 1]\), i.e., \(*\): \([0, 1] \times [0, 1] \rightarrow [0, 1]\) which includes intersection, algebraic product, bounded product, and drastic product. The greatest triangular norm is the intersection and the least one is the drastic product. The operations associated with triangular norms are defined for all \(x, y \in [0, 1]\) by:

  intersection: \(x \circ y = \min\{x, y\}\)
  algebraic product: \(x \cdot y = xy\)
  bounded product: \(x \odot y = \max\{0, x + y - 1\}\)
Appendix B. Introduction to Fuzzy Set Theory

The triangular norms are employed for defining conjunctions in approximate reasoning.

**Triangular Co-Norms or S-norms:**
The triangular co-norm or s-norm \( + \) is a two-place function from \([0,1] \times [0,1]\) to \([0,1]\), i.e., \( + : [0,1] \times [0,1] \to [0,1]\) which includes union, algebraic sum, bounded sum, drastic sum and disjoint sum. The operations associated with triangular co-norms are defined for all \( x, y \in [0,1] \) by:

- **union:** \( x \oplus y = \max\{x, y\} \)
- **algebraic sum:** \( x \oplus y = x + y - xy \)
- **bounded sum:** \( x \ominus y = \min\{1, x + y\} \)
- **drastic sum:** \( x \triangledown y = \begin{cases} x & \text{if } y = 0 \\ y & \text{if } x = 0 \\ 1 & \text{if } x, y > 0 \end{cases} \)
- **disjoint sum:** \( x \Delta y = \max\{\min\{x, 1 - y\}, \min\{1 - x, y\}\} \) (B.15)

The triangular norms are employed for defining conjunctions in approximate reasoning, while the triangular co-norms serve the same role for disjunctions.

A fuzzy control rule, "if \( x \) is \( A \) and \( y \) is \( B \)" is represented by a fuzzy implication function and is denoted by \( A \rightarrow B \), where \( A \) and \( B \) are fuzzy sets in universes \( U \) and \( V \) with membership functions \( \mu_A \) and \( \mu_B \), respectively.

**Fuzzy Conjunction:**
The fuzzy conjunction is defined for all \( u \in U \) and \( v \in V \) by

\[
A \rightarrow B = A \times B = \int_{U \times V} \mu_A(u) \ast \mu_B(v)/(u, v) \quad (B.16)
\]
where $*$ is an operator representing a triangular norm or t-norm.

- **Fuzzy Disjunction:**

  The fuzzy disjunction is defined for all $u \in U$ and $v \in V$ by

  $$A \rightarrow B = A \times B = \int_{U \times V} \mu_A(u) \cdot \mu_B(v) / (u, v)$$

  (B.17)

  where $\cdot$ is an operator representing a triangular co-norm or s-norm.

### B.3 Linguistic Variables and Linguistic Hedges

- **Linguistic Variables**

  Fuzzy sets provide a systematic means for dealing with uncertain and imprecise notions. Of particular significance in control systems is the use of linguistic variables, which may be considered as a variable whose value is a fuzzy number or as a variable whose values are defined in linguistic terms.

  A linguistic variable is characterised by a quintuple $(x, T(x), U, G, M)$ in which $x$ is the name of variable; $T(x)$ is the term set of $x$, that is, the set of names of linguistic values of $x$ with each value being a fuzzy number defined on $U$; $G$ is a syntactic rule for generating the names of values of $x$; and $M$ is a semantic rule for associating with each value its meaning. For example, if *speed* is interpreted as a linguistic variable, then its term set $T(speed)$ could be

  $$T(speed) = \text{slow, moderate, fast, very slow, more or less fast,} \ldots$$

  where each term in $T(speed)$ is characterised by a fuzzy set in a universe of discourse $U = [0, 100]$. It might be interpreted "slow" as "a speed below about 40 kmph," "moderate" as "a speed close to 55 kmph," and "fast" as "a speed above about 70 kmph." These terms can be characterised as fuzzy sets with their membership functions.

- **Linguistic Hedges**
A major reason behind using fuzzy logic in control engineering is the use of qualitative linguistic expressions favoured by human experts and operators such as very small and rather big. The purpose of the hedges such as very, more or less etc. is to generate a larger set of values for a linguistic variable from a small collection of primary terms through the processes of intensifier or concentration, dilation and normalisation.

- **Concentration (CON(F))**: 
  The concentration operation concentrates fuzzy elements by reducing in higher grades of the membership function more than that in lower grades membership function. This operation and the following ones of dilation, intensification and normalisation have no counterpart in ordinary set operations. A common concentration operator is:
  \[
  \mu_{CON(F)}(u) = (\mu_F(u))^2 \tag{B.18}
  \]
  The concentration operator can be used to roughly approximate the effect of the linguistic modifier very. That is, for some fuzzy set \( F \)
  \[
  Very \quad F = F^2 = CON(F) \tag{B.19}
  \]
  The result of applying the operator very on a fuzzy label big is a new fuzzy label very big.

- **Dilation (DIL(F))**: 
  \[
  \mu_{DIL(F)}(u) = (\mu_F(u))^{0.5} \tag{B.20}
  \]
  The dilation operation dilates fuzzy elements by increasing the lower grades of membership function more than that in higher grades of membership function. It performs the inverse operation to concentration for these choices of powers 2 and 0.5. The dilation operator is roughly approximated by the linguistic
modifier More or Less. Thus for any fuzzy set \( F \)

\[
\text{More or Less } F = F^{0.5} = DIL(F)
\]  

(B.21)

**Intensification** (\( \text{INT}(F) \)):

\[
\mu_{\text{INT}(F)}(u) = \begin{cases} 
2(\mu_F(u))^2 & \text{for } 0 \leq \mu_F(u) \leq 0.5 \\
1 - 2(1 - \mu_F(u))^2 & \text{for } 0.5 < \mu_F(u) \leq 1
\end{cases}
\]  

(B.22)

The INT operation is like the contrast intensification of a picture. The intensification raises the membership function grade of those elements within the crossover points and reduces the membership grade of those outside the crossover points.

**Normalisation** (\( \text{NORM}(F) \)):

\[
\mu_{\text{NORM}(F)}(u) = \frac{\mu_F(u)}{\max \{\mu_F(u)\}}
\]  

(B.23)

where the \( \max \) function returns the maximum membership function for all elements \( u \). If the membership function is < 1, then all membership functions will be increased. If the \( \max = 1 \), then the membership functions are unchanged.

### B.4 Fuzzy Inference and Composition

**Fuzzy Relation**:

In control systems, relationships are defined between systems inputs and outputs. In fuzzy systems, these relationships or mappings are between fuzzy variables defined on different universe of discourse through the fuzzy conditional statement or linguistic implication which links the conditional or antecedent set with the consequent or output set. An n-ary fuzzy relation \( R \) is a fuzzy set in \( U_1 \times \cdots \times U_n \) and is expressed as
Appendix B. Introduction to Fuzzy Set Theory 209

\[ R_{U_1 \times \cdots \times U_n} = \{ ((u_1, \cdots, u_n), \mu_R(u_1, \cdots, u_n)) \mid (u_1, \cdots, u_n) \in U_1 \times \cdots \times U_n \} \]  

(B.24)

A broad class of models for logical connectives (union and intersection) is formed by triangular norms.

- **Fuzzy Relation Projection**

Given a fuzzy set \( A \in U, B \in V \), and a fuzzy relation \( R \) defined by \( A \rightarrow B \), with associated membership function \( \mu_R(u, v) \); then \( A^R \) is the projection of the binary relation \( R \) on the domain of \( A \) defined by:

\[ \mu_{A^R}(u) = \sup_{v \in V} \mu_R(u, v), \quad u \in U, v \in V \]  

(B.25)

- **Fuzzy Composition**

To adequately represent any dynamic process or to provide control, several rules in the form of conditional statements or production rules are required. It is impractical to have a rule for every possible situation, therefore use is made of the compositional rule of inference which allows rules to be used in situations not normally covered. This important rule may be viewed as a combination of the fuzzy conjunctive and projection rules.

- **Max-Min Composition:**

If \( R \) and \( S \) are fuzzy relations in \( U \times V \) and \( V \times W \), respectively, the composition of \( R \) and \( S \) is a fuzzy relation denoted by \( R \circ S \) and is defined by

\[ R \circ S = \{ [(u, w), \vee(\mu_R(u, v) \land \mu_s(v, w))] \mid u \in U, v \in V, w \in W \} \]  

(B.26)

where \( \vee \) and \( \land \) denote max and min respectively.

- **Sup-Star Composition:**
If $R$ and $S$ are fuzzy relations in $U \times V$ and $V \times W$, respectively, the composition of $R$ and $S$ is a fuzzy relation denoted by $R \circ S$ and is defined by

$$R \circ S = \{[(u, w), sup(\mu_R(u, v) \ast \mu_s(v, w))] | u \in U, v \in V, w \in W\} \ (B.27)$$

where $\ast$ could be any operator in the class of triangular norms, namely, minimum, algebraic product, bounded product, or drastic product. In addition to these basic operations, there are other operations that are used in the representation of linguistic hedges.

**Fuzzy Implication—Representing the Meaning of If-then Rules:**

In general, a fuzzy control rule is a fuzzy relation which is expressed as a fuzzy implication. Fuzzy implication may be defined in many ways and it may be expressed as a fuzzy implication function. There are nearly 40 distinct fuzzy implication functions described in the literature. In general, they can be classified into three main categories: the fuzzy conjunction, the fuzzy disjunction and the fuzzy implication. The former two which were described previously bear a close relationship to a fuzzy Cartesian product. In fuzzy logic and approximate reasoning, there are five families of fuzzy implication functions in use. These implication functions can be shown as follows:

1. Material implication: $A \rightarrow B = (not \ A) \vee B$
2. Propositional calculus: $A \rightarrow B = (not \ A) \vee (A \ast B)$
3. Extended propositional calculus: $A \rightarrow B = (not \ A \times not \ B) \vee B$
4. Generalisation of modus ponens: $A \rightarrow B = sup\{c \in [0,1], A \ast c \leq B\}$
5. Generalisation of modus tollens: $A \rightarrow B = inf\{t \in [0,1], B \oplus t \leq A\}$

Based on these definitions, many fuzzy implication functions may be generated by utilising the triangular norms and co-norms.

Mamdani’s mini-operation rule of fuzzy implication:

$$R_m = A \times B = \int_{U \times V} \mu_A(u) \land \mu_B(v) / (u, v). \ (B.28)$$
Larsen’s algebraic product operation rule of fuzzy implication:

\[ R_i = A \times B = \int_{U \times V} \mu_A(u) \mu_B(v)/(u, v). \]  (B.29)

Selecting the s-bounded sum operator (see s-norm definition) in the material implication rule leads to Zadeh’s arithmetic rule of fuzzy implication:

\[ R_{Z_a} = (\text{not } A \times V) \oplus (U \times B) = \int_{U \times V} 1 \wedge (1 - \mu_A(u) + \mu_B(v))/(u, v) \]  (B.30)

Also if the union operator is used in the material implication rule, the Boolean fuzzy implication follows:

\[ R_B = (\text{not } A \times V) \cup (U \times B) = \int_{U \times V} (1 - \mu_A(u)) \vee (\mu_B(v))/(u, v) \]  (B.31)

The fuzzy propositional implication, utilising the intersection and union operators leads to Zadeh’s max-min rule of implication:

\[ R_{Z_m} = (A \times B) \cup (\text{not } A \times V) = \int_{U \times V} (\mu_A(u) \wedge \mu_B(v)) \vee (1 - \mu_A(u))/(u, v) \]  (B.32)

The generalisation of modus ponens (GMP) with bounded product leads to the standard sequence fuzzy implication:

\[ R_s = A \times V \rightarrow U \times B = \int_{U \times V} (\mu_A(u) > \mu_B(v))/(u, v) \]  (B.33)

where

\[ \mu_A(u) > \mu_B(v) = \begin{cases} 1 & \text{if } \mu_A(u) \leq \mu_B(v) \\ 0 & \text{if } \mu_A(u) \geq \mu_B(v) \end{cases} \]  (B.34)
If instead, the algebraic product is used for GMP, Goguen’s fuzzy implication follows:

\[
R_G = A \times V \rightarrow U \times B = \int_{U \times V} (\mu_A(u) \Rightarrow \mu_B(v))/(u,v) \quad (B.35)
\]

where

\[
\mu_A(u) \Rightarrow \mu_B(v) = \begin{cases} 
1 & \text{if } \mu_A(u) \leq \mu_B(v) \\
\frac{\mu_B(u)}{\mu_A(v)} & \text{if } \mu_A(u) > \mu_B(v) 
\end{cases} 
\quad (B.36)
\]

B.5 Fuzzy Logic and Approximate Reasoning

Approximate reasoning is the best-known form of fuzzy logic and covers a variety of inference rules whose premises contain fuzzy propositions. Inference in approximate reasoning is in sharp contrast to inference in classical logic—in the former the consequence of a given set of fuzzy propositions depends on the meaning attached to these fuzzy propositions. Thus, inference in approximate reasoning is computation with fuzzy sets that represent the meaning of a certain set of fuzzy propositions. For example, given the membership functions of \( \mu_A \) and \( \mu_R \), representing the meaning of a fuzzy proposition “X is A” and the meaning of a fuzzy conditional “if X is A then Y is B,” the membership function representing the meaning of the conclusion “Y is B” can be computed.

- Inference Rules

In approximate reasoning, two inference rules are of major importance, i.e., the compositional rule of inference and the generalised modus ponens. The first rule uses a fuzzy relation to represent explicitly the connection between two fuzzy propositions, the second uses an if-then rule that implicitly represents a fuzzy relation. The generalised modus ponens has the symbolic inference scheme

\[
S_1 \text{ is } Q_1, \quad \text{if } S_1 \text{ is } P_1 \text{ then } S_2 \text{ is } P_2,
\]
\( S_2 \) is \( Q_2 \);

where \( S_1 \) and \( S_2 \) are symbolic names for objects, and \( P_1, P_2, Q_1 \) and \( Q_2 \) are objects properties.

The \textit{compositional rule of inference} can be considered to be a special case of the generalised modus ponens. Its general symbolic form is

\[
S_1 \text{ is } Q_1, \\
S_1 \text{ } R \text{ } S_2, \\
\Rightarrow S_2 \text{ is } Q_2;
\]

where \( S_1 \text{ } R \text{ } S_2 \) reads as "\( S_1 \) is in relation \( R \) to \( S_2 \)" and its meaning is represented as a fuzzy relation \( \mu_R \). Hence, instead of the if-then rule, there is a fuzzy relation \( R \).

\textbf{• Sup-Star Compositional Rule of Inference:}

If \( R \) is a fuzzy relation in \( U \times V \), and \( x \) is a fuzzy set in \( U \), then the \textit{sup-star compositional rule of inference} asserts that the fuzzy set \( y \) in \( V \) induced by \( x \) is given by

\[
y = x \circ R \tag{B.37}
\]

where \( x \circ R \) is the sup-star composition of \( x \) and \( R \). If the star represents the minimum operator, then this definition reduces to Zadeh's compositional rule of inference [Zadeh, 1973].
Appendix C

The Whole Overlap Ratio (WOR)

C.1 The WOR for Linear Membership Functions

The proposed index of the Whole Overlap Ratio:

\[
WOR = \frac{\int_{-\infty}^{\infty} \text{MIN}(\mu_1(x), \mu_2(x)) \, dx}{\int_{-\infty}^{\infty} \text{MAX}(\mu_1(x), \mu_2(x)) \, dx}
\]  \hspace{1cm} (C.1)

The expression for two adjacent linear membership functions \(\mu_1(x)\) and \(\mu_2(x)\) are:

\[
\mu_1(x) = 1 - \text{abs}(\frac{x - m_1}{\delta})
\]  \hspace{1cm} (C.2)

\[
\mu_2(x) = 1 - \text{abs}(\frac{x - m_2}{\delta})
\]  \hspace{1cm} (C.3)

This can be shown in Figure (C.1).

The maximum height \(h\) of the intersection area is:

\[
h = \frac{m_1 + m_2}{2} - \frac{(m_2 + \delta)(m_2 - m_1)}{2\delta}
\]  \hspace{1cm} (C.4)
For the intersection area:

\[
\int_{-\infty}^{\infty} \min(\mu_1(x), \mu_2(x)) \, dx \\
= \frac{1}{2} \times h \times (m_1 + m_2 + 2\delta) \\
= \frac{1}{2} \times (1 - \frac{m_2 - m_1}{2\delta})(m_1 - m_2 + 2\delta) \\
= \delta \times (1 - \frac{m_2 - m_1}{2\delta})^2
\]

(C.5)

For the whole area:

\[
\int_{-\infty}^{\infty} \max(\mu_1(x), \mu_2(x)) \, dx \\
= \frac{1}{2} \times 2\delta \times 1 + \frac{1}{2} \times 2\delta \times 1 - \int_{-\infty}^{\infty} \min(\mu_1(x), \mu_2(x)) \, dx \\
= 2\delta - \delta \times (1 - \frac{m_2 - m_1}{2\delta})^2 \\
= \delta(2 - (1 - \frac{m_2 - m_1}{2\delta})^2)
\]
The WOR for the two adjacent linear membership functions can be derived as:

\[
WOR = \frac{\int_{-\infty}^{\infty} \text{MIN}(\mu_1(x), \mu_2(x)) \, dx}{\int_{-\infty}^{\infty} \text{MAX}(\mu_1(x), \mu_2(x)) \, dx} \\
= \frac{\delta \times (1 - \frac{m_2 - m_1}{2\delta})^2}{\delta (2 - (1 - \frac{m_2 - m_1}{2\delta})^2)} \\
= \frac{1}{(1 - \frac{m_2 - m_1}{2\delta})^2 - 1}
\]

(C.7)

### C.2 The WOR for Quadratic Membership Functions

The expression for two adjacent quadratic membership functions \( \mu_1(x) \) and \( \mu_2(x) \) are:

\[
\mu_1(x) = 1 - \left( \frac{x - m_1}{\delta} \right)^2 \\
\mu_2(x) = 1 - \left( \frac{x - m_2}{\delta} \right)^2
\]

This can be shown in Figure (C.2).
For the intersection area:

\[
\int_{-\infty}^{\infty} \text{MIN}(\mu_1(x), \mu_2(x)) dx
\]

\[
= 2 \times \int_{\frac{m_1+m_2}{2}}^{\frac{m_1+m_2}{2} - \delta} (1 - \left(\frac{x-m_2}{\delta}\right)^2) dx
\]

\[
= 2 \times \int_{-1}^{\frac{m_1-m_2}{2\delta}} (1 - y^2) \delta dy
\]

\[
= 2 \times \delta \times \left(\frac{1}{3} \times \left(\frac{m_2-m_1}{2\delta}\right)^3 - \frac{m_2-m_1}{2\delta} + \frac{2}{3}\right)
\]

\[
\text{C.10)}
\]
For the whole area:

\[
\int_{-\infty}^{\infty} \max(\mu_1(x), \mu_2(x)) \, dx \\
= 2 \times \int_{m_1+m_2}^{m_2+\delta} \left(1 - \left(\frac{x - m_2}{\delta}\right)^2\right) \, dx \\
= 2 \times \int_{m_1-m_2}^{1} (1 - y^2) \, dy \\
= 2 \times 2 \times \delta \times \left(1 - \frac{1}{3} \times \left(\frac{m_2 - m_1}{2\delta}\right)^3 + \frac{m_2 - m_1}{2\delta} - \frac{1}{3}\right)
\]

(C.11)

The WOR for the two adjacent quadratic membership functions can be derived as:

\[
WOR = \frac{\int_{-\infty}^{\infty} \min(\mu_1(x), \mu_2(x)) \, dx}{\int_{-\infty}^{\infty} \max(\mu_1(x), \mu_2(x)) \, dx} \\
= \frac{2 \times \delta \times \left(\frac{1}{3} \times \left(\frac{m_2 - m_1}{2\delta}\right)^3 - \frac{m_2 - m_1}{2\delta} + \frac{2}{3}\right)}{2 \times \delta \times \left(1 - \frac{1}{3} \times \left(\frac{m_2 - m_1}{2\delta}\right)^3 + \frac{m_2 - m_1}{2\delta} - \frac{1}{3}\right)} \\
= \frac{2}{3} \left(\frac{m_2 - m_1}{2\delta}\right)^3 + \frac{1}{3} \left(\frac{m_2 - m_1}{2\delta}\right)^3 \\
= \frac{2}{3} + \frac{m_2 - m_1}{2\delta} - \frac{1}{3} \left(\frac{m_2 - m_1}{2\delta}\right)^3
\]

(C.12)
C.3 The WOR for Gaussian Membership Functions

The expression for two adjacent Gaussian (exponential) membership functions $\mu_1(x)$ and $\mu_2(x)$ are:

$$\mu_1(x) = e^{-\left(\frac{x-m_1}{\delta}\right)^2} \quad (C.13)$$

$$\mu_2(x) = e^{-\left(\frac{x-m_2}{\delta}\right)^2} \quad (C.14)$$

This can be shown in Figure (C.3).

Figure C.3: Two adjacent exponential membership functions

$$M(x) = \int_{-\infty}^{x} e^{-\left(\frac{t-m}{\delta}\right)^2} dt = \delta \sqrt{\pi} F\left(\frac{\sqrt{2}}{\delta} (x - m)\right) \quad (C.15)$$
Appendix C. The Whole Overlap Ratio

For the intersection area:

\[
\int_{-\infty}^{\infty} \text{MIN}(\mu_1(x), \mu_2(x)) \, dx
= 2 \times \int_{-\infty}^{\frac{m_1 + m_2}{2}} e^{-\frac{(x - m_2)^2}{\delta}} \, dt
= 2 \times M_1\left(\frac{m_1 + m_2}{2}\right)
= 2 \times \delta \times \sqrt{\pi} F\left(\frac{\sqrt{2}}{\delta} \times \frac{m_1 - m_2}{2}\right)
= 2 \times \delta \times \sqrt{\pi} F\left(\sqrt{2} \times \frac{m_1 - m_2}{2\delta}\right)
\]

(C.16)

For the whole area:

\[
\int_{-\infty}^{\infty} \text{MAX}(\mu_1(x), \mu_2(x)) \, dx
= 2 \times \int_{-\infty}^{\frac{m_1 + m_2}{2}} e^{-\frac{(x - m_1)^2}{\delta}} \, dt
= 2 \times \delta \times \sqrt{\pi} F\left(\sqrt{2} \times \frac{m_2 - m_1}{2\delta}\right)
\]

(C.17)

The WOR for the two adjacent Gaussian membership functions can be derived as:
\[ WOR = \frac{\int_{-\infty}^{\infty} \text{MIN}(\mu_1(x), \mu_2(x)) \, dx}{\int_{-\infty}^{\infty} \text{MAX}(\mu_1(x), \mu_2(x)) \, dx} \]

\[ = \frac{F(\sqrt{2} \times \frac{m_1 - m_2}{2\delta})}{F(\sqrt{2} \times \frac{m_2 - m_1}{2\delta})} \]

\[ = 1 - \frac{F(\sqrt{2} \times \frac{m_2 - m_1}{2\delta})}{F(\sqrt{2} \times \frac{m_2 - m_1}{2\delta})} = 1 \]

(C.18)
Appendix D

Mathematical Model for Multi-machine Power System

D.1 Statement of the Problem

The equations will be developed here is in the case where the loads are to be represented by constant impedances. The objective is to give a mathematical description of the multi-machine system with the load constraints included [Anderson, 1977].

For multi-machine system, each machine is described mathematically by a set of equations of the form

\[ \dot{x} = f(x, v, T_m, t) \]  \hspace{1cm} (D.1)

where \( x \) is a vector of state variables, \( v \) is a vector of voltages, and \( T_m \) is the mechanical torque. The dimension of the vector \( x \) depends on the model used. The order of \( x \) ranges from seventh order for the full model to second order for the classical model where only \( \omega \) and \( \delta \) are retained as the state variables.

For machine \( i \) the phasors \( \tilde{V}_i \) and \( \tilde{I}_i \) can be defined as

\[ \tilde{V}_i = V_{qi} + j V_{di} \hspace{1cm} \tilde{I}_i = I_{qi} + j I_{di} \]  \hspace{1cm} (D.2)
where

\[ V_{qi} \triangleq \frac{v_{qi}}{\sqrt{3}} \quad V_{di} \triangleq \frac{v_{di}}{\sqrt{3}} \quad I_{qi} \triangleq \frac{i_{qi}}{\sqrt{3}} \quad I_{di} \triangleq \frac{i_{di}}{\sqrt{3}} \quad (D.3) \]

and where the axis $q_i$ is taken as the phasor reference in each case. Then the complex vectors $\vec{V}$ and $\vec{I}$ can be defined by

\[
\vec{V} \triangleq \begin{bmatrix} V_{q1} + jV_{d1} \\
V_{q2} + jV_{d2} \\
\vdots \\
V_{qn} + jV_{dn} \end{bmatrix} = \begin{bmatrix} \vec{V}_1 \\
\vec{V}_2 \\
\vdots \\
\vec{V}_n \end{bmatrix} \quad \vec{I} \triangleq \begin{bmatrix} I_{q1} + jI_{d1} \\
I_{q2} + jI_{d2} \\
\vdots \\
I_{qn} + jI_{dn} \end{bmatrix} = \begin{bmatrix} \vec{I}_1 \\
\vec{I}_2 \\
\vdots \\
\vec{I}_n \end{bmatrix} \quad (D.4)
\]

The voltage $\vec{V}_i$ and the current $\vec{I}_i$ are referred to the $q$ and $d$ axes of machine $i$. In other words the different voltages and currents are expressed in terms of different reference frames. At steady state these currents and voltages can be represented by phasors to a common reference frame. To distinguish these phasors defined by (D.2), the symbols $\hat{I}_i$ and $\hat{V}_i$, $i = 1, 2, \ldots, n$ will be used to designate the use of a common frame of reference.

Similarly, the matrices $\hat{I}_i$ and $\hat{V}_i$ can be formed. From the network steady state equation

\[ \hat{I} = \hat{Y} \hat{V} \quad (D.5) \]

where

\[
\hat{I} \triangleq \begin{bmatrix} \hat{I}_1 \\
\hat{I}_2 \\
\vdots \\
\hat{I}_n \end{bmatrix} \quad \hat{V} \triangleq \begin{bmatrix} \hat{V}_1 \\
\hat{V}_2 \\
\vdots \\
\hat{V}_n \end{bmatrix} \quad (D.6)
\]

and $\hat{Y}$ is the short circuit admittance matrix of the network.
D.2 Conversion to a Common Reference Frame

To obtain general network relationships, it is desirable to express the various branch quantities to the same reference. Let us assume that we want to convert the phasor $\vec{V}_i = V_{qi} + jV_{di}$ to the common reference frame (moving at synchronous speed). Let the same voltage, expressed in the new notation, be $\hat{V}_i = V_Q + jV_D$ as shown in Figure (D.1)

![Figure D.1: Two frames of reference for phasor quantities for a voltage $V_i$](image)

From Figure (D.1) it can be seen that

$$V_{Qi} + jV_{Di} = (V_{qi}\cos\delta_i - V_{di}\sin\delta_i) + j(V_{qi}\sin\delta_i + V_{di}\cos\delta_i)$$

or

$$\hat{V}_i = V_i e^{j\delta_i} \quad (D.7)$$

Convert network branch voltage drop equation to the system reference frame by using (D.7)

$$\hat{V}_k e^{-j\delta_i} = \hat{Z}_k \hat{I}_k e^{-j\delta_i}$$

or

$$\hat{V}_k = \hat{Z}_k \hat{I}_k \quad k = 1, 2, \cdots, b \quad (D.8)$$
Appendix D. Mathematical Model for Multi-machine System

Where \( b \) is the number of the network branches and impedance matrix \( Z_k \) is calculated based on rated angular speed.

Equation (D.8) can be expressed in matrix form

\[
\hat{V}_b = \hat{z}_b \hat{I}_b \tag{D.9}
\]

Where the subscript \( b \) is used to indicate a branch matrix. The inverse of the primitive branch matrix \( \tilde{Z}_b \) exists and is denoted by \( \tilde{Y}_b \), thus

\[
\hat{I}_b = \tilde{y}_b \hat{V}_b \tag{D.10}
\]

Equation (D.10) is expressed in terms of the primitive admittance matrix of a passive network. From network theory the node incidence matrix \( A \) can be constructed which is used to convert (D.10) into a nodal admittance equation

\[
\hat{I} = (A^T \tilde{y}_b A)\hat{V} \triangleq \hat{Y} \hat{V} \tag{D.11}
\]

Where \( \hat{Y} \) is the matrix of short circuit driving point and transfer admittances and

\[
A = [a_{pq}] = 1 \text{ if current in branch } p \text{ leaves node } q
\]

\[
A = [a_{pq}] = -1 \text{ if current in branch } p \text{ enters node } q
\]

\[
A = [a_{pq}] = 0 \text{ if branch } p \text{ is not connected to node } q
\]

with \( p = 1, 2, \ldots, b \) and \( q = 1, 2, \ldots, n \).

Since \( \tilde{Y}^{-1} = \tilde{Z} \) exists,

\[
\hat{V} = \tilde{Y}^{-1} \hat{I} = \tilde{Z} \hat{I} \tag{D.12}
\]

Where \( \tilde{Z} \) is the matrix of the open circuit driving point and transfer impedances of the network.
Appendix D. Mathematical Model for Multi-machine System

D.3 Conversion of Machine Coordinates to System Reference

Consider a voltage $v_{abc}$ at node $i$. The Park’s transformation can be applied to this voltage to obtain $v_{dq}$. From (D.2) this voltage can be expressed in phasor notation as $\tilde{V}_i$, using the rotor of machine $i$ as reference. It can also be expressed to the system reference as $\hat{V}_i$, using the transformation of equation (D.7). Equation (D.7) can be generalised to include all the nodes. Let

$$T = \begin{bmatrix} e^{j\delta_1} & 0 & \cdots & 0 \\ 0 & e^{j\delta_2} & \cdots & 0 \\ \cdots & \cdots & \cdots & \cdots \\ 0 & 0 & \cdots & e^{j\delta_n} \end{bmatrix}, \quad \hat{V} = \begin{bmatrix} V_{Q1} + jV_{D1} \\ V_{Q2} + jV_{D2} \\ \vdots \\ V_{Qi} + jV_{Di} \end{bmatrix}, \quad \check{V} = \begin{bmatrix} V_{q1} + jV_{d1} \\ V_{q2} + jV_{d2} \\ \vdots \\ V_{qn} + jV_{dn} \end{bmatrix} \quad (D.13)$$

Then

$$\hat{V} = T\check{V} \quad (D.14)$$

Thus $T$ is a transformation that transforms the $d$ and $q$ quantities of all machines to the system frame, which is a common frame moving at synchronous speed. The transformation $T$ is orthogonal, i.e.,

$$T^{-1} = T^* \quad (D.15)$$

Therefore, from equation (D.14) and equation (D.15)

$$\hat{V} = T \ast \check{V} \quad (D.16)$$

Similarly for the node currents we get

$$\hat{I} = T\check{I} \quad \check{I} = T \ast \hat{I} \quad (D.17)$$
The relation between machine currents and voltages is:

\[ T \ddot{I} = \check{Y} \check{T} \check{V} \quad (D.18) \]

Premultiplying equation (D.18) by \( T^{-1} \)

\[ \check{I} = T^{-1} \check{Y} \check{T} \check{V} = \check{M} \check{V} \quad (D.19) \]

Where

\[ \check{M} \overset{\Delta}{=} (T^{-1} \check{Y} T) \quad (D.20) \]

and if \( \check{M}^{-1} \) exists,

\[ \check{V} = (T^{-1} \check{Y} T)^{-1} \check{I} = (T^{-1} \check{Z} T) \check{I} \quad (D.21) \]

For a three-machine system, the matrix \( \check{Y} \) of the network is of the form

\[ \check{Y} = \begin{bmatrix} Y_{11} e^{j\theta_1} & Y_{12} e^{j\theta_2} & Y_{13} e^{j\theta_3} \\ Y_{21} e^{j\theta_1} & Y_{22} e^{j\theta_2} & Y_{23} e^{j\theta_3} \\ Y_{31} e^{j\theta_1} & Y_{32} e^{j\theta_2} & Y_{33} e^{j\theta_3} \end{bmatrix} \quad (D.22) \]

\[ T = \begin{bmatrix} e^{j\delta_1} & 0 & 0 \\ 0 & e^{j\delta_2} & 0 \\ 0 & 0 & e^{j\delta_3} \end{bmatrix} \quad T^{-1} = \begin{bmatrix} e^{-j\delta_1} & 0 & 0 \\ 0 & e^{-j\delta_2} & 0 \\ 0 & 0 & e^{-j\delta_3} \end{bmatrix} \quad (D.23) \]

\[ \check{Y} T = \begin{bmatrix} Y_{11} e^{j(\theta_1 + \delta_1)} & Y_{12} e^{j(\theta_1 + \delta_2)} & Y_{13} e^{j(\theta_1 + \delta_3)} \\ Y_{21} e^{j(\theta_2 + \delta_1)} & Y_{22} e^{j(\theta_2 + \delta_2)} & Y_{23} e^{j(\theta_2 + \delta_3)} \\ Y_{31} e^{j(\theta_3 + \delta_1)} & Y_{32} e^{j(\theta_3 + \delta_2)} & Y_{33} e^{j(\theta_3 + \delta_3)} \end{bmatrix} \quad (D.24) \]
Appendix D. Mathematical Model for Multi-machine System

\[ T^{-1} \hat{Y}T \equiv \tilde{M} = \begin{bmatrix} Y_{11}e^{j\theta_{11}} & Y_{12}e^{j(\theta_{12}-\delta_{12})} & Y_{13}e^{j(\theta_{13}-\delta_{13})} \\ Y_{21}e^{j(\theta_{21}-\delta_{21})} & Y_{22}e^{j\theta_{22}} & Y_{23}e^{j(\theta_{23}-\delta_{23})} \\ Y_{31}e^{j(\theta_{31}-\delta_{31})} & Y_{32}e^{j(\theta_{32}-\delta_{32})} & Y_{33}e^{j\theta_{33}} \end{bmatrix} \]  

(D.25)

D.4 Linearised Model for the Network

From equation (D.14) \( \hat{V} = TV \), where \( T \) is defined by equation (D.23) and \( V \) and \( \hat{V} \) are defined by equations (D.4), (D.6) and also from (D.19) \( \hat{I} = \hat{M}\hat{V} \), where \( \hat{M} \) is given by equation (D.20). Linearising equation (D.19)

\[ \hat{I}_\Delta = \hat{M}_0\hat{V}_\Delta + \hat{M}_\Delta \hat{V}_0 \]  

(D.26)

Where \( \hat{M}_0 \) is evaluated at the initial angles \( \delta_{i0}, i = 1, 2, \cdots, n \), and \( \hat{V}_0 \) is the initial value of the vector \( \hat{V} \). Let \( \delta_i = \delta_{i0} + \delta_i \Delta \). Then the matrix \( \hat{M} \) becomes

\[ \hat{M} = \begin{bmatrix} Y_{11}e^{j\theta_{11}} & Y_{12}e^{j(\theta_{12}-\delta_{12}-\delta_{12\Delta})} & Y_{13}e^{j(\theta_{13}-\delta_{13}+\delta_{13\Delta})} \\ Y_{21}e^{j(\theta_{21}-\delta_{210}-\delta_{21\Delta})} & Y_{22}e^{j\theta_{22}} & Y_{23}e^{j(\theta_{23}-\delta_{230}-\delta_{23\Delta})} \\ Y_{31}e^{j(\theta_{31}-\delta_{310}-\delta_{31\Delta})} & Y_{32}e^{j(\theta_{32}-\delta_{320}-\delta_{32\Delta})} & Y_{33}e^{j\theta_{33}} \end{bmatrix} \]  

(D.27)

The general term \( m_{ij} \) of the matrix \( \hat{M} \) is of the form \( Y_{ij}e^{j(\theta_{ij}-\delta_{ij0}-\delta_{ij\Delta})} \), thus

\[ m_{ij} = Y_{ij}e^{j(\theta_{ij}-\delta_{ij0})}e^{-j\delta_{ij\Delta}} \]  

(D.28)

using the relation \( \delta_{ij\Delta} \approx 1, \sin\delta_{ij\Delta} \approx \delta_{ij\Delta} \), the general term can be obtained:

\[ m_{ij} \equiv Y_{ij}e^{j(\theta_{ij}-\delta_{ij0})(1 - j\delta_{ij\Delta})} \]  

(D.29)
Appendix D. Mathematical Model for Multi-machine System

The general term in $\bar{M}_\Delta$ is given by

$$m_{ij\Delta} \equiv -j Y_{ij} e^{j(\theta_{ij} - \delta_{ij\Delta})} \delta_{ij\Delta} \quad (D.30)$$

$$\bar{M}_\Delta \bar{V}_0 =$$

$$-j \begin{bmatrix}
0 & Y_{12} e^{j(\theta_{12} - \delta_{12\Delta})} & Y_{13} e^{j(\theta_{13} - \delta_{13\Delta})} & Y_{23} e^{j(\theta_{23} - \delta_{23\Delta})} \\
Y_{21} e^{j(\theta_{21} - \delta_{21\Delta})} & 0 & Y_{23} e^{j(\theta_{23} - \delta_{23\Delta})} & 0 \\
Y_{31} e^{j(\theta_{31} - \delta_{31\Delta})} & Y_{32} e^{j(\theta_{32} - \delta_{32\Delta})} & 0 & 0
\end{bmatrix} \begin{bmatrix}
\bar{V}_{10} \\
\bar{V}_{20} \\
\bar{V}_{30}
\end{bmatrix} \quad (D.31)$$

and the linearised equation (D.27) becomes

$$\bar{M}_\Delta \bar{V}_0 = -j \begin{bmatrix}
\sum_{k=1}^{3} Y_{1k} e^{j(\theta_{1k} - \delta_{1k\Delta})} \bar{V}_{k0} \delta_{1k\Delta} \\
\sum_{k=1}^{3} Y_{2k} e^{j(\theta_{2k} - \delta_{2k\Delta})} \bar{V}_{k0} \delta_{2k\Delta} \\
\sum_{k=1}^{3} Y_{3k} e^{j(\theta_{3k} - \delta_{3k\Delta})} \bar{V}_{k0} \delta_{3k\Delta}
\end{bmatrix} \quad (D.32)$$

Let $T = T_0 - \delta_{\Delta}$ to compute

$$T_\Delta = j T_0 \delta_{\Delta} \quad \delta_{\Delta} \triangleq diag(\delta_{1\Delta}, \delta_{2\Delta}, \delta_{3\Delta}) \quad (D.34)$$
Appendix D. Mathematical Model for Multi-machine System

\[ M_\Delta = -j(T_0^{-1}\delta_\Delta Y T_0 - T_0^{-1}\bar{\delta} T_0 \delta_\Delta) \] (D.35)

\[ T_0^{-1}\bar{\delta} T_0 \delta_\Delta = \begin{bmatrix} Y_{11}e^{j\theta_{11}} & Y_{12}e^{j(\theta_{12} - \delta_{120})} & Y_{13}e^{j(\theta_{13} - \delta_{130})} \\ Y_{21}e^{j(\theta_{21} - \delta_{210})} & Y_{22}e^{j\theta_{22}} & Y_{23}e^{j(\theta_{23} - \delta_{230})} \\ Y_{31}e^{j(\theta_{31} - \delta_{310})} & Y_{32}e^{j(\theta_{32} - \delta_{320})} & Y_{33}e^{j\theta_{33}} \end{bmatrix} \begin{bmatrix} \delta_{1\Delta} & 0 & 0 \\ 0 & \delta_{2\Delta} & 0 \\ 0 & 0 & \delta_{3\Delta} \end{bmatrix} = \bar{M}_0\delta_\Delta \] (D.36)

\[ T_0^{-1}\delta_\Delta \bar{\delta} T_0 = \begin{bmatrix} Y_{11}e^{j\theta_{11}} \delta_{1\Delta} & Y_{12}e^{j(\theta_{12} - \delta_{120})}\delta_{1\Delta} & Y_{13}e^{j(\theta_{13} - \delta_{130})}\delta_{1\Delta} \\ Y_{21}e^{j(\theta_{21} - \delta_{210})}\delta_{2\Delta} & Y_{22}e^{j\theta_{22}} \delta_{2\Delta} & Y_{23}e^{j(\theta_{23} - \delta_{230})}\delta_{2\Delta} \\ Y_{31}e^{j(\theta_{31} - \delta_{310})}\delta_{3\Delta} & Y_{32}e^{j(\theta_{32} - \delta_{320})}\delta_{3\Delta} & Y_{33}e^{j\theta_{33}} \delta_{3\Delta} \end{bmatrix} = \delta_\Delta \bar{M}_0 \] (D.37)

\[ \bar{M}_\Delta = -j[\delta_\Delta \bar{M}_0 - \bar{M}_0\delta_\Delta] \] (D.38)

\[ \bar{I}_\Delta = \bar{M}_0 \bar{V}_\Delta - j[\delta_\Delta \bar{M}_0 - \bar{M}_0\delta_\Delta]\bar{V}_0 \] (D.39)
Appendix D. Mathematical Model for Multi-machine System

\[ \begin{bmatrix} I_{1\Delta} \\ I_{2\Delta} \\ I_{3\Delta} \end{bmatrix} = \begin{bmatrix} Y_{11}e^{j\theta_{11}} & Y_{12}e^{j(\theta_{12} - \theta_{13})} & Y_{13}e^{j(\theta_{13} - \theta_{12})} \\ Y_{21}e^{j(\theta_{11} - \theta_{21})} & Y_{22}e^{j\theta_{22}} & Y_{23}e^{j(\theta_{23} - \theta_{22})} \\ Y_{31}e^{j(\theta_{11} - \theta_{31})} & Y_{32}e^{j(\theta_{32} - \theta_{31})} & Y_{33}e^{j\theta_{33}} \end{bmatrix} \begin{bmatrix} V'_{1\Delta} \\ V'_{2\Delta} \\ V'_{3\Delta} \end{bmatrix} - jV'_{20}Y_{13}e^{j(\theta_{13} - \theta_{12})} - jV'_{30}Y_{12}e^{j(\theta_{12} - \theta_{13})} - jV'_{20}Y_{13}e^{j(\theta_{13} - \theta_{12})} - jV'_{30}Y_{23}e^{j(\theta_{23} - \theta_{22})} - jV'_{30}Y_{32}e^{j(\theta_{32} - \theta_{31})} \]

[D.40]

\[
V'_{1\Delta} = V'_{2\Delta} = V'_{3\Delta} = 0
\]

\[
\delta_{1\Delta} = \delta_{12\Delta} = \delta_{13\Delta} = \delta_{23\Delta}
\]

D.5 Generator Equations

Generator 2 and 3 (two-axis model) (the subscript \( \Delta \) is omitted, generator 1 has been treated as infinite bus in this case)

\[
\tau'_{q0i}E_{di}' = -E_{di}' - (x_{qi} - x'_{di})I_{qi}
\]

\[
\tau'_{d0i}E_{qi}' = -E_{F}E_{di}' - E_{qi}' + (x_{di} - x'_{di})I_{di}
\]

\[
\tau_{ji}\dot{\omega}_i = T_{mi} - D_i\omega_i - I_{di0}E_{di}' - I_{qi0}E_{qi}' - E_{di0}'I_{di} - E_{qi0}'I_{qi}
\]

\[
\delta'_{1i} = \omega_1 - \omega_i, \quad i = 2, 3
\]

[D.41]
Appendix E

The Input FPL File and the Generated Rule Base

E.1 The Input FPL File

PROJECT FLC
VAR aSpeed
    TYPE float
    MIN -100
    MAX 100
    MEMBER NB
    POINTS -100,1, -75, 1, -50,0
    END
    MEMBER NM
    POINTS -75,0, -50, 1, -25, 0
    END
    MEMBER NS
    POINTS -50,0, -25, 1, 0, 0
    END
    MEMBER Z
    POINTS -25,0, 0, 1, 25, 0
    END
MEMBER PS
POINTS 0,0, 25, 1, 50, 0
END
MEMBER PM
POINTS 25,0, 50, 1, 75, 0
END
MEMBER PB
POINTS 50,0, 75, 1, 100,1
END
END

VAR bAcceleration
  TYPE float
  MIN -1500
  MAX 1500
MEMBER NB
POINTS -1500,1, -1125, 1, -750,0
END
MEMBER NM
POINTS -1125,0, -750, 1, -375, 0
END
MEMBER NS
POINTS -750,0, -375, 1, 0, 0
END
MEMBER Z
POINTS -375,0, 0, 1, 375, 0
END
MEMBER PS
POINTS 0,0, 375, 1, 750, 0
END
MEMBER PM
POINTS 375,0, 750, 1, 1125, 0
END
MEMBER PB
POINTS 750,0, 1125, 1, 1500,1
END

END

END /* Acceleration definition */

VAR Control
    TYPE float
    MIN -800
    MAX 800
    MEMBER NB
    POINTS -800,1, -600, 1, -400,0
END
MEMBER NM
POINTS -600,0, -400, 1, -200, 0
END
MEMBER NS
POINTS -400,0, -200, 1, 0, 0
END
MEMBER Z
POINTS -200,0, 0, 1, 200, 0
END
MEMBER PS
POINTS 0,0, 200, 1, 400, 0
END
MEMBER PM
POINTS 200,0, 400, 1, 600, 0
END
MEMBER PB
POINTS 400,0, 600, 1, 800,1
END
E.2 The Generated Rule Base

RULE Rule0000
  OPTIONS
  ENABLE=“ON”
END
  IF (aSpeed IS NB) AND (bAcceleration IS NS) THEN
    Control=NB
END
RULE Rule0001
  OPTIONS
  ENABLE=“ON”
RULE Rule0002
OPTIONS
ENABLE="ON"

END

IF (aSpeed IS NB) AND (bAcceleration IS Z) THEN
  Control=NB
END

RULE Rule0003
OPTIONS
ENABLE="ON"

END

IF (aSpeed IS NM) AND (bAcceleration IS NS) THEN
  Control=NM
END

RULE Rule0004
OPTIONS
ENABLE="ON"

END

IF (aSpeed IS NM) AND (bAcceleration IS Z) THEN
  Control=NM
END

RULE Rule0005
OPTIONS
ENABLE="ON"

END

IF (aSpeed IS NS) AND (bAcceleration IS NM) THEN
  Control=NB
END
RULE Rule0006
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS NS) AND (bAcceleration IS NS) THEN
    Control=NM
  END
RULE Rule0007
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS NS) AND (bAcceleration IS Z) THEN
    Control=NS
  END
RULE Rule0008
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS NS) AND (bAcceleration IS PS) THEN
    Control=Z
  END
RULE Rule0009
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS NS) AND (bAcceleration IS PM) THEN
    Control=PS
  END
RULE Rule0010
  OPTIONS
  ENABLE="ON"
  END
Appendix E. The Input FPL File and the Generated Rule Base

IF (aSpeed IS Z) AND (bAcceleration IS NM) THEN
  Control=NM
END

RULE Rule0011
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS Z) AND (bAcceleration IS NS) THEN
    Control=NM
  END

RULE Rule0012
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS Z) AND (bAcceleration IS Z) THEN
    Control=Z
  END

RULE Rule0013
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS Z) AND (bAcceleration IS PS) THEN
    Control=PM
  END

RULE Rule0014
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS Z) AND (bAcceleration IS PM) THEN
    Control=PM
  END

RULE Rule0015
OPTIONS
ENABLE="ON"
END

IF (aSpeed IS PS) AND (bAcceleration IS NM) THEN
  Control=NS
END

RULE Rule0016
OPTIONS
ENABLE="ON"
END

IF (aSpeed IS PS) AND (bAcceleration IS NS) THEN
  Control=Z
END

RULE Rule0017
OPTIONS
ENABLE="ON"
END

IF (aSpeed IS PS) AND (bAcceleration IS Z) THEN
  Control=PS
END

RULE Rule0018
OPTIONS
ENABLE="ON"
END

IF (aSpeed IS PS) AND (bAcceleration IS PS) THEN
  Control=PM
END

RULE Rule0019
OPTIONS
ENABLE="ON"
END

IF (aSpeed IS PS) AND (bAcceleration IS PM) THEN
Control=PB
END
RULE Rule0020
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS PM) AND (bAcceleration IS NS) THEN
    Control=Z
  END
RULE Rule0021
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS PM) AND (bAcceleration IS Z) THEN
    Control=PM
  END
RULE Rule0022
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS PM) AND (bAcceleration IS PS) THEN
    Control=PM
  END
RULE Rule0023
  OPTIONS
  ENABLE="ON"
  END
  IF (aSpeed IS PM) AND (bAcceleration IS PM) THEN
    Control=PB
  END
Appendix F

Bibliography
Bibliography


Appendix F. Bibliography


Appendix F. Bibliography


Appendix F. Bibliography


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Appendix G

Turbo Pascal Source Code For
Single-Machine Infinite Bus Power System
Program response(Input,Output);
uses crt,dos,auxinout,dt2801,scnplt5;

Const
  dtconv=204.8;
  number_points=800;
  norm_color=red;
  chan=0;
  chan1=1;
  chan2=2;
  chan3=3;
  chan4=4;
  alt_color=cyan;
  console : boolean  =  false;
  print : boolean  =  true;
  car_ret = AM;
  NormalTimer=0; {Constants for interrupt}
  OneMillisecond=1179;
  TenMillisecond=11790;
  TimerInt=$08;

  type
    line_string=string[70];
    output_array=array[1..number_points] of real;
    string19=string[19];

Var
  { Variables for main program }
  v_out:output_array;
  control_array,power_array,speed_array:output_array;
  angle_array,angle1_array,time_array:output_array;
  inerror,outerror:array [1..2] of byte;
  op_dev : text;
repeatprocess,first_time,returnmenu,quit_f :boolean;
voltage,current,voltage1,uk,uk_1,plant_input,control_output, uf,uf_1 :real;
plus,rnum,xmax,ymin,ymax,sample_time,timer,power_factor :real;
plant_input,plant_input1,ref,error_signal,umax,umin,e_array_1,e_array : real;
angle,angle_0,angle_1,op,op_1,ip,angle_old,angular_speed_1,angular_speed :real;
pss,pss_1,pss_2,pss_3,speed,speed_1,a_speed,a_speed_1,a_speed_2,a_speed_3:real;
number_waits,wait,temp,index,IDX,IDY,da_data,da_data1,i,ad_data,count :integer;
ad_data1,ad_data2,ad_data3 :integer;
uk_2,uk_3,uk_4,uk_5,uk_6,uk_7,uk_8,uk_9,uk_10,uk_11,uk_12 :real;
ask,kb_cuar,reply :char;
Dr,Dk,Gk,Us,Pk,Usmax,acce,theta,x,y,power_voltage,power_current,power_angle :real;
op_6,op_5,op_4,op_3,op_2,ip_6,ip_5,ip_4,ip_3,ip_2,ip_1,: real;
uf_4,uf_3,uf_2: real;
plant_input4,plant_input3,plant_input2 :real;
anguspeed,anguspeed_1,anguspeed_2,anguspeed_3,anguspeed_4: real;
speed_4,speed_3,speed_2:real;
outf :text;
Clicks: Word; { For interrupt Procedure}

OldVector: Pointer;
key: Char;

{/PA}

{******************************************************Procedure for Interrupt ******************************************************}

Procedure TimerClick ;Interrupt;
Var
  Regs: Registers;
Begin
  Inc(Clicks);
  port[$20]:=$20;
End;
Procedure SetTimerPeriod (N : Word);
Var
Appendix G. Turbo Pascal Source Code For SMIB Power System

A: Integer;

Begin
  port[$43]:=$36;
  Inc(A);
  Port[$40]:=Lo (N);
  Inc(A);
  Port[$40]:=Hi (N);
End;

Procedure InitTimer;

Begin
  GetIntVec(TimerInt,OldVector);
  SetIntVec(TimerInt,@TimerClick);
  SetTimerPeriod (OneMilliSecond);
  Clicks:=0;
End;

Procedure RestoreTimer;

Begin
  SetTimerPeriod (NormalTimer);
  SetIntVec(TimerInt,Oldvector);
End;

{ ************* Read Analog Voltage From Specified Channel ************* }

Procedure ad_read;

var
  ad_data,ad_data1,ad_data2,ad_data3,m,status,gain,dummy:integer;
  ad_data4.chan,chan1,chan2,chan3,chan4: integer;

begin
  chan:=0;
  chan1:=1;
  chan2:=2;
  chan3:=3;
  chan4:=4;
  gain:=0;
dummy := 0;
adstp;
rdadi(gain, chan, ad_data, status); {channel 0 terminal voltage}  
rdadi(gain, chan1, ad_data1, status); {channel 1 rotor angle}  
rdadi(gain, chan2, ad_data2, status); {channel 2 voltage}  
rdadi(gain, chan3, ad_data3, status); {channel 3 current}  
rdadi(gain, chan4, ad_data4, status); {channel 4 power angle}  
voltage := ad_data/204.8; {convert digital voltage to analogue}  
plant_output := voltage/5; {convert to reference voltage, (400v:5v)}  
ip := ad_data1/204.8;  
op := 1.627*op_1 - 1.89031*op_2 + 1.07761*op_3 - 0.46637*op_4 + 0.08469*op_5  
- 0.0123*op_6 + 0.0550073*(ip + 1.0491*ip_1 + 2.19433*ip_2 + 2.05156*ip_3  
+ 2.19433*ip_4 + 1.0491*ip_5 + 1*ip_6);  
op_6 := op_5;  
op_5 := op_4;  
op_4 := op_3; \{use 6th order Chebyshev I filter to filter from angle signal\}  
op_3 := op_2;  
op_2 := op_1;  
op_1 := op;  
ip_6 := ip_5;  
ip_5 := ip_4;  
ip_4 := ip_3;  
ip_3 := ip_2;  
ip_2 := ip_1;  
ip_1 := ip;  
angle := op;  
speed := (angle - angle_1)/(0.025*314); \{calculate speed from measured rotor angle\}  
angle_1 := angle;  
power.voltage := ad_data2/204.8;  
power.current := ad_data3/204.8; \{convert digital current to analogue\}  
power.angle := ad_data4/204.8;  
end;
Appendix G. Turbo Pascal Source Code For SMIB Power System

************Fuzzy Logic Based Power System Stabiliser ***************

Procedure pssf;
begin
  Dr:=2;
  Usmax:=0.4;
  anguspeed:=1.0586*anguspeed_1-0.98622*anguspeed_2+0.389485*anguspeed_3
  -0.0789937*anguspeed_4+0.0385299*(speed+4*speed_1+6*speed_2
  +4*speed_3+speed_4);
  anguspeed_4:=anguspeed_3;
  {use 4th order Chebyshev.I filter to filter noise from angle signal}
  anguspeed_3:=anguspeed_2;
  anguspeed_2:=anguspeed_1;
  anguspeed_1:=anguspeed;
  speed_4:=speed_3;
  speed_3:=speed_2;
  speed_2:=speed_1;
  speed_1:=speed;
  angular_speed:=anguspeed;
  acce:=(angular_speed-angular_speed_l)/0.025; {calculate acceleration signal}
  Dk:=sqrt(angular_speed*angular_speed-acce*acce);
  if Dk<Dr then Gk:=Dk/Dr
  else Gk:=1;
  angular_speed_1:=angular_speed;
  x:=angular_speed;
  y:=acce;
  if x=0 then x:=0.0000001;
  if x>0 then
    if y>0 then theta:=arctan(y/x)
    else theta:=2*3.1415926+arctan(y/x);
  if x<0 then theta:=3.1415926+arctan(y/x);
  if theta<1.658 then Pk:=0;
  if theta<1.91986 then

if theta>1.658 then
    Pk:=7.2951*(theta-1.658)*(theta-1.658);
if theta<=2.18166 then
    if theta>1.91986 then
        Pk:=1-7.2951*(theta-2.18166)*(theta-2.18166);
    if theta<4.7996 then
        if theta>2.18166 then
            Pk:=1;
        if theta<5.06145 then
            if theta>4.7996 then
                Pk:=1-7.2951*(theta-4.7996)*(theta-4.7996);
            if theta<5.32325 then
                if theta>5.06145 then
                    Pk:=7.2951*(theta-5.32325)*(theta-5.32325);
                if theta>5.32325 then
                    Pk:=0;
    Us:=Gk*Usmax*(1-2*Pk);
pss:=Us;
end;

{******************** Automatic Voltage Regulator ***********************}
Procedure controller;
begin
    error_signal:=ref+pss-plant_output;
e:=error_signal;
plant_input:=(0.1467*uk_1)+(0.1304*uk_2)+(0.1160*uk_3)+(0.1031*uk_4)
            +(0.0917*uk_5)+(0.0815*uk_6)+(0.0725*uk_7)+(0.0644*uk_8)
            +(0.0573*uk_9)+(0.0509*uk_10)+(0.0453*uk_11)+(0.0402*uk_12)
            +(50*((5.0586*e)+(0*e_1)+(0*e_2)+(0*e_3)+(0*e_4)
            +(0*e_5)+(0*e_6)+(0*e_7)+(0*e_8)+(0*e_9)
            +(0*e_10)+(0*e_11)+(-1.2345*e_12));
uk:=plant_input;
uk_12:=uk_11;
uk_11:=uk_10;
uk_10:=uk_9;
uk_9:=uk_8;
uk_8:=uk_7;
uk_7:=uk_6;
uk_6:=uk_5;
uk_5:=uk_4;
uk_4:=uk_3;
uk_3:=uk_2;
uk_2:=uk_1;
uk_1:=uk;
e_12:=e_11;
e_11:=e_10;
e_10:=e_9;
e_9:=e_8;
e_8:=e_7;
e_7:=e_6;
e_6:=e_5;
e_5:=e_4;
e_4:=e_3;
e_3:=e_2;
e_2:=e_1;
e_1:=e;
if(uk>9.9) then uk:=9.9; {DT2801 A/D and D/A converter limit 10}
if(uk<-9.9) then uk:=-9.9;
end;

{ ************ Output an Analog Voltage on Specified Channel ************ }
Procedure da_write;
var
    chan,dummy,status :integer;
begin
    chan:=0;
    control_output:=uk*204.8;
da_data:=round(control_output); {convert analog to digital}
wrdai(chan, da.data, dummy, status);
end;

Procedure da_write1;
var
  chan1, dummy, status : integer;
begin
  chan1 := 1;
  for i := 1 to 10 do
    begin
      plus := 5 * 204.8;
      da.data1 := round(plus);
      wrdai(chan1, da.data1, dummy, status);
    end;
end;

Procedure da_write0;
var
  chan1, dummy, status : integer;
begin
  chan1 := 1;
  for i := 1 to 10 do
    begin
      plus := 0 * 204.8;
      da.data1 := round(plus);
      wrdai(chan1, da.data1, dummy, status);
    end;
end;

{*******************************************************************************
Scale*******************************************************************************}

Procedure testr;
var
  xply, rtmp : real;
  icnt : integer;
begin

icnt:=0;
xply:=0.1;
while rnum>0.001 do
begin
   rnum:=rnum*xply;
   icnt:=icnt+1;
end;
rtmp:=0.001;
if(rnum>0.0001)then rtmp:=0.0002;
if(rnum>0.0002)then rtmp:=0.00025;
if(rnum>0.00025)then rtmp:=0.0005;
if(rnum>0.0005)then rtmp:=0.001;
if(icnt>0) then
   begin
      for index:=1 to icnt do
      rtmp:=rtmp/xply;
      rnum:=rtmp;
   end
else
   rnum:=rtmp;
end; {testr}
{******************************************************************************}
Procedure graphresults;
begin
   clearplotdata;
   plotlabel('time (sec)', 'plant output', 'System Response');
   plotdata(time_array,v_out,number_points,curve);
   plotdata(time_array,control_array,number_points,curve);
   plotdata(time_array,angle_array,number_points,curve);
   plotdata(time_array,power_array,number_points,curve);
   plotdata(time_array,speed_array,number_points,curve);
   plotgraph;
end;
Procedure hardcopy;
var
  xfactor, yfactor, scalex, scaley, adds, increment: real;
  ix, iy, increm, itemp, ixtk, yup, ydn, ilim, ixof, iyof, i, xx, yy: integer;
  iyy: integer;
  xact, yact: real;
  iend: char;
  com1: text;
begin
  assignaux(com1, 0, $E7);
  rewrite(com1);
  xfactor := 9000/xmax; {scale factor for Hp}
  yfactor := 7000/(ymax-ymin);
  ix := 1000; {seems good place for origin}
  iy := 1000-round(ymin*yfactor);
  scalex := 800/xfactor; {find scale value for 2cm}
  rnum := scalex; {get nice number for scale}
  testr;
  scalex := rnum;
  scaley := 800/yfactor;
  rnum := scaley;
  testr;
  scaley := rnum;
  writeln(com1, 'IN;SP1;PAPU', ix, ',', iy, ';'); {start plotter}
  increm := 400; {1 cm ticks}
  itemp := ix;
  ixtk := 0;
  repeat
    writeln(com1, 'PRPD', increm, ',', 0, ',XT;'); {plot x axis with ticks}
    itemp := itemp + increm;
    ixtk := ixtk + 1;
Appendix G. Turbo Pascal Source Code For SMIB Power System

until (itemp ≥ 9300);
itemp:=iy;
yup:=0;
writeln(com1,'PAPU',ix, ',', iy, ';');  { return pen to origin}
repeat
    writeln(com1,'PRPDO,',increm,'YT;');  { positive y axis now}
    itemp:=itemp+increm;
yup:=yup+1;
until (itemp ≥ 7500);
writeln(com1,'PAPU',ix, ',', iy, ';');
itemp:=iy;
ydn:=0;
increm:=-400;
repeat
    writeln(com1,'PRPDO,',increm,'YT;');  { negative y axis}
    itemp:=itemp-hincrem;
ydn:=ydn+h 1;
until (itemp ≤ 2000);
iend:=char(3);
xact:=scalex;
yact:=scaley;
writeln(com1,'PAPU',ix, ',', iy, ';SI;DIO,l;');  {start printing scale}
iyof:=iy-720;
increm:=800;
ilim:=round(ixtk/2 -1);
if (ixtk>2) then
begin
    for i:=1 to ilim do
    begin
        ixof:=ix-(i*increm)+40;
writeln(com1,'PAPU',ixof, ',', iyof, ';LB',xact:4:2,iend);
xact:=xact+scalex;
    end
end;
end;
end;
ixof:=ix-750;
writeln(com1,'D11,0;');
ilim:=round(yup/2);
if (yup>2) then
begin
  for i:=1 to ilim do
  begin
    iyof:=(increm*i)-fy-40;
    writeln(com1,'PAPU',ixof,',',iyof,';LB',yact:4:2,iend);
    yact:=yact+scaley;
  end;
end;
yact:=-scaley;
ilim:=round(ydn/2);
if (ydn>2) then
begin
  for i:=1 to ilim do
  begin
    iyof:=iy-(increm*i)-40;
    writeln(com1,'PAPU',ixof,',',iyof,';LB',yact:4:2,iend);
    yact:=yact-scaley;
  end;
end;

writeln(com1,'PAPU',ixof,',',iy,';LB0.00',iend);
writeln(com1  ,'PAPU5000,7000;LB SYSTEM RESPONSE WITH AVR AND PSS',iend);
iyy:=iy+round(800/scaley*v_out[l]);
writeln(com1,'SP2;PAPU',ix,',',iyy);
for i:=1 to number_points do
begin
xx:=ix+round(800/scalex * time_array[i]);
yy:=iy+round(800/scaley * v_out[i]);
writeln(com1,'PAPD',xx,',',yy,';');
increment:=increment+adds;
end;
iyy:=iy+round(800/scaley*control_array[1]);
writeln(com1,'SP3;PAPU',ix,',',iyy);
for i:=1 to number_points do
begin
xx:=ix+round(800/scalex * time_array[i]);
yy:=iy+round(800/scaley * control_array[i]);
writeln(com1,'PAPD',xx,',',yy,';');
increment:=increment+adds;
end;
iyy:=iy+round(800/scaley*angle_array[1]);
writeln(com1,'SP4;PAPU',ix,',',iyy);
for i:=1 to number_points do
begin
xx:=ix+round(800/scalex * time_array[i]);
yy:=iy+round(800/scaley * angle_array[i]);
writeln(com1,'PAPD',xx,',',yy,';');
increment:=increment+adds;
end;
iyy:=iy+round(800/scaley*power_array[1]);
writeln(com1,'SP4;PAPU',ix,',',iyy);
for i:=1 to number_points do
begin
xx:=ix+round(800/scalex * time_array[i]);
yy:=iy+round(800/scaley * power_array[i]);
writeln(com1,'PAPD',xx,',',yy,';');
increment:=increment+adds;
end;
writeLn(com1,'IN;PU,SP0;');
close(com1);
end;

{********************* Display Instructions *********************}

Procedure display_insts;
begin
  clrscr;
textcolor(lightgray);
gotoxy(20,5);write('<<<<<<< >>>>>>>');
gotoxy(20,6);write('<<<<<<< >>>>>>>');
gotoxy(20,7);write('<<<<<<< >>>>>>>');
gotoxy(28,5);
textcolor(lightgreen);write('MEASUREMENT OF STEP RESPONSE');
textcolor(green);
gotoxy(28,7);write('Set_up Instructions for IBM');
if first_time then
begin
  textcolor(alt_color);
gotoxy(20,12);write('[1]');
textcolor(norm_color);
  write('connect system output to A/D channel 0,1 and 2');
gotoxy(20,15);
textcolor(alt_color);write('[2]');
textcolor(norm_color);
  write('connect D/A channel 0 to plant input');
gotoxy(20,18);
textcolor(alt_color);write('[3]');
textcolor(norm_color);
  write('press ENTER key to continue....');
repeat
  kb_char:=readkey;
until kb_char = car_ret;
 Appendix G. Turbo Pascal Source Code For SMIB Power System

```pascal
first_time := false;
end;
textcolor(yellow);
clrscr;
gotoxy(17,8);write('Sample time is 25 milliseconds ');
gotoxy(17,10);
write('Enter reference -> ');
readln(ref);
repeat
gotoxy(17,18);
write('Enter final time of plot, minimum is 5 secs -> ');
readln(xmax);
until xmax>5.0;
clrscr;
gotoxy(15,17);writeln('WAIT - Response being measured ...');
gotoxy(15,19);
writeln('Press any key to perform sudden load change and collect data...');
end;
{display_insts}
{************************************************************************Set Menu************************************************************************}
Procedure read_menu;
var
  kb_char : char;
begin
  repeatprocess := false;
  returnmenu := false;
  repeat
    kb_char:=readkey;
    kb_char := upcase(kb_char);
  until kb_char in ['G','Q','R','H'];
case kb_char of
  'H': begin
```
hardcopy;
returnmenu := true;
end;
'R': repeatprocess := true;
'Q': begin
clrscr;
end;
'G': begin
graphresults;
clrscr;
returnmenu := true;
end;
end;
end;

Procedure output_menu;
begin
textcolor(lightgray);
gotoxy(20,5);write('<<<<« OUTPUT MENU »>>>>');
textcolor(red);
gotoxy(20,8);write('G');textcolor(green);write('raph of results on screen');
textcolor(red);
gotoxy(20,10);write('H');textcolor(green);write('ardcopy of plot');
gotoxy(20,12);textcolor(red);
gotoxy(20,14);write('S');textcolor(green);write('creen listing of graph data');
textcolor(red);
gotoxy(20,16);write('P');textcolor(green);write('rinter listing of graph data');
textcolor(red);
gotoxy(20,18);write('R');textcolor(green);write('epeat test Procedure');
textcolor(red);
gotoxy(20,20);write('Q');textcolor(green);write('uit resp.com program');
textcolor(lightgray);
gotoxy(20,21); write('Enter highlighted letter option...');
Appendix G. Turbo Pascal Source Code For SMIB Power System

read_menu;

textcolor(norm_color);
end;

 /*************************************************************************
 * Main Program **********************************************************/

var

status, dummy: integer;

Begin

clrscr;

writeln('Please wait for a while ...');
delay(5000);
InitTimer;
assign(outf, 'c:/tp/vflpss.shi');
rewrite(outf);
first time := true;
xmax := 5;
repeat

clrscr;
ref := 0;
ip_6 := 0; ip_5 := 0; ip_4 := 0; ip_3 := 0; ip_2 := 0; ip := 0;
op_6 := 0; op_5 := 0; op_4 := 0; op_3 := 0; op_2 := 0; op_1 := 0; op := 0;
uf_4 := 0; uf_3 := 0; uf_2 := 0; uf_1 := 0;
plant_input4 := 0; plant_input3 := 0; plant_input2 := 0; plant_input1 := 0;
error signal := 0; voltage := 0;
speed := 0; speed_1 := 0; speed_2 := 0; speed_3 := 0; speed_4 := 0;
anguspeed := 0; anguspeed_1 := 0; anguspeed_2 := 0; anguspeed_3 := 0;
anguspeed_4 := 0; angular_speed := 0; angular_speed_1 := 0;
a_speed := 0; a_speed_1 := 0; a_speed_2 := 0; a_speed_3 := 0;
angle := 0; angle_0 := 0; angle_1 := 1;
pss := 0; pss_1 := 0; pss_2 := 0; pss_3 := 0;
power_voltage := 0; power_current := 0; power_angle := 0;
for i := 1 to number_points do

begin
v_out[i]:=0;
control_array[i]:=0;
angle_array[i]:=0;
angle1_array[i]:=0;
power_array[i]:=0;
time_array[i]:=0;
speed_array[i]:=0;
end;
uf:=0; uf:=0;
plant_input1:=0;
uk:=0; uk.1:=0; uk.2:=0; uk.3:=0; uk.4:=0; uk.5:=0; uk.6:=0;
uk.7:=0; uk.8:=0; uk.9:=0; uk.10:=0; uk.11:=0; uk.12:=0;
e:=0; e.1:=0; e.2:=0; e.3:=0; e.4:=0; e.5:=0; e.6:=0;
e.7:=0; e.8:=0; e.9:=0; e.10:=0; e.11:=0; e.12:=0;
acce:=0;
angular_speed:=0; angular_speed.1:=0;
Dr:=0; Dk:=0; Gk:=0; Us:=0; Pk:=0;
theta:=0; x:=0; y:=0; plant_output:=0;
display_insts;
if clicks>=25 then
begin
   Clicks:=0;
ad_read;
pssf;
controller;
da_write;
end;
repeat
if clicks>=25 then
   clicks:=0;
ad_read;
pssf;
controller;
da_write;
end;
until keypressed;
if clicks≥25 then
begin
  clicks:=0;
ad_read;
pssf;
controller;
da_write;
v.out[1]:=plant_output*5;
power_facter:=cos(power_angle*3.14159/18);
power_array[1]:=(3*power_current*power_voltage*power_facter)/10;
control_array[1]:=uk;
angle_array[1]:=angle;
speed_array[1]:=angular.speed;
time_array[1]:=0;
end;
for i:=2 to 200 do
begin
  repeat until clicks≥25;
  clicks:=0;
ad_read;
pssf;
controller;
da_write;
v.out[i]:=plant_output*5;
power_facter:=cos(power_angle*3.14159/18);
power_array[i]:=(3*power_current*power_voltage*power_facter)/10;
control_array[i]:=uk;
angle_array[i]:=angle;
speed_array[i]:=angular_speed;
time_array[i]:=0.025+time_array[i-1];
end;
da_write1; {produce signal to operate the relay}
for i:=201 to 500 do
begin
  repeat until clicks>=25;
  clicks:=0;
ad_read;
pssf;
controller;
da_write;
v_out[i]:=plant_output*5;
power_facter:=cos(power_angle*3.14159/18);
power_array[i]:(3*power_current*power_voltage*power_facter)/10;
control_array[i]:=uk;
angle_array[i]:=angle;
speed_array[i]:=angular_speed;
time_array[i]:=0.025+time_array[i-1];
end;
da_write0;
for i:=501 to number_points do
begin
  repeat until clicks>=25;
  clicks:=0;
ad_read;
pssf;
controller;
da_write;
v_out[i]:=plant_output*5;
power_facter:=cos(power_angle*3.14159/18);
power_array[i]:(3*power_current*power_voltage*power_facter)/10;
Appendix G. Turbo Pascal Source Code For SMIB Power System

```pascal
control_array[i]:=uk;
angle_array[i]:=angle;
speed_array[i]:=angular_speed;
time_array[i]:=0.025+time_array[i-1];
end;
for i:=1 to 200 do
begin
  repeat until clicks>=25;
  clicks:=0;
ad_read;
pssf;
controller;
da_write;
end;
RestoreTimer;
for i:=1 to number_points do
begin
  writeln(outf,time_array[i],',',v_out[i],',',control_array[i],',',
  power_array[i],',',angle_array[i],',',speed_array[i]);
end;
ymax:=10;
ymin:=-4;
for index:=1 to number_points do
begin
  if v_out[index]>ymax then ymax:=v_out[index];
  if v_out[index]<ymin then ymin:=v_out[index];
  if control_array[index]>ymax then
      ymax:=control_array[index];
  if control_array[index]<ymin then
      ymin:=control_array[index];
  if angle1_array[index]>ymax then
      ymax:=angle1_array[index];
```

if angle1_array[index]<ymin then
    ymin:=angle1_array[index];
end;
if ymin>0 then ymin:=-4;
repeatprocess := false;
returnmenu := false;
repeat
    clrscr;
    output_menu;
    until not returnmenu;
    until not repeatprocess;
close(outf);
    RestoreTimer;
end.